

200MHz Slew Enhanced VFA

The EL5100, EL5101, and EL5300 represent high-speed voltage feedback amplifiers based on the current feedback amplifier architecture. This gives the typical high slew rate benefits of a CFA family along with the stability and ease of use associated with the VFA type architecture. This family is available in single, dual, and triple versions, with 200MHz, 400MHz, and 700MHz versions. This family operates on single 5V or $\pm 5V$ supplies from minimum supply current. The EL5100 and EL5300 also feature an output enable function, which can be used to put the output in to a high-impedance mode. This enables the outputs of multiple amplifiers to be tied together for use in multiplexing applications.

Ordering Information

PART NUMBER	PACKAGE	TAPE & REEL	PKG. DWG. #
EL5100IS	8-Pin SO	-	MDP0027
EL5100IS-T7	8-Pin SO	7"	MDP0027
EL5100IS-T13	8-Pin SO	13"	MDP0027
EL5100IW-T7	6-Pin SOT-23	7" (3K pcs)	MDP0038
EL5100IW-T7A	6-Pin SOT-23	7" (250 pcs)	MDP0038
EL5101IC-T7	SC-70	7" (3K pcs)	
EL5101IC-T7A	SC-70	7" (250 pcs)	
EL5101IW-T7	5-Pin SOT-23	7" (3K pcs)	MDP0038
EL5101IW-T7A	5-Pin SOT-23	7" (250 pcs)	MDP0038
EL5300IU	16-Pin QSOP	-	MDP0040
EL5300IU-T7	16-Pin QSOP	7"	MDP0040
EL5300IU-T13	16-Pin QSOP	13"	MDP0040
EL5300IUZ (See Note)	16-Pin QSOP (Pb-free)	-	MDP0040
EL5300IUZ-T7 (See Note)	16-Pin QSOP (Pb-free)	7"	MDP0040
EL5300IUZ-T13 (See Note)	16-Pin QSOP (Pb-free)	13"	MDP0040

NOTE: Intersil Pb-free products employ special Pb-free material sets; molding compounds/die attach materials and 100% matte tin plate termination finish, which is compatible with both SnPb and Pb-free soldering operations. Intersil Pb-free products are MSL classified at Pb-free peak reflow temperatures that meet or exceed the Pb-free requirements of IPC/JEDEC J STD-020C.

Features

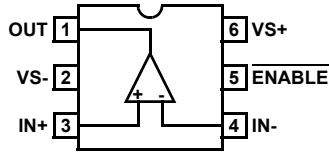
- Pb-free available as an option
- Specified for 5V or $\pm 5V$ applications
- Power-down to 17 μA /amplifier
- -3dB bandwidth = 200MHz
- ± 0.1 dB bandwidth = 20MHz
- Low supply current = 2.5mA
- Slew rate = 2200V/ μs
- Low offset voltage = 4mV max
- Output current = 100mA
- $A_{VOL} = 1000$
- Diff gain/phase = 0.08%/0.1°

Applications

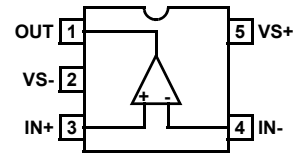
- Video amplifiers
- PCMCIA applications
- A/D drivers
- Line drivers
- Portable computers
- High speed communications
- RGB applications
- Broadcast equipment
- Active filtering

Pinouts

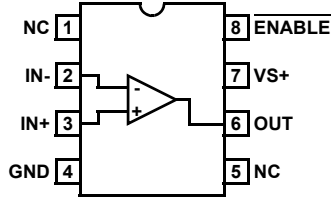
EL5100
(6-PIN SOT-23)
TOP VIEW



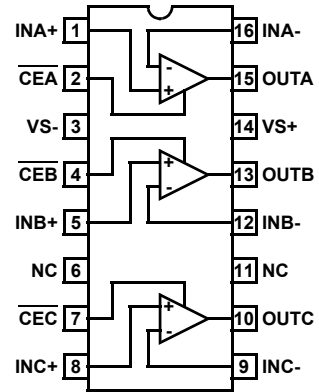
EL5101
(5-PIN SOT-23)
TOP VIEW



EL5100
(8-PIN SO)
TOP VIEW



EL5300
(16-PIN QSOP)
TOP VIEW



Absolute Maximum Ratings (T_A = 25°C)

Supply Voltage between V_{S+} and GND. 13.2V
 Input Voltage ±V_S
 Differential Input Voltage ±4V
 Maximum Output Current. 80mA

Storage Temperature Range -65°C to +150°C
 Ambient Operating Temperature Range -40°C to +85°C
 Operating Junction Temperature 150°C

CAUTION: Stresses above those listed in "Absolute Maximum Ratings" may cause permanent damage to the device. This is a stress only rating and operation of the device at these or any other conditions above those indicated in the operational sections of this specification is not implied.

IMPORTANT NOTE: All parameters having Min/Max specifications are guaranteed. Typical values are for information purposes only. Unless otherwise noted, all tests are at the specified temperature and are pulsed tests, therefore: T_J = T_C = T_A

DC Electrical Specifications V_S = ±5V, GND = 0V, T_A = 25°C, V_{CM} = 0V, V_{OUT} = 0V, V_{ENABLE} = GND or OPEN, unless otherwise specified.

PARAMETER	DESCRIPTION	CONDITIONS	MIN	TYP	MAX	UNIT
V _{OS}	Offset Voltage		-4	1	4	mV
TCV _{OS}	Offset Voltage Temperature Coefficient	Measured from T _{MIN} to T _{MAX}		8		μV/°C
I _B	Input Bias Current	V _{IN} = 0V	-6	2	6	μA
I _{OS}	Input Offset Current	V _{IN} = 0V	-2.5	0.5	2.5	μA
TCI _{OS}	Input Bias Current Temperature Coefficient	Measured from T _{MIN} to T _{MAX}		8		nA/°C
PSRR	Power Supply Rejection Ratio		70	90		dB
CMRR	Common Mode Rejection Ratio	V _{CM} from -3V to +3V	60	75		dB
CMIR	Common Mode Input Range	Guaranteed by CMRR test	-3		+3	V
R _{IN}	Input Resistance	V _{IN} = -3V to +3V	0.7	1.2		MΩ
C _{IN}	Input Capacitance			1		pF
I _{S,ON}	Supply Current - Enabled	Per amplifier	2.1	2.5	2.9	mA
I _{S,OFF}	Supply Current - Shut Down	V _{S+} , per amplifier	-5	0	5	μA
		V _{S-} , per amplifier	5	17	25	μA
PSOR	Power Supply Operating Range		3.3		12	V
AVOL	Open Loop Gain	R _L = 1kΩ to GND, V _{OUT} from -2.5V to +2.5V	55	60		dB
V _{OP}	Positive Output Voltage Swing	R _L = 150Ω to GND	3.2	3.4		V
		R _L = 1kΩ to GND	3.6	3.8		V
V _{ON}	Negative Output Voltage Swing	R _L = 150Ω to GND		-3.4	-3.2	V
		R _L = 1kΩ to GND		-3.8	-3.6	V
I _{OUT}	Output Current	R _L = 10Ω to 0V	±60	±100		mA
V _{IH-EN}	ENABLE pin Voltage for Power Up		V _{S+} -4			V
V _{IL-EN}	ENABLE pin Voltage for Shut Down				V _{S+} -1	V
I _{EN}	Enable Pin Current	Enabled, V _{EN} = 0V	-1		1	μA
		Disabled, V _{EN} = 5V	5	17	25	μA

Closed Loop AC Electrical Specifications $V_S = \pm 5V$, $T_A = 25^\circ C$, $V_{ENABLE} = 0V$, $A_V = +1$, $R_F = 0\Omega$, $R_L = 150\Omega$ to GND, unless otherwise specified.

PARAMETER	DESCRIPTION	CONDITIONS	MIN	TYP	MAX	UNIT
BW	-3dB Bandwidth ($V_{OUT} = 200mV_{P-P}$)	$V_S = \pm 5V$, $A_V = 1$, $R_F = 0\Omega$	150	200		MHz
SR	Slew Rate	$R_L = 100\Omega$, $V_{OUT} = -3V$ to $+3V$, $A_V = +2$	1500	2200	4500	V/ μs
t_R, t_F	Rise Time, Fall Time	$\pm 0.1V$ step		2.8		ns
OS	Overshoot	$\pm 0.1V$ step		10		%
t_{PD}	Propagation Delay	$\pm 0.1V$ step		3.2		ns
t_S	0.1% Settling Time	$V_S = \pm 5V$, $R_L = 500\Omega$, $A_V = 1$, $V_{OUT} = \pm 2.5V$		20		ns
dG	Differential Gain	$A_V = 2$, $R_L = 150\Omega$, $V_{INDC} = -1$ to $+1V$		0.08		%
dP	Differential Phase	$A_V = 2$, $R_L = 150\Omega$, $V_{INDC} = -1$ to $+1V$		0.1		$^\circ$
e_N	Input Noise Voltage	$f = 10kHz$		10		nV/ $\sqrt{Hz}$
i_N	Input Noise Current	$f = 10kHz$		7		pA/ $\sqrt{Hz}$
t_{DIS}	Disable Time			180		ns
t_{EN}	Enable Time			650		ns

Typical Performance Curves

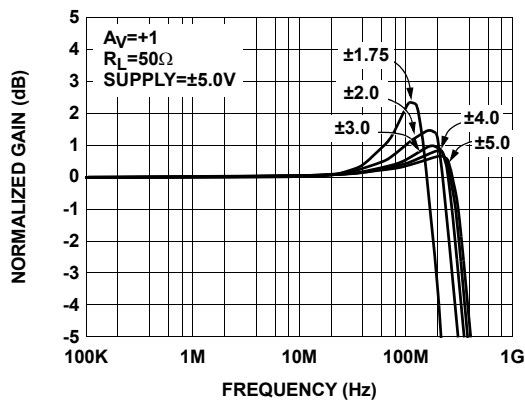


FIGURE 1. GAIN vs FREQUENCY FOR VARIOUS C_L

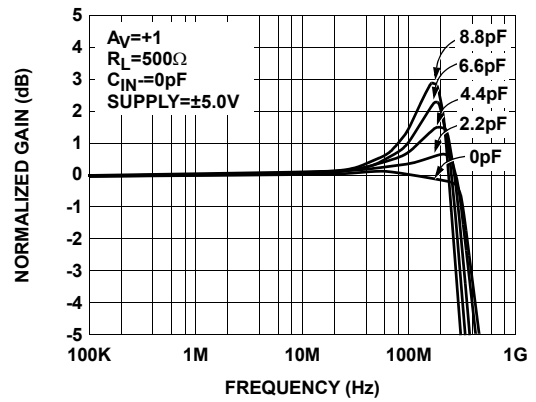


FIGURE 2. GAIN vs FREQUENCY FOR VARIOUS C_L

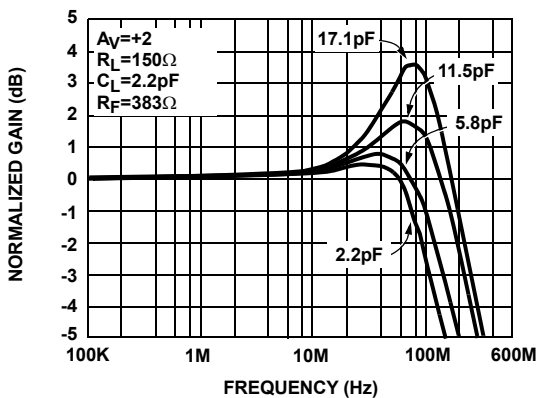


FIGURE 3. GAIN vs FREQUENCY FOR VARIOUS C_{IN}

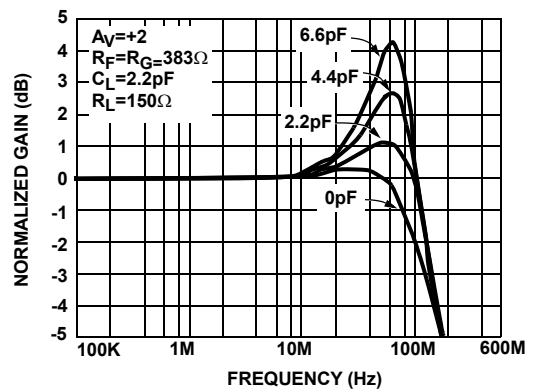


FIGURE 4. GAIN vs FREQUENCY FOR VARIOUS C_{IN}

Typical Performance Curves (Continued)

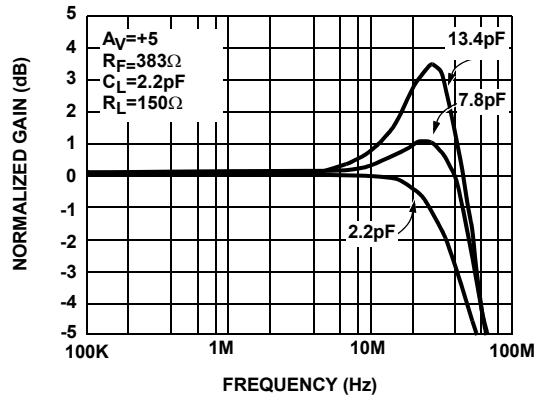


FIGURE 5. GAIN vs FREQUENCY FOR VARIOUS C_{IN} (-)

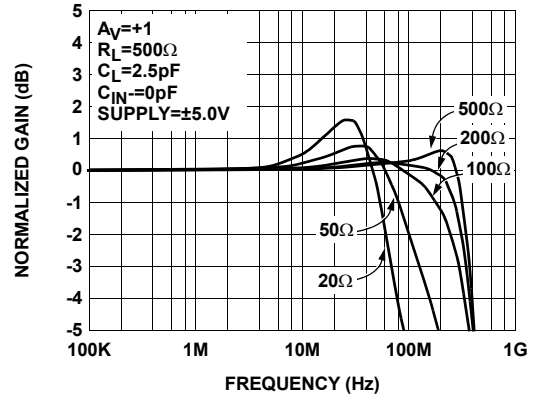


FIGURE 6. GAIN vs FREQUENCY FOR VARIOUS R_L

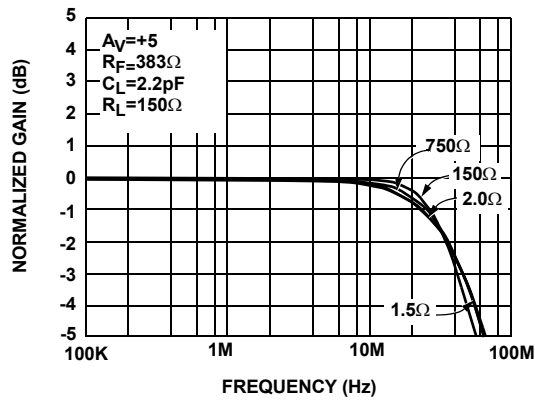


FIGURE 7. GAIN vs FREQUENCY FOR VARIOUS R_L

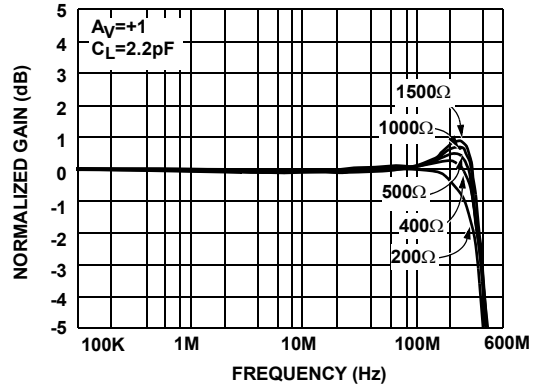


FIGURE 8. GAIN vs FREQUENCY FOR VARIOUS R_L

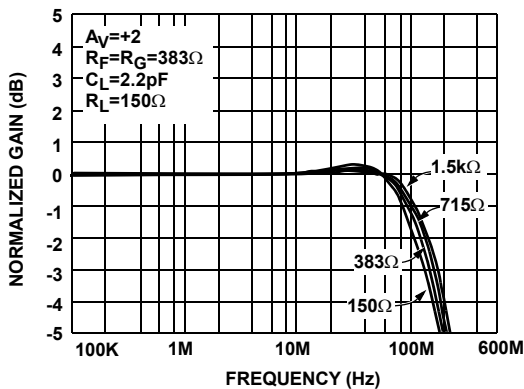


FIGURE 9. GAIN vs FREQUENCY FOR VARIOUS R_L

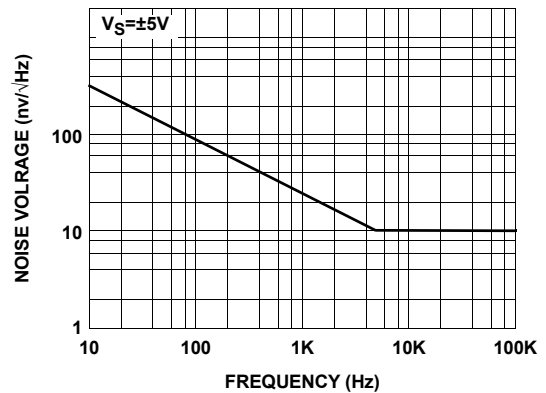


FIGURE 10. EQUIVALENT INPUT VOLTAGE NOISE vs FREQUENCY

Typical Performance Curves (Continued)

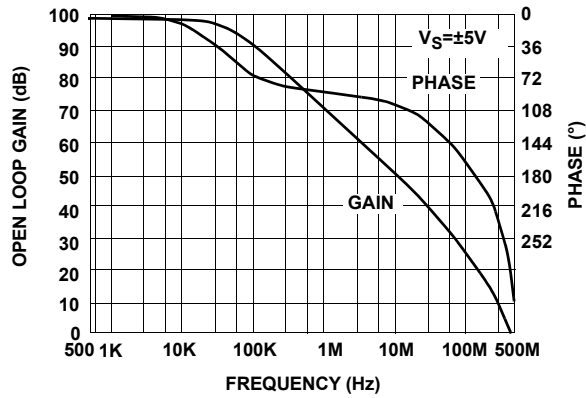


FIGURE 11. OPEN LOOP GAIN AND PHASE vs FREQUENCY

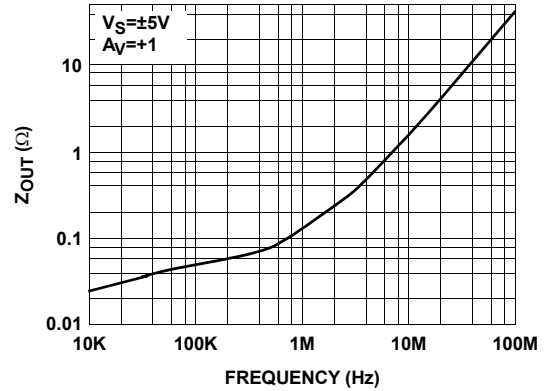


FIGURE 12. Z_{OUT} vs FREQUENCY

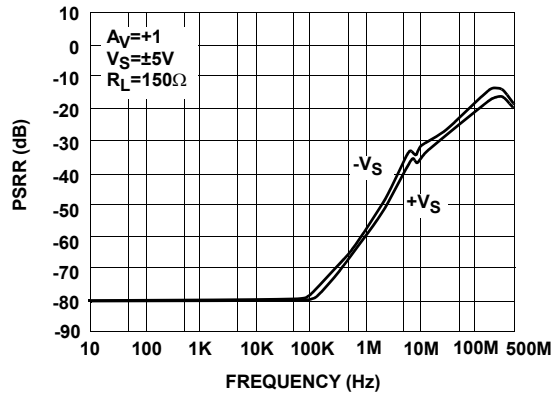


FIGURE 13. PSRR vs FREQUENCY

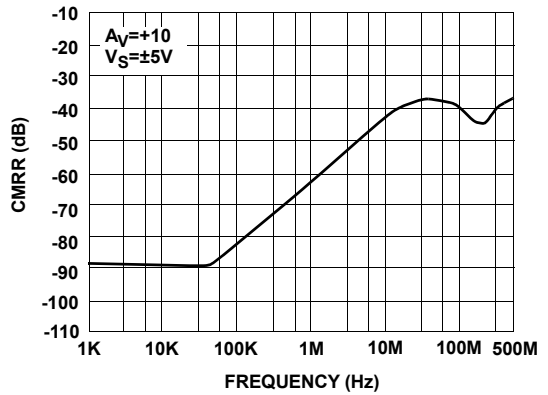


FIGURE 14. CMRR vs FREQUENCY

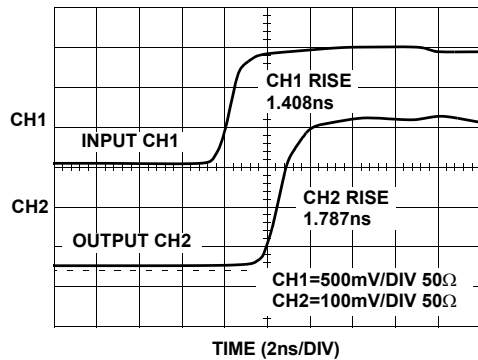


FIGURE 15. LARGE SIGNAL RISE TIME

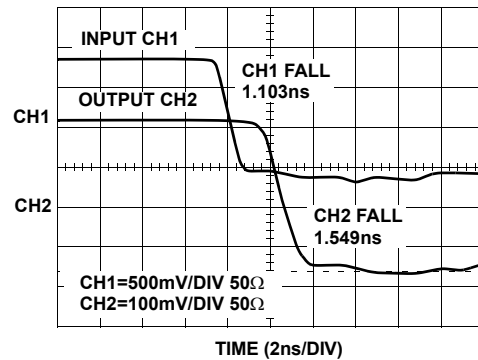


FIGURE 16. LARGE SIGNAL FALL TIME

Typical Performance Curves (Continued)

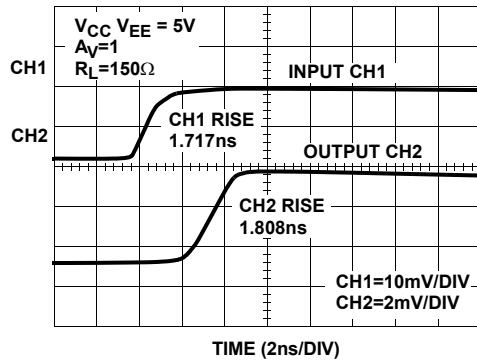


FIGURE 17. SMALL SIGNAL RISE TIME

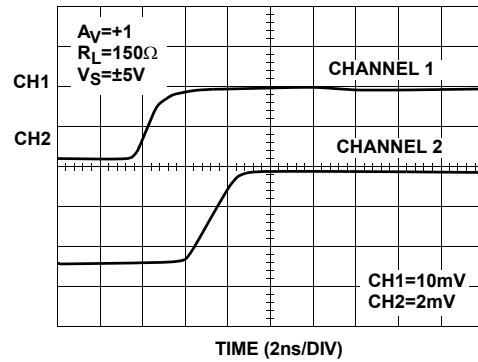


FIGURE 18. SMALL SIGNAL RISE TIME

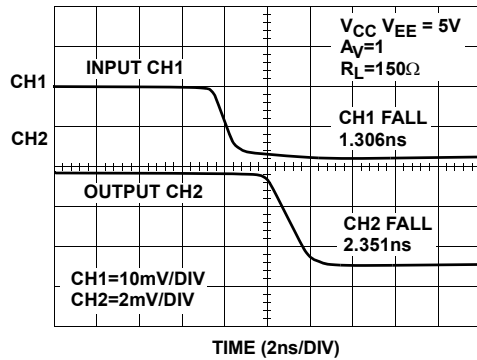


FIGURE 19. SMALL SIGNAL FALL TIME

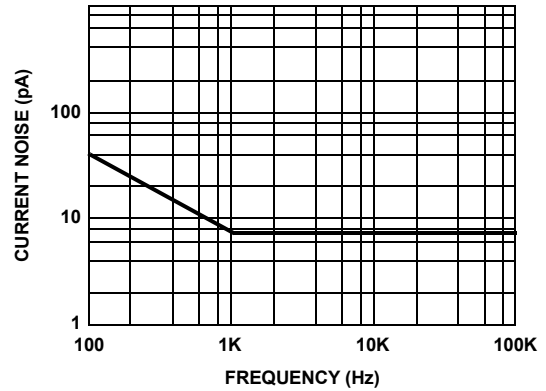


FIGURE 20. CURRENT NOISE

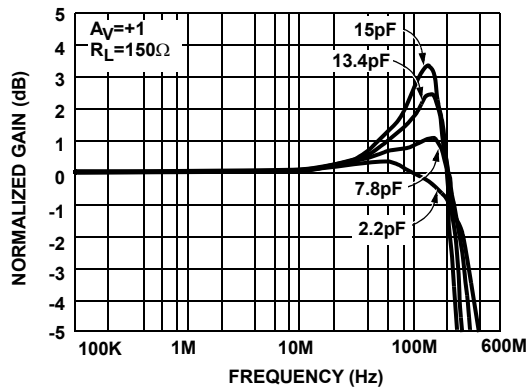


FIGURE 21. GAIN vs FREQUENCY FOR VARIOUS C_L

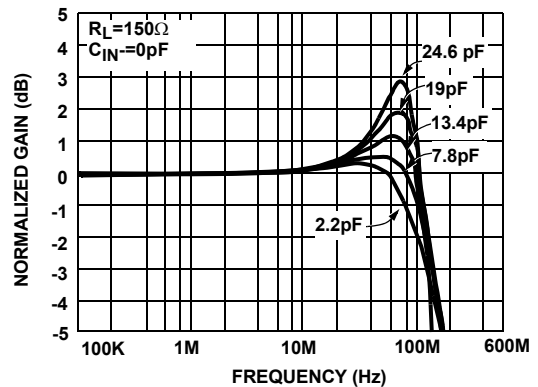


FIGURE 22. GAIN vs FREQUENCY FOR VARIOUS C_L

Typical Performance Curves (Continued)

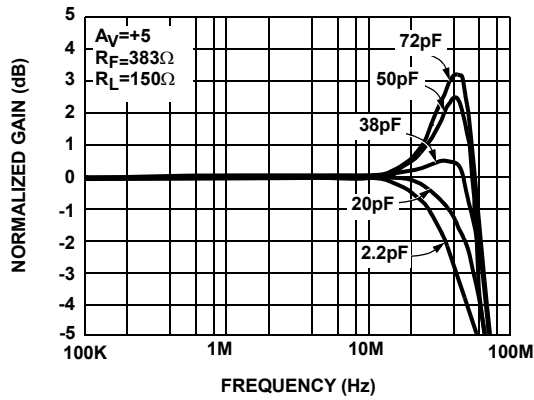


FIGURE 23. GAIN vs FREQUENCY FOR VARIOUS C_L

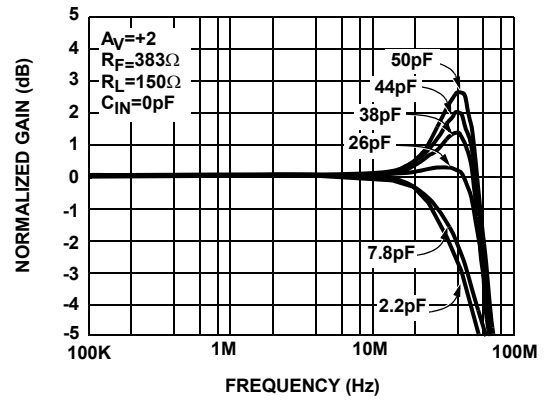


FIGURE 24. GAIN vs FREQUENCY FOR VARIOUS C_L

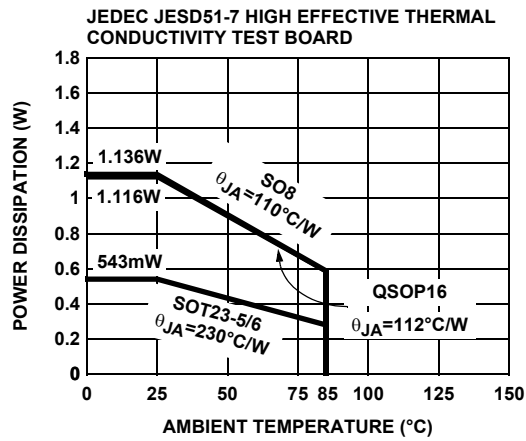


FIGURE 25. PACKAGE POWER DISSIPATION vs AMBIENT TEMPERATURE

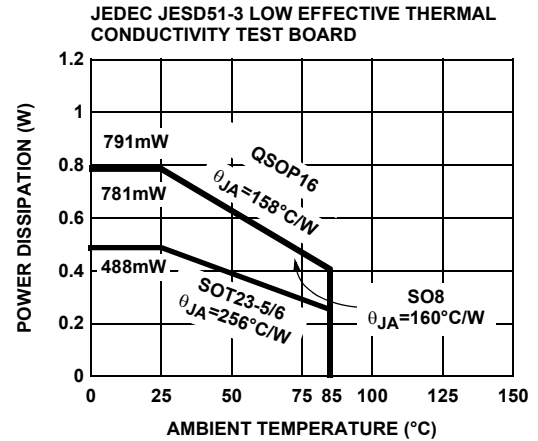


FIGURE 26. PACKAGE POWER DISSIPATION vs AMBIENT TEMPERATURE

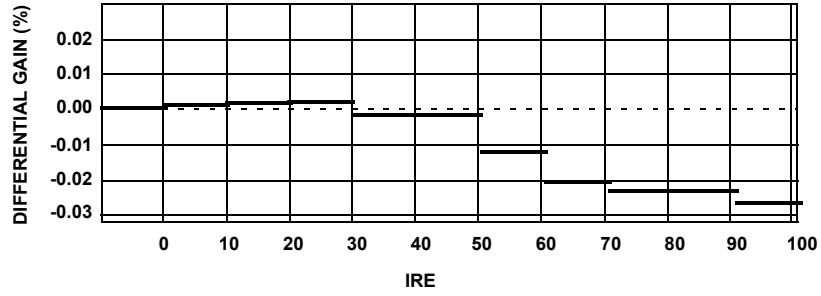


FIGURE 27. DIFFERENTIAL GAIN (%)

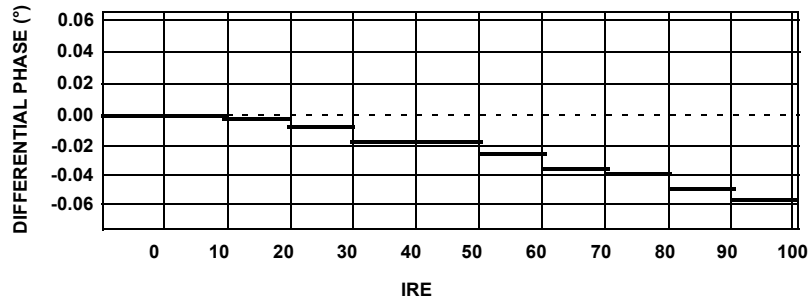


FIGURE 28. DIFFERENTIAL PHASE (°)

Application Information

Video Amplifier with Reduced Size Output Capacitance

If you have a video line driver $Z = 75\Omega$, the DC decoupling capacitor could be relatively large.

$$C = \frac{1}{2\pi \times R \times f} =$$

$$f = 10\text{Hz}, R = Z = 75\Omega, \quad C = 132\mu\text{F}$$

By using the circuit below, C could be reduced to $C2 = 22\mu\text{F}$.

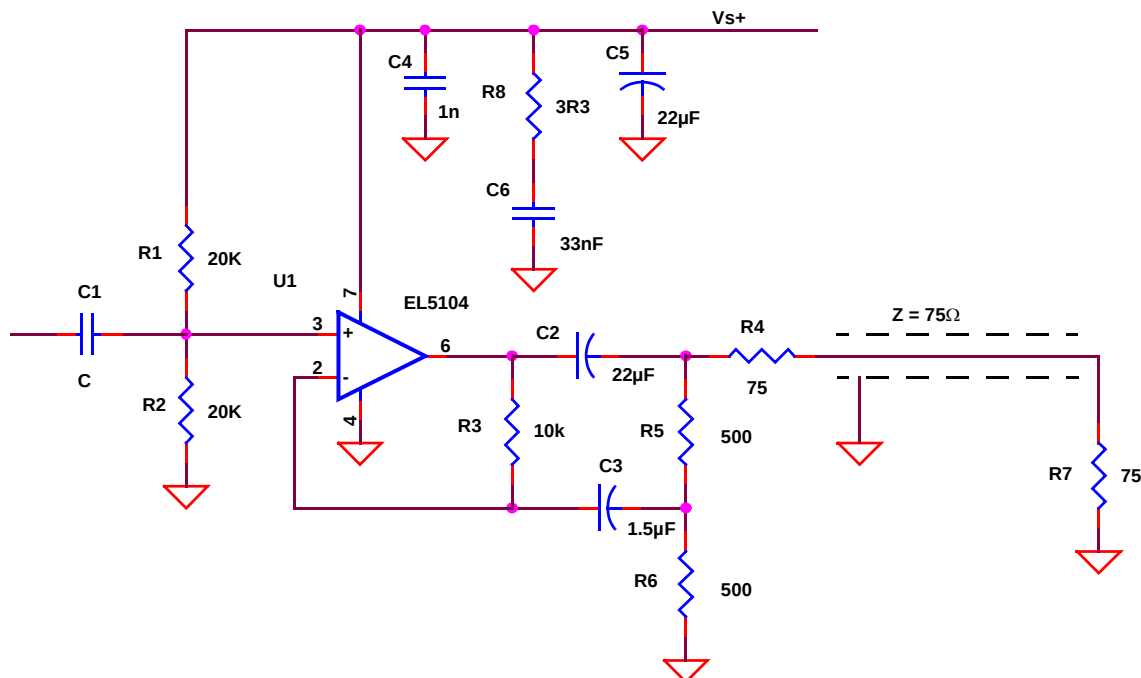


FIGURE 29.

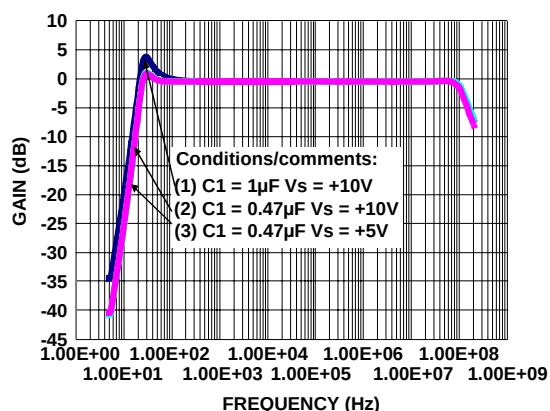


FIGURE 30. VIDEO-

The test result is shown on Figure 30.

By selecting a different value for $C1$, we could reduce the effect, created by $C3$ $R3$ and get flat response from 16Hz

with an 1/5 value, price and size output capacitor. There is another, very important issue by using high bandwidth amplifiers.

In the past when the bandwidth of the operational amplifier ended at a few hundred kHz even at few MHz, the power-supply bypass was not a very critical issue, since a $0.1\mu\text{F}$ capacitor “did the job”, but today’s amplifiers could have bandwidth, what used to be reserved for microwave circuits not to long time ago.

Therefore that high bandwidth amplifiers require the same respect what we reserve for microwave circuits. Particularly the power supply bypass and the pcb-layout could very heavily influence the performance of a modern high bandwidth amplifiers. It could happen above a few MHz, but it will happen above 100MHz, that the capacitor will behave like an inductor.

The reason for that is the very small but not zero value serial inductance of the capacitor.

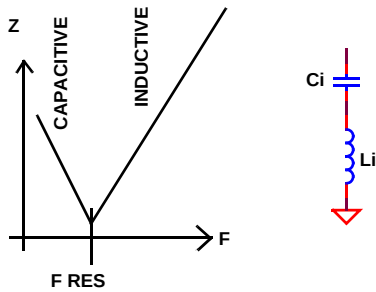


FIGURE 31.

The capacitor will behave as a capacitor up to its resonance frequency, above the resonance frequency it will behave as an inductor.

Just 1nHy inductance serial with 1nF capacitance will have serial resonance at:

$$F = \frac{1}{2\pi\sqrt{L \times C}}$$

$$C = 1\text{nF}, L = 1\text{nHy}, F = 159\text{ MHz}$$

And another 1nHy is very easy to get together with the inductance of traces on the pcb, and therefore you could encounter resonances from ca 50MHz and above anywhere. So if the amplifier has a bandwidth of a few hundred MHz, the proper power supply by-pass could become a serious if not difficult task.

Intuitively, you would use capacitors value 0.1µF parallel with a few µF tantalum, and to cure the effect of it's serial resonance put a smaller one parallel to it.

The result will surprise to you, because you will get even something worse than without the small capacitor.

What is happening there? Just look what we get:

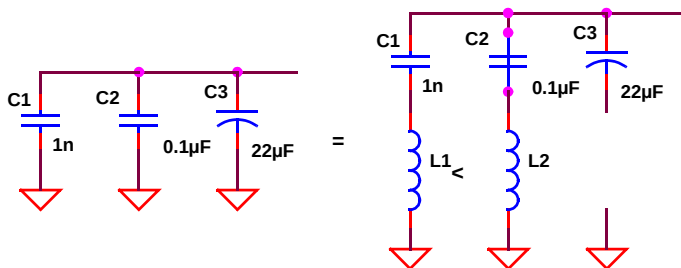


FIGURE 32.

Above its serial resonance $C2^*$ the ideal capacitance of $C2$ is a short, the Tantalum capacitor for high frequencies is not effective, the left over is $C1$ capacitor and $L1 + L2$ inductors, we get a parallel tank circuit, which is at its resonance a high impedance path and do not carry any high frequency current, it does not work as bypass at all!

The impedance of a parallel tank circuit at resonance is dependent from its Q. High Q high impedance.

The Q of a parallel tank circuit could be reduced by bypassing it with a resistor, or adding a resistor in serial to one of the reactive components. Since the bypassing would short the DC supply we do have to go to add resistor in serial to the reactive component, we will add a resistor serial with the inductor. (See Figure 33.)

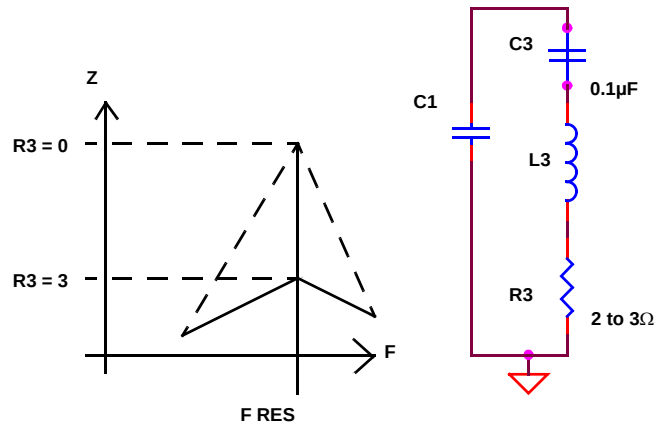


FIGURE 33.

The final power supply bypass circuit will look:

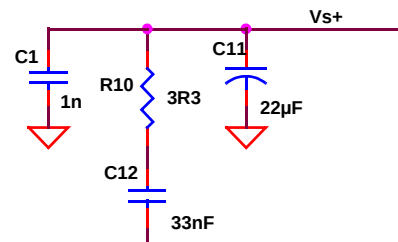


FIGURE 34.

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