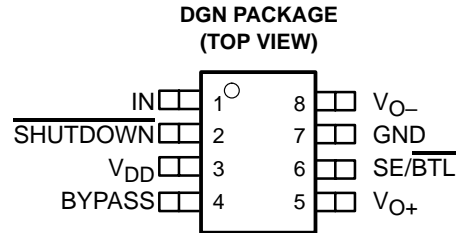


# TPA0211

## 2-W MONO AUDIO POWER AMPLIFIER

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- Ideal for Wireless Communicators, Notebook PCs, PDAs, and Other Small Portable Audio Devices
- 2 W Into 4  $\Omega$  From 5-V Supply
- 0.6 W Into 4  $\Omega$  From 3-V Supply
- Wide Power Supply Compatibility  
3 V to 5 V
- Low Supply Current
  - 4 mA Typical at 5 V
  - 4 mA Typical at 3 V
- Shutdown Control . . . 1  $\mu$ A Typical
- Shutdown Pin Is TTL Compatible
- –40°C to 85°C Operating Temperature Range
- Space-Saving, Thermally-Enhanced MSOP Packaging



### description

The TPA0211 is a 2-W mono bridge-tied-load (BTL) amplifier designed to drive speakers with as low as 4- $\Omega$  impedance. The device is ideal for use in small wireless communicators, notebook PCs, PDAs, anywhere a mono speaker and stereo headphones are required. From a 5-V supply, the TPA0211 can deliver 2 W of power into a 4- $\Omega$  speaker.

The gain of the input stage is set by the user-selected input resistor and a 50-k $\Omega$  internal feedback resistor ( $A_V = -R_F/R_I$ ). The power stage is internally configured with a gain of –1.25 V/V in SE mode, and –2.5 V/V in BTL mode. Thus, the overall gain of the amplifier is –62.5 k $\Omega$ /  $R_I$  in SE mode and –125 k $\Omega$ /  $R_I$  in BTL mode. The input terminals are high-impedance CMOS inputs, and can be used as summing nodes.

The TPA0211 is available in the 8-pin thermally-enhanced MSOP package (DGN) and operates over an ambient temperature range of –40°C to 85°C.

### AVAILABLE OPTIONS

T <sub>A</sub>	PACKAGED DEVICES	MSOP SYMBOLIZATION
	MSOP† (DGN)	
–40°C to 85°C	TPA0211DGN	AEG

† The DGN package are available taped and reeled. To order a taped and reeled part, add the suffix R to the part number (e.g., TPA0211DGNR).



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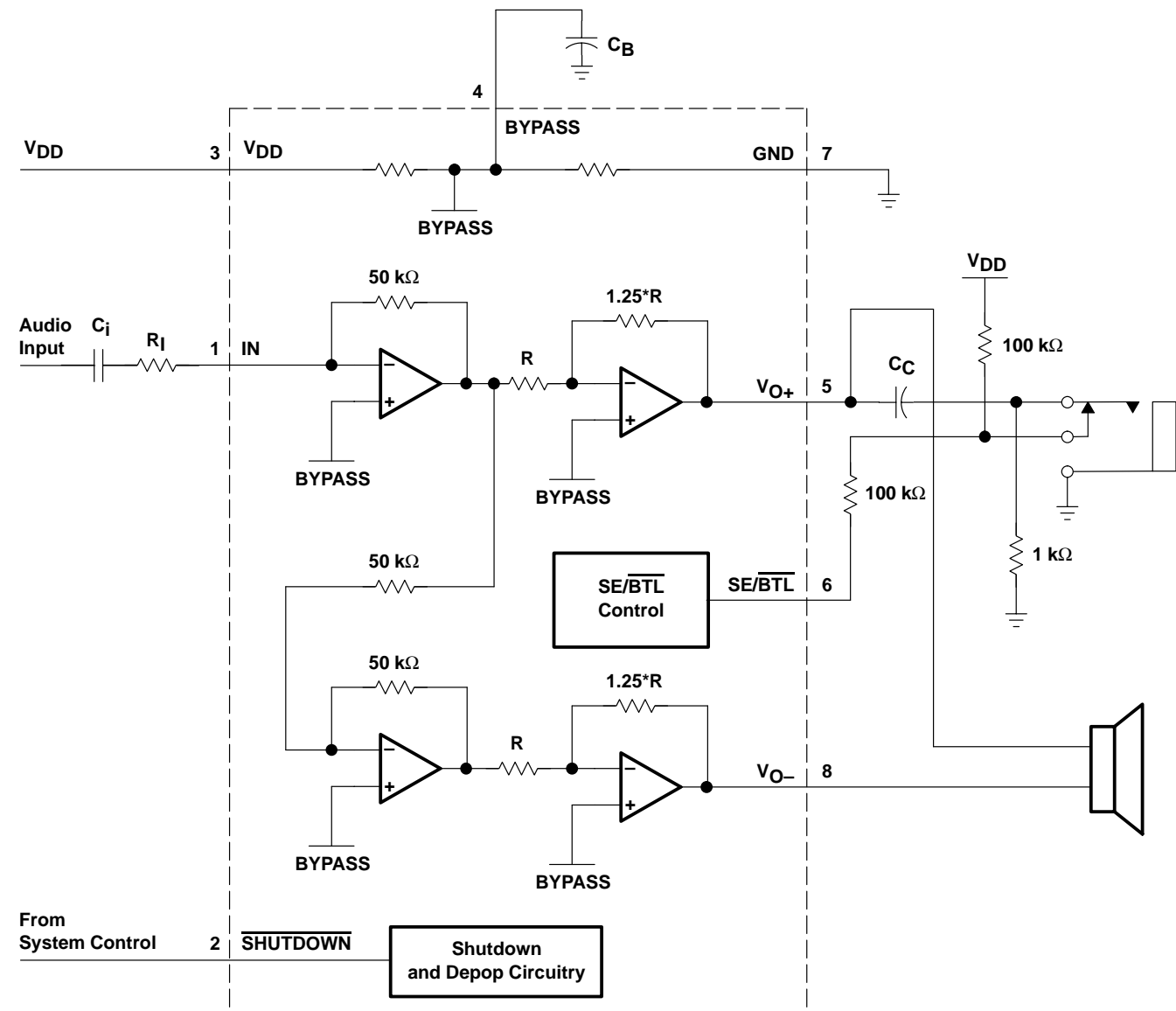
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# TPA0211

## 2-W MONO AUDIO POWER AMPLIFIER

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### functional block diagram



Terminal Functions			
TERMINAL NAME	NO.	I/O	DESCRIPTION
BYPASS	4	I	BYPASS is the tap to the voltage divider for internal mid-supply bias. This terminal should be connected to a 0.1-μF to 1-μF capacitor.
GND	7		GND is the ground connection.
IN	1	I	IN is the audio input terminal.
SE/BTL	6	I	When SE/BTL is held low, the TPA0211 is in BTL mode. When SE/BTL is held high, the TPA0211 is in SE mode.
SHUTDOWN	2	I	SHUTDOWN places the entire device in shutdown mode when held low. TTL compatible input.
VDD	3		VDD is the supply voltage terminal.
VO+	5	O	VO+ is the positive output for BTL and SE modes.
VO-	8	O	VO- is the negative output in BTL mode and a high-impedance output in SE mode.

# TPA0211

## 2-W MONO AUDIO POWER AMPLIFIER

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### absolute maximum ratings over operating free-air temperature range (unless otherwise noted)<sup>†</sup>

Supply voltage, $V_{DD}$	6 V
Input voltage, $V_I$	–0.3 V to $V_{DD} + 0.3$ V
Continuous total power dissipation	internally limited (see Dissipation Rating Table)
Operating free-air temperature range, $T_A$	–40°C to 85°C
Operating junction temperature range, $T_J$	–40°C to 150°C
Storage temperature range, $T_{stg}$	–65°C to 150°C
Lead temperature 1,6 mm (1/16 inch) from case for 10 seconds	260°C

<sup>†</sup>Stresses beyond those listed under “absolute maximum ratings” may cause permanent damage to the device. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those indicated under “recommended operating conditions” is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

DISSIPATION RATING TABLE

PACKAGE	$T_A \leq 25^\circ\text{C}$	DERATING FACTOR	$T_A = 70^\circ\text{C}$	$T_A = 85^\circ\text{C}$
DGN	2.14 W <sup>‡</sup>	17.1 mW/°C	1.37 W	1.11 W

<sup>‡</sup> See the Texas Instruments document, *PowerPAD Thermally Enhanced Package Application Report* (literature number SLMA002), for more information on the PowerPAD package. The thermal data was measured on a PCB layout based on the information in the section entitled *Texas Instruments Recommended Board for PowerPAD* on page 33 of the before mentioned document.

### recommended operating conditions

		MIN	MAX	UNIT
Supply voltage, $V_{DD}$		2.5	5.5	V
High-level input voltage, $V_{IH}$	SE/BTL	$V_{DD} = 3$ V	2.7	V
		$V_{DD} = 5$ V	4.5	
	SHUTDOWN		2	
Low-level input voltage, $V_{IL}$	SE/BTL	$V_{DD} = 3$ V	1.65	V
		$V_{DD} = 5$ V	2.75	
	SHUTDOWN		0.8	
Operating free-air temperature, $T_A$		–40	85	°C

### electrical characteristics at specified free-air temperature, $V_{DD} = 3$ V, $T_A = 25^\circ\text{C}$ (unless otherwise noted)

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
$ V_{OO} $ Output offset voltage (measured differentially)				30	mV
$I_{DD}$ Supply current			4	6	mA
$I_{DD(SD)}$ Supply current, shutdown mode			1	10	μA

### operating characteristics, $V_{DD} = 3$ V, $T_A = 25^\circ\text{C}$ , $R_L = 4 \Omega$

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
$P_O$ Output power	THD = 1%, BTL mode, $f = 1$ kHz		660		mW
	THD = 0.1%, SE mode, $f = 1$ kHz, $R_L = 32 \Omega$		33		
THD + N Total harmonic distortion plus noise	$P_O = 500$ mW, $f = 20$ Hz to 20 kHz		0.3%		
BOM Maximum output power bandwidth	Gain = 2, THD = 2%		20		kHz
SNR Signal-to-noise ratio			88		dB
$V_n$ Output noise voltage	$C_B = 0.47 \mu\text{F}$ , $f = 20$ Hz to 20 kHz				μV <sub>RMS</sub>
	BTL mode, $R_L = 8 \Omega$ , $A_V = 8$ dB		65		
	SE mode, $R_L = 32 \Omega$ , $A_V = 2$ dB		25		



# TPA0211

## 2-W MONO AUDIO POWER AMPLIFIER

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**electrical characteristics at specified free-air temperature,  $V_{DD} = 5\text{ V}$ ,  $T_A = 25^\circ\text{C}$  (unless otherwise noted)**

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
$ V_{OO} $ Output offset voltage (measured differentially)				30	mV
$I_{DD}$ Supply current			4	6	mA
$I_{DD}(\text{SD})$ Supply current, shutdown mode			1	10	$\mu\text{A}$

**operating characteristics,  $V_{DD} = 5\text{ V}$ ,  $T_A = 25^\circ\text{C}$ ,  $R_L = 4\ \Omega$**

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
$P_O$ Output power	THD = 1%, BTL mode, $f = 1\text{ kHz}$		2		W
	THD = 0.1%, SE mode, $f = 1\text{ kHz}$ , $R_L = 32\ \Omega$		92		mW
THD + N Total harmonic distortion plus noise	$P_O = 1.5\text{ W}$ , $f = 20\text{ Hz to } 20\text{ kHz}$		0.2%		
BOM Maximum output power bandwidth	Gain = 2.5, THD = 2%		20		kHz
SNR Signal-to-noise ratio			93		dB
$V_n$ Output noise voltage	$C_B = 0.47\ \mu\text{F}$ , $f = 20\text{ Hz to } 20\text{ kHz}$ , BTL mode, $R_L = 8\ \Omega$ , $A_V = 8\text{ dB}$		65		$\mu\text{V}_{\text{RMS}}$
	SE mode, $R_L = 32\ \Omega$ , $A_V = 2\text{ dB}$		25		

### TYPICAL CHARACTERISTICS

Table of Graphs

		FIGURE
Supply ripple rejection ratio	vs Frequency	1, 2
$I_{DD}$ Supply current	vs Supply voltage	3
$P_O$ Output power	vs Supply voltage	4, 5
	vs Load resistance	6, 7
THD+N Total harmonic distortion plus noise	vs Frequency	8, 9, 10, 11
	vs Output power	12, 13, 14, 15, 16, 17
$V_n$ Output noise voltage	vs Frequency	18, 19
Closed loop gain and phase		20, 21



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## TYPICAL CHARACTERISTICS

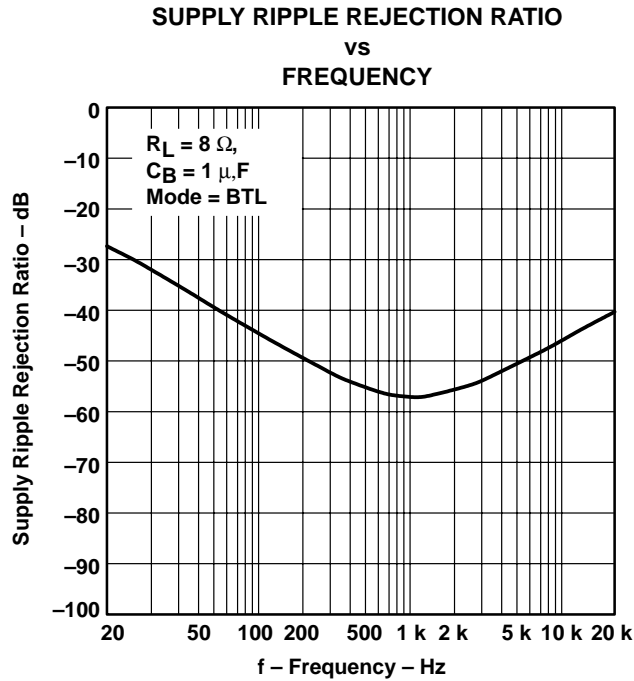


Figure 1

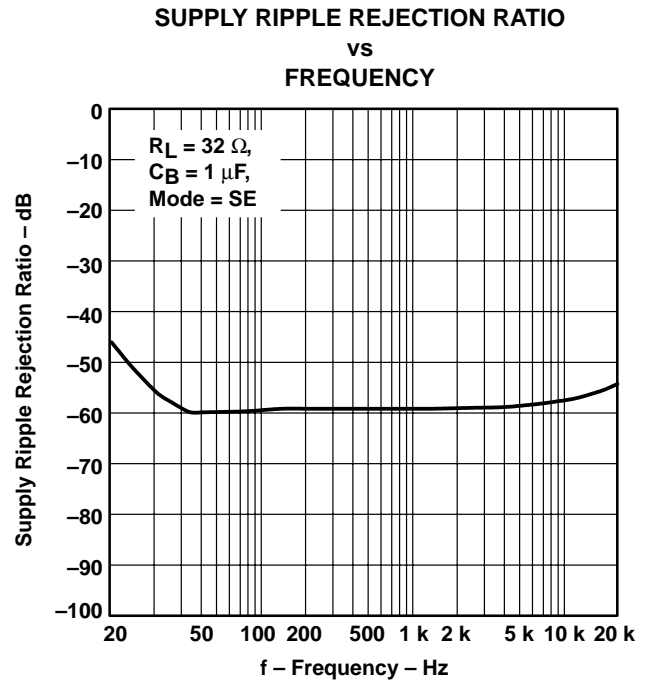


Figure 2

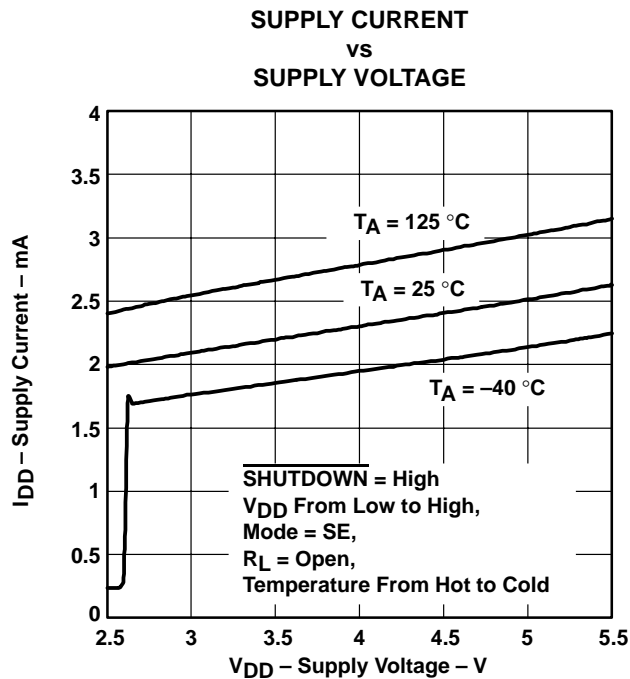


Figure 3

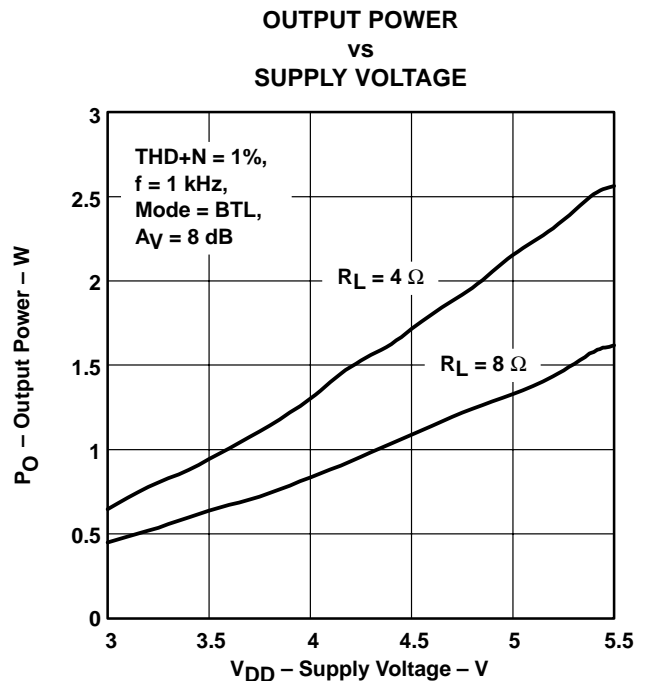
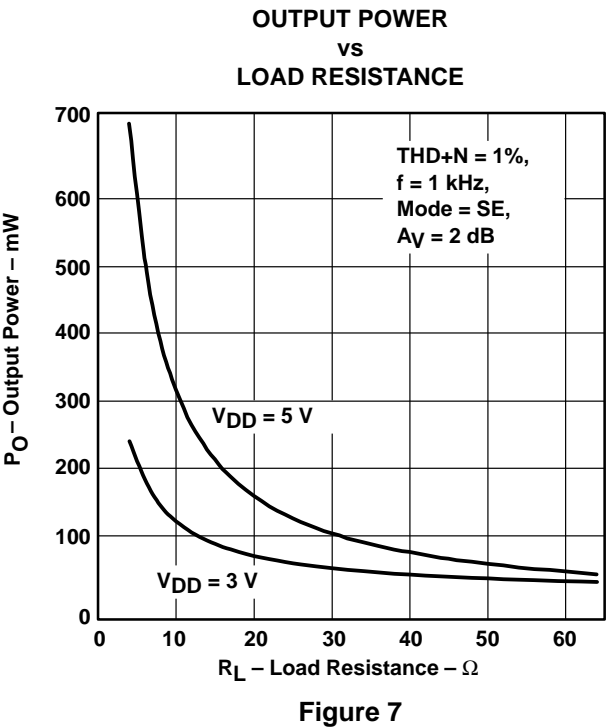
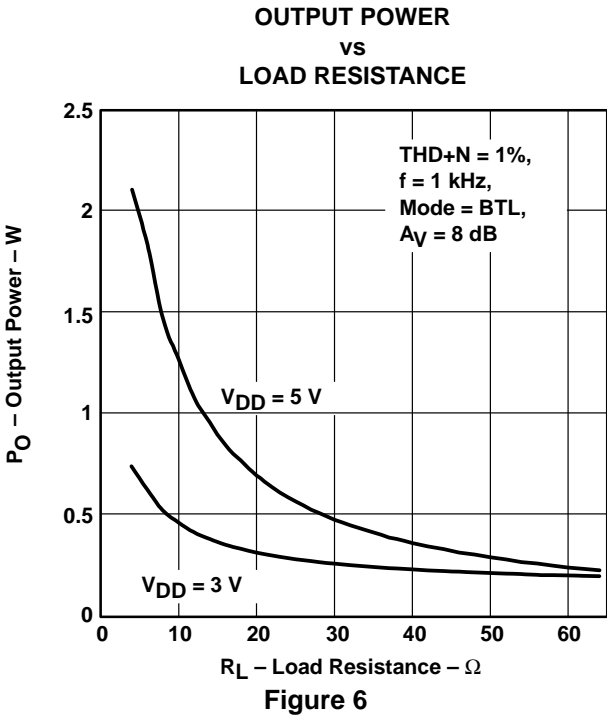
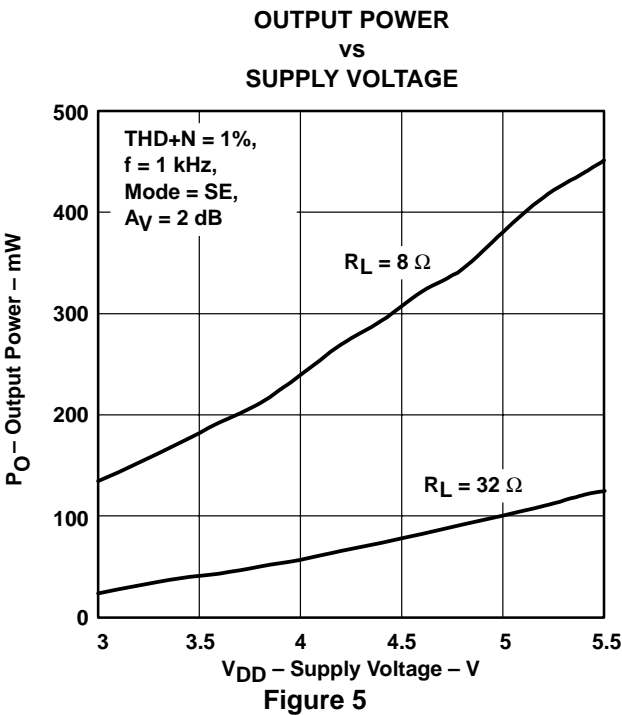


Figure 4

TPA0211  
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TYPICAL CHARACTERISTICS



## TYPICAL CHARACTERISTICS

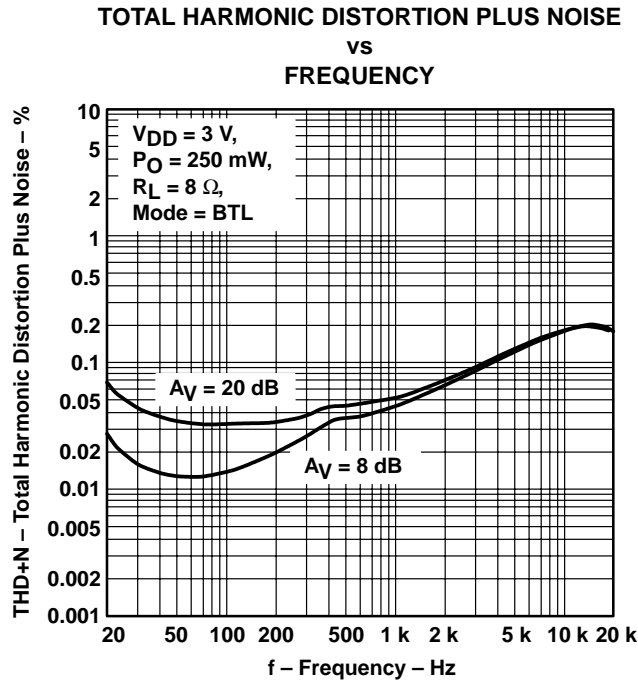


Figure 8

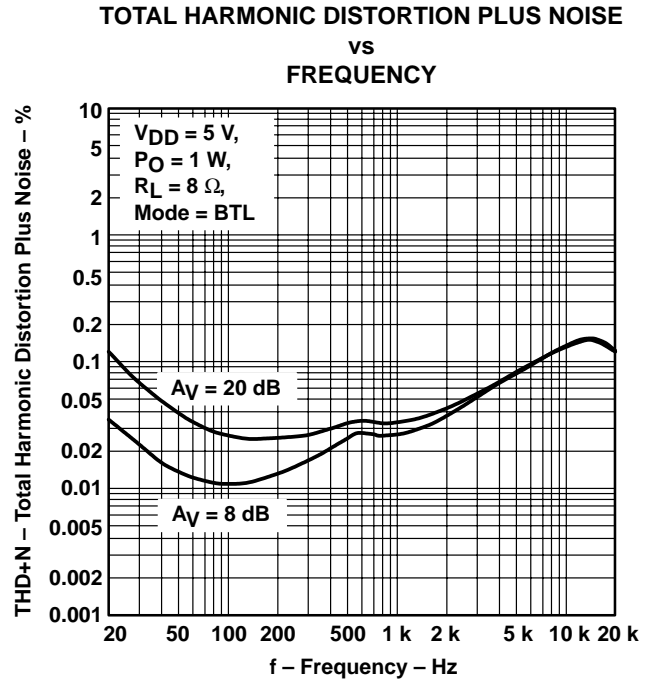


Figure 9

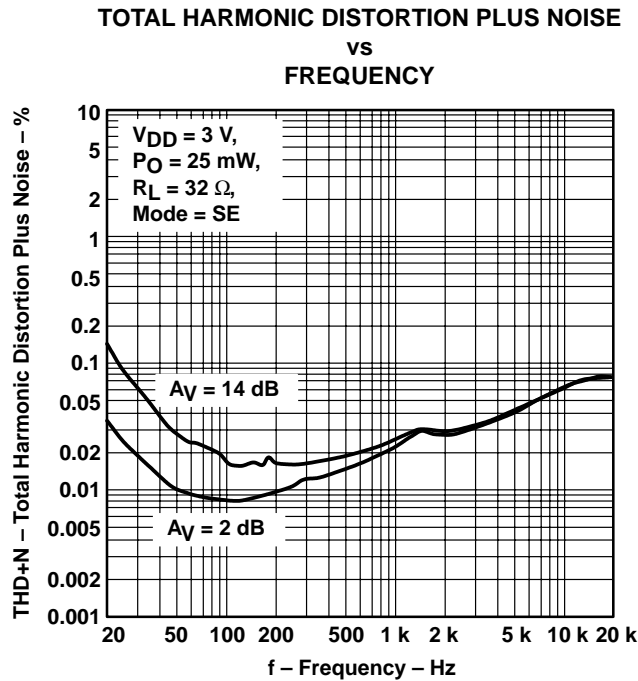


Figure 10

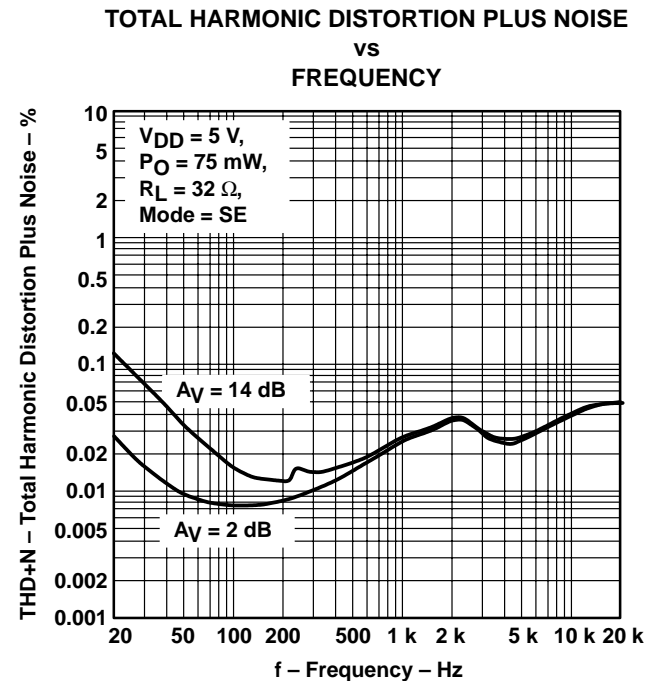


Figure 11

# TPA0211

## 2-W MONO AUDIO POWER AMPLIFIER

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### TYPICAL CHARACTERISTICS

TOTAL HARMONIC DISTORTION PLUS NOISE  
vs  
OUTPUT POWER

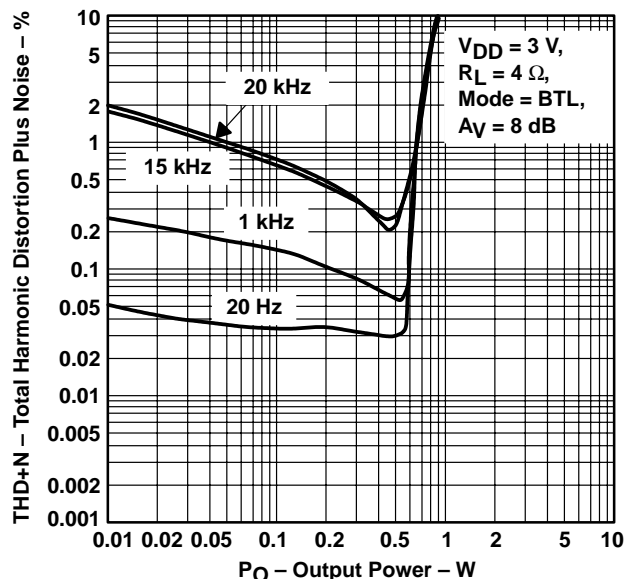


Figure 12

TOTAL HARMONIC DISTORTION PLUS NOISE  
vs  
OUTPUT POWER

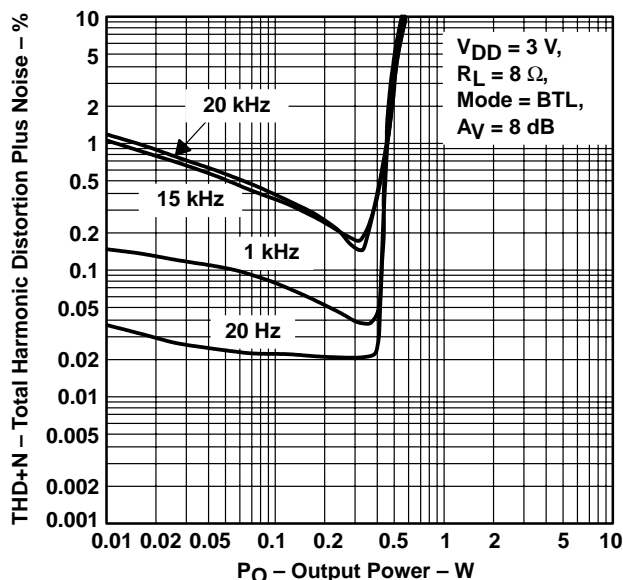


Figure 13

TOTAL HARMONIC DISTORTION PLUS NOISE  
vs  
OUTPUT POWER

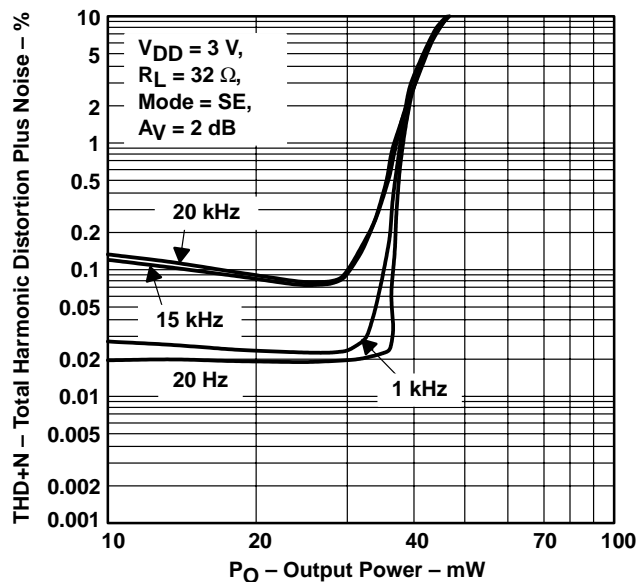


Figure 14

TOTAL HARMONIC DISTORTION PLUS NOISE  
vs  
OUTPUT POWER

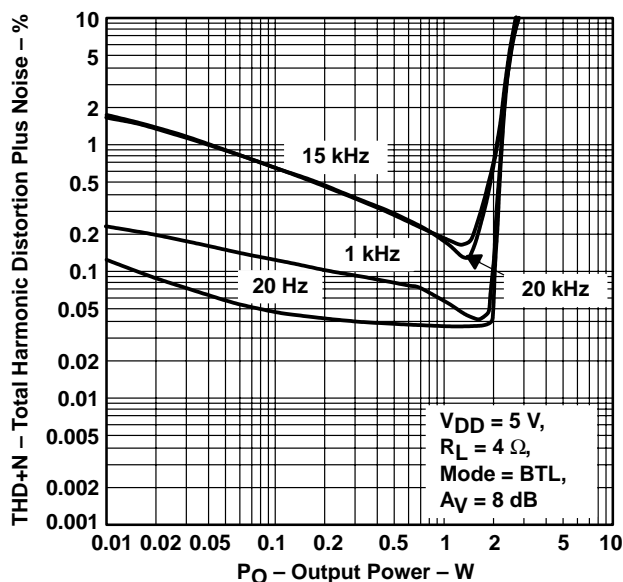


Figure 15



## TYPICAL CHARACTERISTICS

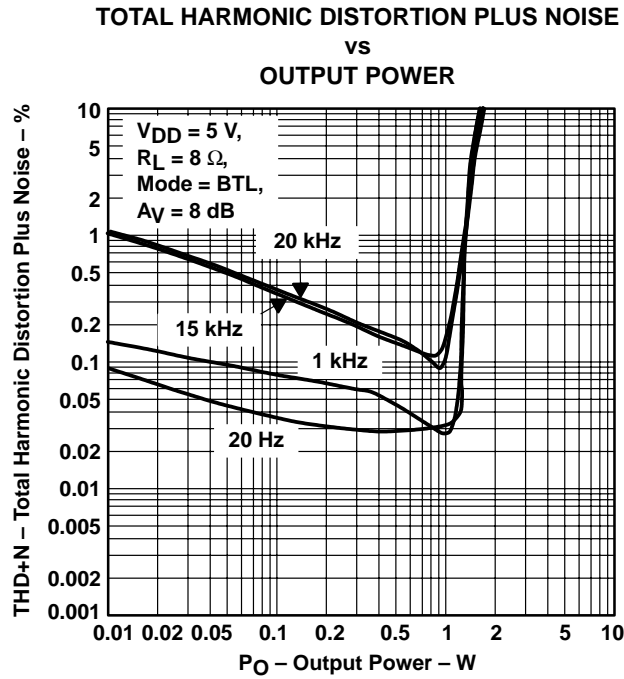


Figure 16

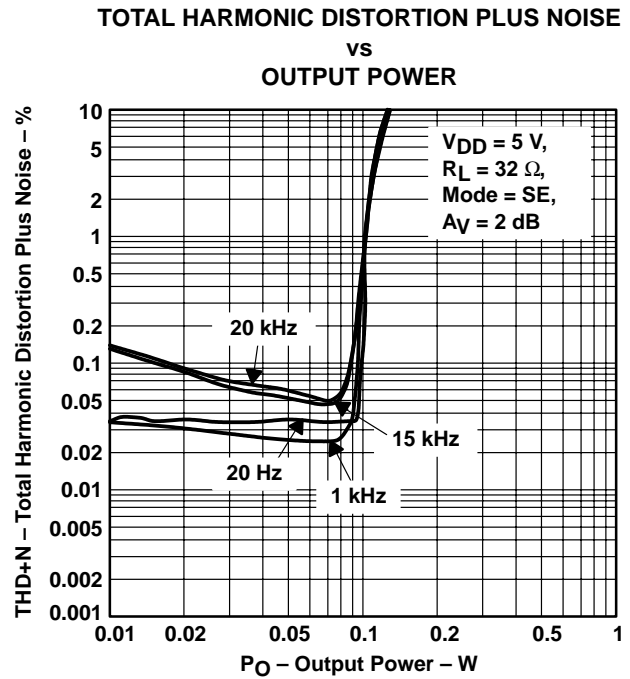


Figure 17

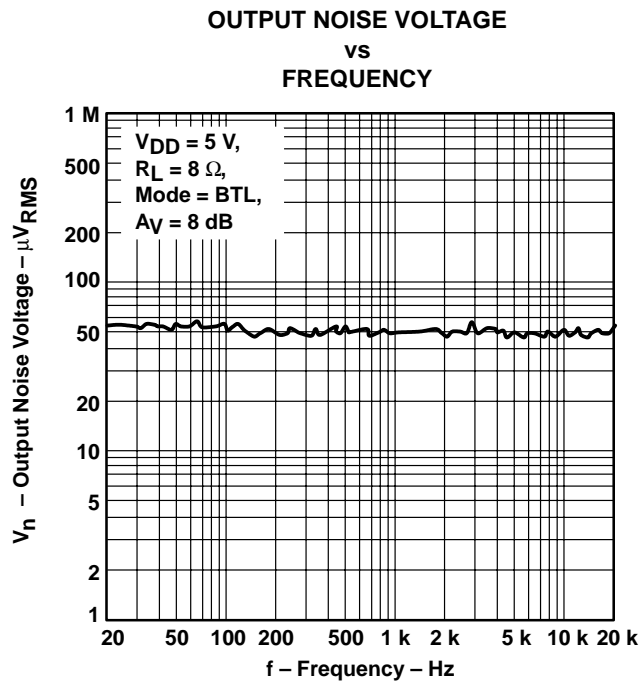


Figure 18

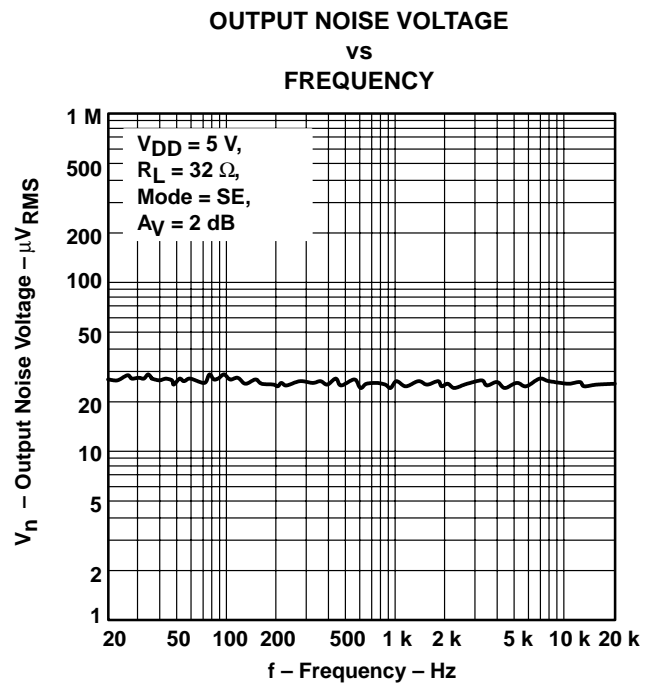


Figure 19

# TPA0211

## 2-W MONO AUDIO POWER AMPLIFIER

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### TYPICAL CHARACTERISTICS

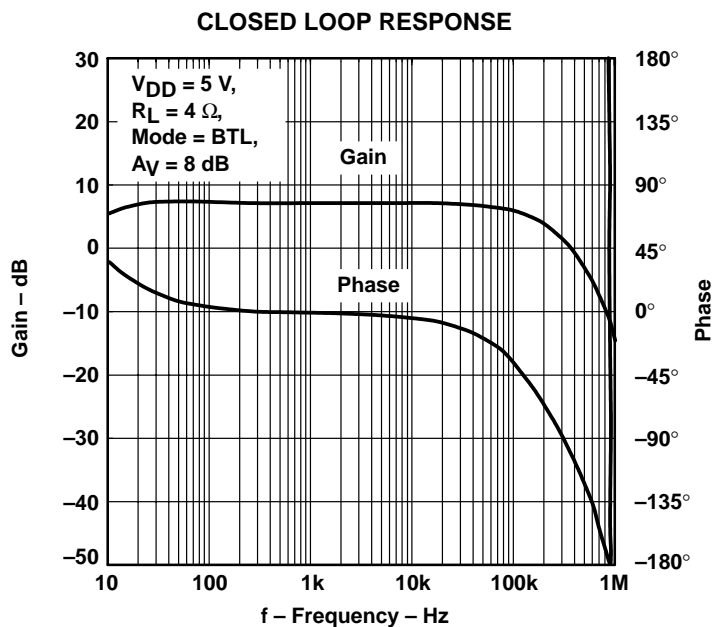


Figure 20

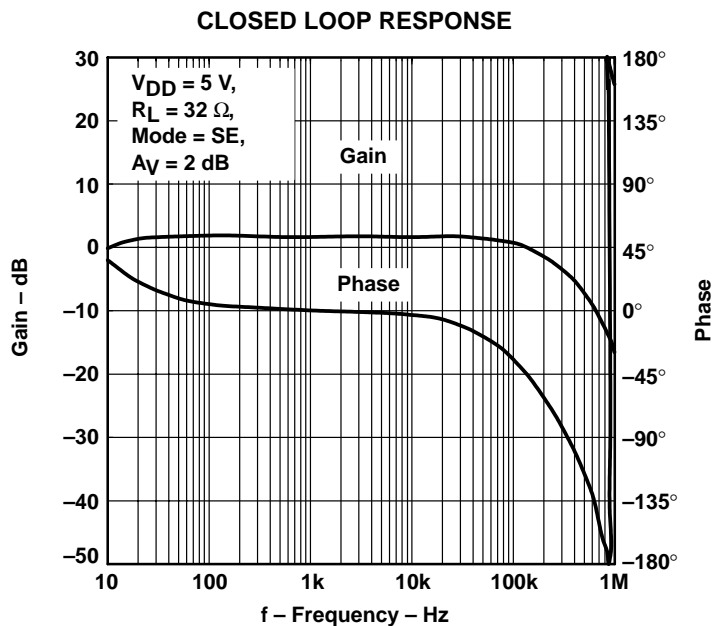


Figure 21

## APPLICATION INFORMATION

### gain setting via input resistance

The gain of the input stage is set by the user-selected input resistor and a 50-kΩ internal feedback resistor.

However, the power stage is internally configured with a gain of  $-1.25$  V/V in SE mode, and  $-2.5$  V/V in BTL mode. Thus, the feedback resistor ( $R_F$ ) is effectively 62.5 kΩ in SE mode and 125 kΩ in BTL mode. Therefore, the overall gain can be calculated using equations (1) and (2).

$$A_V = \frac{-125 \text{ k}\Omega}{R_I} \quad (\text{BTL}) \quad (1)$$

$$A_V = \frac{-62.5 \text{ k}\Omega}{R_I} \quad (\text{SE}) \quad (2)$$

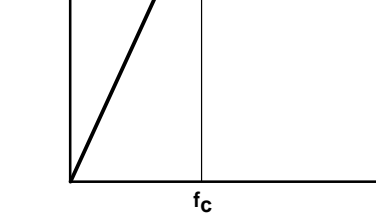
The  $-3$  dB frequency can be calculated using equation 3:

$$f_{-3 \text{ dB}} = \frac{1}{2\pi R_I C_i} \quad (3)$$

If the filter must be more accurate, the value of the capacitor should be increased while the value of the resistor to ground should be decreased. In addition, the order of the filter could be increased.

### input capacitor, $C_i$

In the typical application an input capacitor,  $C_i$ , is required to allow the amplifier to bias the input signal to the proper dc level for optimum operation. In this case,  $C_i$  and the input resistance of the amplifier,  $R_I$ , form a high-pass filter with the corner frequency determined in equation 4.

$$f_{c(\text{highpass})} = \frac{1}{2\pi R_I C_i} \quad (4)$$


The value of  $C_i$  is important to consider as it directly affects the bass (low frequency) performance of the circuit. Consider the example where  $R_I$  is 10 kΩ and the specification calls for a flat bass response down to 40 Hz. Equation 2 is reconfigured as equation 5.

$$C_i = \frac{1}{2\pi R_I f_c} \quad (5)$$

In this example,  $C_i$  is 0.4 μF so one would likely choose a value in the range of 0.47 μF to 1 μF. A further consideration for this capacitor is the leakage path from the input source through the input network ( $C_i$ ) and the feedback network to the load. This leakage current creates a dc offset voltage at the input to the amplifier that reduces useful headroom, especially in high gain applications. For this reason a low-leakage tantalum or ceramic capacitor is the best choice. When polarized capacitors are used, the positive side of the capacitor should face the amplifier input in most applications as the dc level there is held at  $V_{DD}/2$ , which is likely higher than the source dc level. Note that it is important to confirm the capacitor polarity in the application.

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### APPLICATION INFORMATION

#### power supply decoupling, $C_{(S)}$

The TPA0211 is a high-performance CMOS audio amplifier that requires adequate power supply decoupling to ensure the output total harmonic distortion (THD) is as low as possible. Power supply decoupling also prevents oscillations for long lead lengths between the amplifier and the speaker. The optimum decoupling is achieved by using two capacitors of different types that target different types of noise on the power supply leads. For higher frequency transients, spikes, or digital hash on the line, a good low equivalent-series-resistance (ESR) ceramic capacitor, typically  $0.1\ \mu\text{F}$  placed as close as possible to the device  $V_{DD}$  lead, works best. For filtering lower-frequency noise signals, a larger aluminum electrolytic capacitor of  $10\ \mu\text{F}$  or greater placed near the audio power amplifier is recommended.

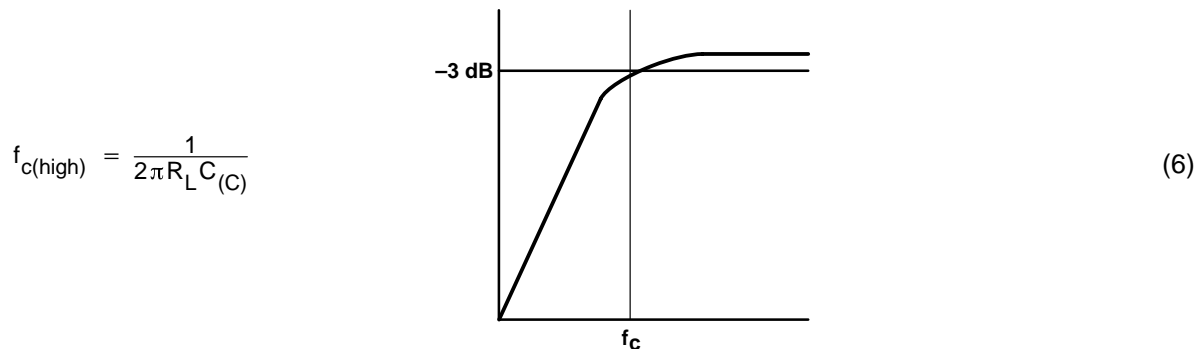
#### midrail bypass capacitor, $C_{(BYP)}$

The midrail bypass capacitor,  $C_{(BYP)}$ , is the most critical capacitor and serves several important functions. During start-up or recovery from shutdown mode,  $C_{(BYP)}$  determines the rate at which the amplifier starts up. The second function is to reduce noise produced by the power supply caused by coupling into the output drive signal. This noise is from the midrail generation circuit internal to the amplifier, which appears as degraded PSRR and THD+N.

Bypass capacitor,  $C_{(BYP)}$ , values of  $0.47\ \mu\text{F}$  to  $1\ \mu\text{F}$  ceramic or tantalum low-ESR capacitors are recommended for the best THD and noise performance.

#### output coupling capacitor, $C_{(C)}$

In the typical single-supply SE configuration, an output coupling capacitor ( $C_{(C)}$ ) is required to block the dc bias at the output of the amplifier thus preventing dc currents in the load. As with the input coupling capacitor, the output coupling capacitor and impedance of the load form a high-pass filter governed by equation 6.



The main disadvantage, from a performance standpoint, is the load impedances are typically small, which drives the low-frequency corner higher, degrading the bass response. Large values of  $C_{(C)}$  are required to pass low frequencies into the load. Consider the example where a  $C_{(C)}$  of  $330\ \mu\text{F}$  is chosen and loads vary from  $3\ \Omega$ ,  $4\ \Omega$ ,  $8\ \Omega$ ,  $32\ \Omega$ ,  $10\ \text{k}\Omega$ , to  $47\ \text{k}\Omega$ . Table 1 summarizes the frequency response characteristics of each configuration.

## APPLICATION INFORMATION

**Table 1. Common Load Impedances vs Low Frequency Output Characteristics in SE Mode**

$R_L$	$C(C)$	Lowest Frequency
3 $\Omega$	330 $\mu F$	161 Hz
4 $\Omega$	330 $\mu F$	120 Hz
8 $\Omega$	330 $\mu F$	60 Hz
32 $\Omega$	330 $\mu F$	15 Hz
10,000 $\Omega$	330 $\mu F$	0.05 Hz
47,000 $\Omega$	330 $\mu F$	0.01 Hz

As Table 1 indicates, most of the bass response is attenuated into a 4- $\Omega$  load, an 8- $\Omega$  load is adequate, headphone response is good, and drive into line level inputs (a home stereo for example) is exceptional.

Furthermore, the total amount of ripple current that must flow through the capacitor must be considered when choosing the component. As shown in the application circuit, one coupling capacitor must be in series with the mono loudspeaker for proper operation of the stereo-mono switching circuit. For a 4- $\Omega$  load, this capacitor must be able to handle about 700 mA of ripple current for a continuous output power of 2 W.

### using low-ESR capacitors

Low-ESR capacitors are recommended throughout this applications section. A real (as opposed to ideal) capacitor can be modeled simply as a resistor in series with an ideal capacitor. The voltage drop across this resistor minimizes the beneficial effects of the capacitor in the circuit. The lower the equivalent value of this resistance the more the real capacitor behaves like an ideal capacitor.

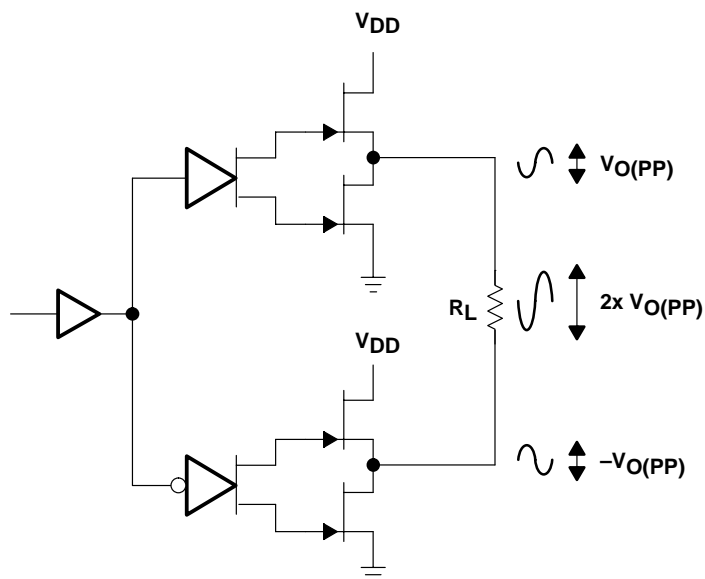
### bridged-tied load versus single-ended mode

Figure 22 shows a Class-AB audio power amplifier (APA) in a BTL configuration. The TPA0211 BTL amplifier consists of two Class-AB amplifiers driving both ends of the load. There are several potential benefits to this differential drive configuration, but initially consider power to the load. The differential drive to the speaker means that as one side is slewing up, the other side is slewing down, and vice versa. This in effect doubles the voltage swing on the load as compared to a ground referenced load. Plugging  $2 \times V_{O(PP)}$  into the power equation, where voltage is squared, yields  $4\times$  the output power from the same supply rail and load impedance (see equation 7).

$$V_{(RMS)} = \frac{V_{O(PP)}}{2\sqrt{2}} \quad (7)$$

$$Power = \frac{V_{(RMS)}^2}{R_L}$$

## APPLICATION INFORMATION



**Figure 22. Bridge-Tied Load Configuration**

In a typical computer sound channel operating at 5 V, bridging raises the power into an 8-Ω speaker from a singled-ended (SE, ground reference) limit of 250 mW to 1 W. In sound power, that is a 6-dB improvement—which is loudness that can be heard. In addition to increased power, there are frequency response concerns. Consider the single-supply SE configuration shown in Figure 23. A coupling capacitor is required to block the dc offset voltage from reaching the load. These capacitors can be quite large (approximately 33 μF to 1000 μF) so they tend to be expensive, heavy, occupy valuable PCB area, and have the additional drawback of limiting low-frequency performance of the system. This frequency limiting effect is due to the high pass filter network created with the speaker impedance and the coupling capacitance and is calculated with equation 8.

$$f_c = \frac{1}{2\pi R_L C_{(C)}} \quad (8)$$

## APPLICATION INFORMATION

### bridged-tied load versus single-ended mode (continued)

For example, a 68- $\mu\text{F}$  capacitor with an 8- $\Omega$  speaker would attenuate low frequencies below 293 Hz. The BTL configuration cancels the dc offsets, which eliminates the need for the blocking capacitors. Low-frequency performance is then limited only by the input network and speaker response. Cost and PCB space are also minimized by eliminating the bulky coupling capacitor.

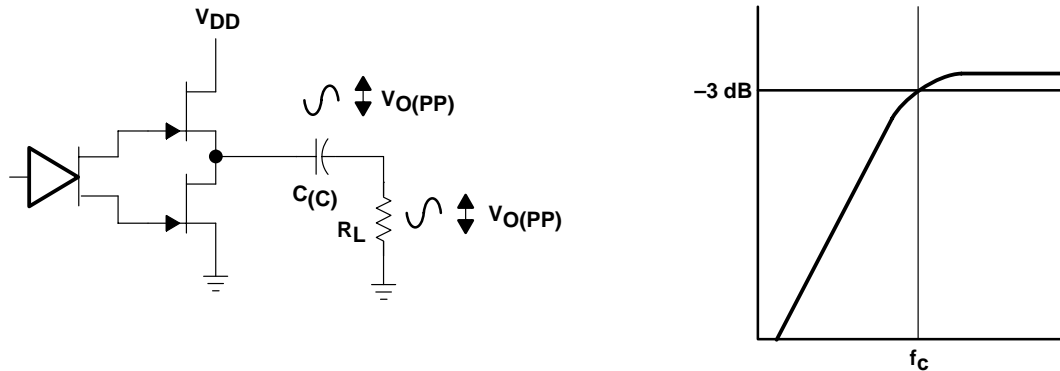


Figure 23. Single-Ended Configuration and Frequency Response

Increasing power to the load does carry a penalty of increased internal power dissipation. The increased dissipation is understandable considering that the BTL configuration produces 4 $\times$  the output power of the SE configuration. Internal dissipation versus output power is discussed further in the *crest factor and thermal considerations* section.

### single-ended operation

In SE mode (see Figure 22 and Figure 23), the load is driven from one amplifier output ( $V_{O+}$ , terminal 5).

The amplifier switches to single-ended operation when the  $\text{SE}/\overline{\text{BTL}}$  terminal is held high.

### BTL amplifier efficiency

Class-AB amplifiers are inefficient. The primary cause of inefficiencies is the voltage drop across the output stage transistors. There are two components of the internal voltage drop. One is the headroom or dc voltage drop that varies inversely to output power. The second component is due to the sinewave nature of the output. The total voltage drop can be calculated by subtracting the RMS value of the output voltage from  $V_{DD}$ . The internal voltage drop multiplied by the RMS value of the supply current,  $I_{DD\text{rms}}$ , determines the internal power dissipation of the amplifier.

An easy-to-use equation to calculate efficiency starts out as being equal to the ratio of power from the power supply to the power delivered to the load. To accurately calculate the RMS and average values of power in the load and in the amplifier, the current and voltage waveform shapes must first be understood (see Figure 24).

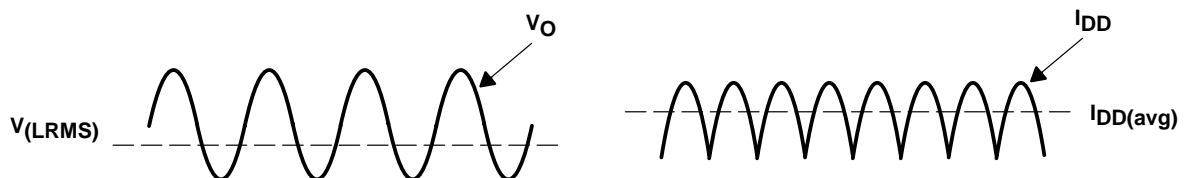


Figure 24. Voltage and Current Waveforms for BTL Amplifiers

## APPLICATION INFORMATION

### BTL amplifier efficiency (continued)

Although the voltages and currents for SE and BTL are sinusoidal in the load, currents from the supply are very different between SE and BTL configurations. In an SE application the current waveform is a half-wave rectified shape, whereas in BTL it is a full-wave rectified waveform. This means RMS conversion factors are different. Keep in mind that for most of the waveform both the push and pull transistors are not on at the same time, which supports the fact that each amplifier in the BTL device only draws current from the supply for half the waveform. The following equations are the basis for calculating amplifier efficiency.

$$\text{Efficiency of a BTL amplifier} = \frac{P_L}{P_{SUP}} \quad (9)$$

Where:

$$P_L = \frac{V_{LRMS}^2}{R_L}, \text{ and } V_{LRMS} = \frac{V_P}{\sqrt{2}}, \text{ therefore, } P_L = \frac{V_P^2}{2R_L}$$

$$\text{and } P_{SUP} = V_{DD} I_{DDavg} \quad \text{and} \quad I_{DDavg} = \frac{1}{\pi} \int_0^{\pi} \frac{V_P}{R_L} \sin(t) dt = \frac{1}{\pi} \times \frac{V_P}{R_L} [\cos(t)]_0^{\pi} = \frac{2V_P}{\pi R_L}$$

Therefore,

$$P_{SUP} = \frac{2 V_{DD} V_P}{\pi R_L}$$

substituting  $P_L$  and  $P_{SUP}$  into equation 9,

$$\text{Efficiency of a BTL amplifier} = \frac{\frac{V_P^2}{2R_L}}{\frac{2 V_{DD} V_P}{\pi R_L}} = \frac{\pi V_P}{4 V_{DD}}$$

Where:

$$V_P = \sqrt{2 P_L R_L}$$

Therefore,

$$\eta_{BTL} = \frac{\pi \sqrt{2 P_L R_L}}{4 V_{DD}} \quad (10)$$

$P_L$  = Power delivered to load  
 $P_{SUP}$  = Power drawn from power supply  
 $V_{LRMS}$  = RMS voltage on BTL load  
 $R_L$  = Load resistance

$V_P$  = Peak voltage on BTL load  
 $I_{DDavg}$  = Average current drawn from the power supply  
 $V_{DD}$  = Power supply voltage  
 $\eta_{BTL}$  = Efficiency of a BTL amplifier



## APPLICATION INFORMATION

### BTL amplifier efficiency (continued)

Table 2 employs equation 10 to calculate efficiencies for four different output power levels. Note that the efficiency of the amplifier is quite low for lower power levels and rises sharply as power to the load is increased resulting in a nearly flat internal power dissipation over the normal operating range. Note that the internal dissipation at full output power is less than in the half power range. Calculating the efficiency for a specific system is the key to proper power supply design.

**Table 2. Efficiency Vs Output Power in 5-V 8-Ω BTL Systems**

Output Power (W)	Efficiency (%)	Peak Voltage (V)	Internal Dissipation (W)
0.25	31.4	2.00	0.55
0.50	44.4	2.83	0.62
1.00	62.8	4.00	0.59
1.25	70.2	4.47†	0.53

† High peak voltages cause the THD to increase.

A final point to remember about Class-AB amplifiers (either SE or BTL) is how to manipulate the terms in the efficiency equation to utmost advantage when possible. Note that in equation 10,  $V_{DD}$  is in the denominator. This indicates that as  $V_{DD}$  goes down, efficiency goes up.

### crest factor and thermal considerations

Class-AB power amplifiers dissipate a significant amount of heat in the package under normal operating conditions. A typical music CD requires 12 dB to 15 dB of dynamic range, or headroom above the average power output, to pass the loudest portions of the signal without distortion. In other words, music typically has a crest factor between 12 dB and 15 dB. When determining the optimal ambient operating temperature, the internal dissipated power at the average output power level must be used. From the TPA0211 data sheet, one can see that when the TPA0211 is operating from a 5-V supply into a 4-Ω speaker 4-W peaks are available. Converting watts to dB:

$$P_{dB} = 10 \log \frac{P_W}{P_{ref}} = 10 \log \frac{4 \text{ W}}{1 \text{ W}} = 6 \text{ dB} \quad (11)$$

Subtracting the headroom restriction to obtain the average listening level without distortion yields:

- 6 dB – 15 dB = –9 dB (15-dB crest factor)
- 6 dB – 12 dB = –6 dB (12-dB crest factor)
- 6 dB – 9 dB = –3 dB (9-dB crest factor)
- 6 dB – 6 dB = 0 dB (6-dB crest factor)
- 6 dB – 3 dB = 3 dB (3-dB crest factor)

# TPA0211

## 2-W MONO AUDIO POWER AMPLIFIER

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### APPLICATION INFORMATION

#### crest factor and thermal considerations (continued)

Converting dB back into watts:

$$P_W = 10^{P_{dB}/10} \times P_{ref} \quad (12)$$

- = 63 mW (18-dB crest factor)
- = 125 mW (15-dB crest factor)
- = 250 mW (9-dB crest factor)
- = 500 mW (6-dB crest factor)
- = 1000 mW (3-dB crest factor)
- = 2000 mW (15-dB crest factor)

This is valuable information to consider when attempting to estimate the heat dissipation requirements for the amplifier system. Comparing the absolute worst case, which is 2 W of continuous power output with a 3 dB crest factor, against 12 dB and 15 dB applications drastically affects maximum ambient temperature ratings for the system. Using the power dissipation curves for a 5-V, 4-Ω system, the internal dissipation in the TPA0211 and maximum ambient temperatures is shown in Table 3.

**Table 3. TPA0211 Power Rating, 5-V, 4-Ω, Mono**

PEAK OUTPUT POWER (W)	AVERAGE OUTPUT POWER	POWER DISSIPATION (W)	MAXIMUM AMBIENT TEMPERATURE
4	2 W (3-dB crest factor)	1.7	–3°C
4	1000 mW (6-dB crest factor)	1.6	6°C
4	500 mW (9-dB crest factor)	1.4	24°C
4	250 mW (12-dB crest factor)	1.1	51°C
4	125 mW (15-dB crest factor)	0.8	78°C
4	63 mW (18-dB crest factor)	0.6	96°C

As a result, this simple formula for calculating  $P_{Dmax}$  may be used for an 4-Ω application:

$$P_{Dmax} = \frac{2V_{DD}^2}{\pi^2 R_L} \quad (13)$$

However, in the case of a 4-Ω load, the  $P_{Dmax}$  occurs at a point well above the normal operating power level. The amplifier may therefore be operated at a higher ambient temperature than required by the  $P_{Dmax}$  formula for a 4-Ω load.

The maximum ambient temperature depends on the heat sinking ability of the PCB system. The derating factor for the DGN package is shown in the dissipation rating table. Converting this to  $\Theta_{JA}$ :

$$\Theta_{JA} = \frac{1}{\text{Derating Factor}} = \frac{1}{0.0171} = 58.48^\circ\text{C/W} \quad (14)$$

## APPLICATION INFORMATION

### crest factor and thermal considerations (continued)

To calculate maximum ambient temperatures, first consider that the numbers from the dissipation graphs are per channel so the dissipated power needs to be doubled for two channel operation. Given  $\Theta_{JA}$ , the maximum allowable junction temperature, and the total internal dissipation, the maximum ambient temperature can be calculated with the following equation. The maximum recommended junction temperature for the TPA0211 is 150°C. The internal dissipation figures are taken from the Power Dissipation vs Output Power graphs.

$$T_A \text{ Max} = T_J \text{ Max} - \Theta_{JA} P_D = 150 - 58.48(0.8 \times 2) = 56^\circ\text{C} \text{ (15-dB crest factor)} \quad (15)$$

**NOTE:**

Internal dissipation of 0.8 W is estimated for a 2-W system with 15-dB crest factor per channel.

Table 3 shows that for some applications no airflow is required to keep junction temperatures in the specified range. The TPA0211 is designed with thermal protection that turns the device off when the junction temperature surpasses 150°C to prevent damage to the IC. Table 3 was calculated for maximum listening volume without distortion. When the output level is reduced the numbers in the table change significantly. Also, using 8-Ω speakers dramatically increases the thermal performance by increasing amplifier efficiency.

### SE/BTL (stereo/mono) operation

The ability of the TPA0211 to easily switch between mono BTL and stereo SE modes is one of its most important cost saving features. This feature eliminates the requirement for an additional headphone amplifier in applications where an internal speaker is driven in BTL mode but an external headphone must be accommodated. When SE/BTL is held high for SE mode, the  $V_{O-}$  output goes into a high impedance state while the  $V_{O+}$  output operates normally. When SE/BTL is held low, the  $V_{O-}$  output operates normally, placing the amplifier in BTL mode.

# TPA0211

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### APPLICATION INFORMATION

#### ST/BTL operation (continued)

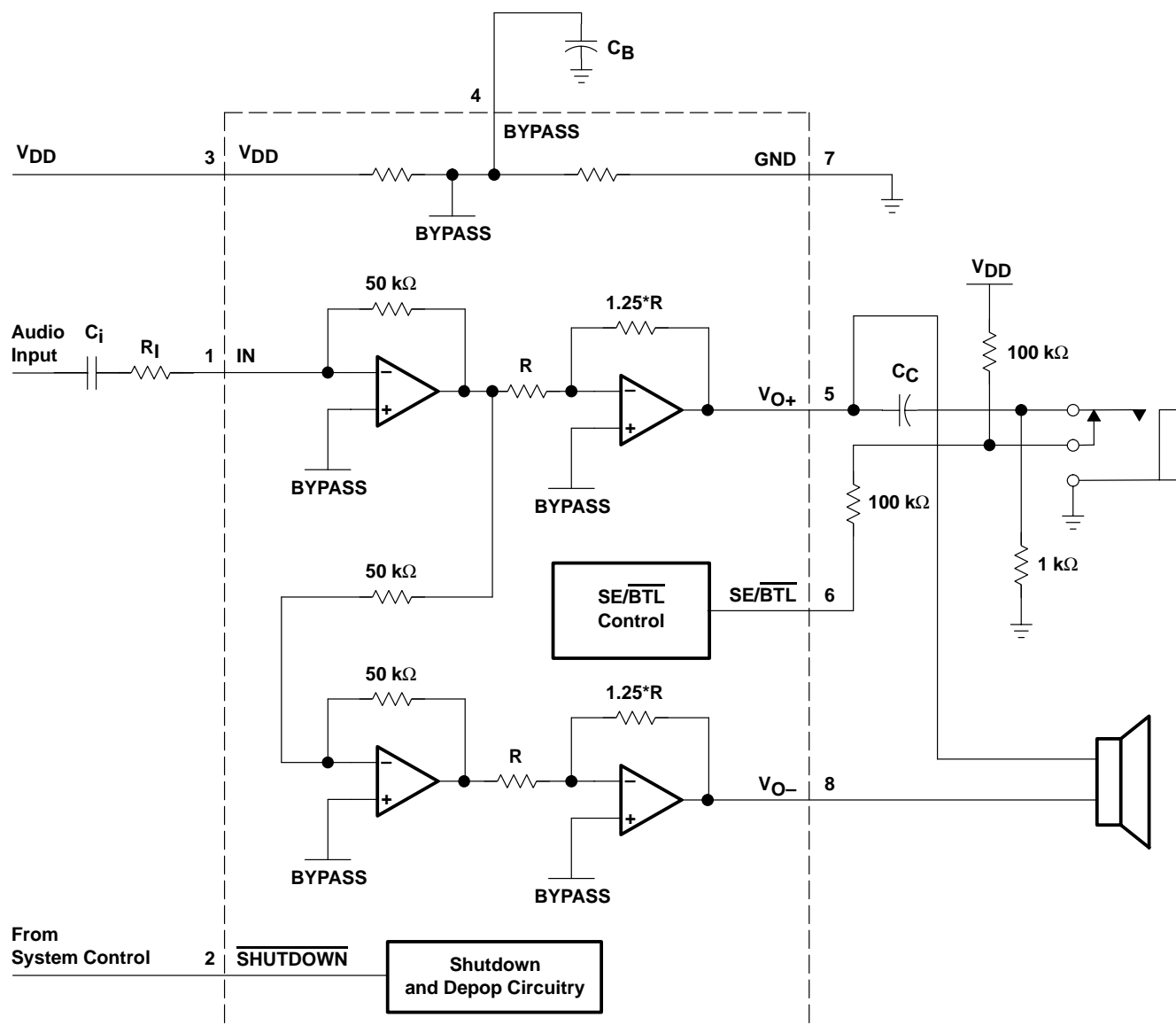


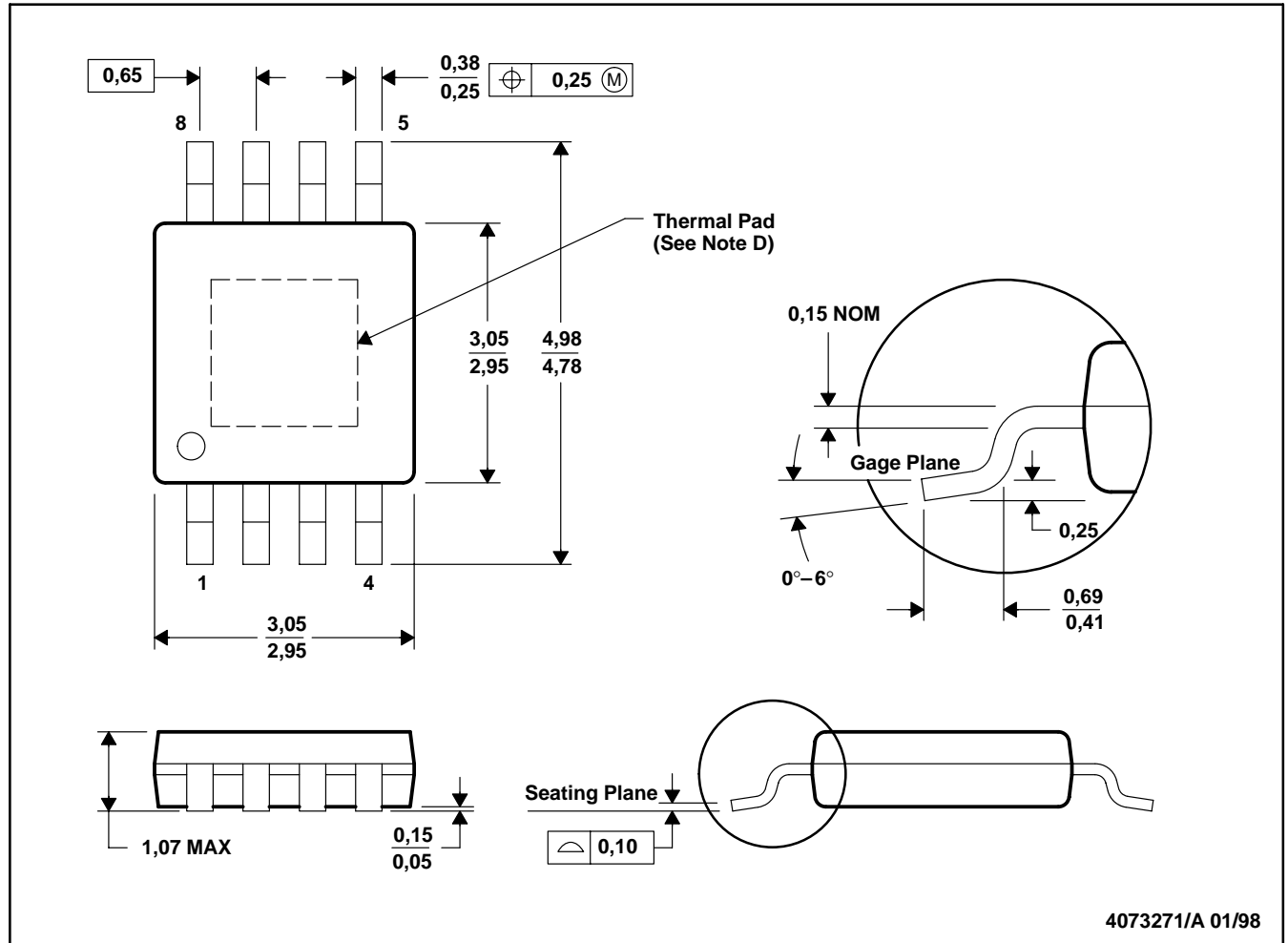
Figure 25. TPA0211 Resistor Divider Network Circuit

Using a readily available 1/8-in. (3.5 mm) mono headphone jack, the control switch is closed when no plug is inserted. When closed, the 100-kΩ/1-kΩ divider pulls the SE/BTL input low. When a plug is inserted, the 1-kΩ resistor is disconnected and the SE/BTL input is pulled high.

MECHANICAL DATA

DGN (S-PDSO-G8)

PowerPAD™ PLASTIC SMALL-OUTLINE PACKAGE



- NOTES:
- A. All linear dimensions are in millimeters.
  - B. This drawing is subject to change without notice.
  - C. Body dimensions include mold flash or protrusions.
  - D. The package thermal performance may be enhanced by attaching an external heat sink to the thermal pad. This pad is electrically and thermally connected to the backside of the die and possibly selected leads. The dimension of the thermal pad is 1.40 mm (height as illustrated) × 1.80 (width as illustrated) mm (maximum). The pad is centered on the bottom of the package.
  - E. Falls within JEDEC MO-187

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