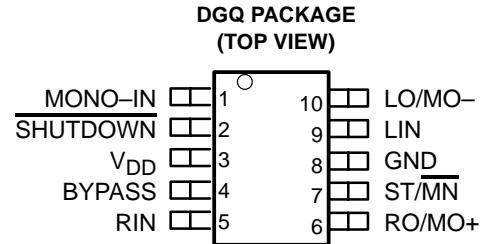


TPA0213

2-W MONO AUDIO POWER AMPLIFIER WITH HEADPHONE DRIVE

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- Ideal for Notebook Computers, PDAs, and Other Small Portable Audio Devices
- 2 W Into 4 Ω From 5-V Supply
- 0.6 W Into 4 Ω From 3-V Supply
- Stereo Headphone Drive
- Separate Inputs for the Mono (BTL) Signal, and Stereo (SE) Left/Right Signals
- Wide Power Supply Compatibility 2.5 V to 5.5 V
- Low Supply Current
 - 4.2 mA Typical at 5 V
 - 3.6 mA Typical at 3 V
- Shutdown Control . . . 1 μ A Typical
- Shutdown Pin Is TTL Compatible
- -40°C to 85°C Operating Temperature Range
- Space-Saving, Thermally-Enhanced MSOP Packaging



description

The TPA0213 is a 2-W mono bridge-tied-load (BTL) amplifier designed to drive speakers with as low as 4- Ω impedance. The amplifier can be reconfigured on-the-fly to drive two stereo single-ended (SE) signals into headphones. This makes the device ideal for use in small notebook computers, PDAs, personal digital audio players, anywhere a mono speaker and stereo headphones are required. From a 5-V supply, the TPA0213 can deliver 2-W of power into a 4- Ω speaker.

The gain of the input stage is set by the user-selected input resistor and a 50-k Ω internal feedback resistor ($A_V = -R_F/R_I$). The power stage is internally configured with a gain of -1.25 V/V in SE mode, and -2.5 V/V in BTL mode. Thus, the overall gain of the amplifier is -62.5 k Ω/R_I in SE mode and -125 k Ω/R_I in BTL mode.

The TPA0213 is available in the 10-pin thermally-enhanced MSOP package (DGQ) and operates over an ambient temperature range of -40°C to 85°C .

AVAILABLE OPTIONS

T _A	PACKAGED DEVICES	MSOP SYMBOLIZATION
	MSOP† (DGQ)	
-40°C to 85°C	TPA0213DGQ	AEH

† The DGQ package are available taped and reeled. To order a taped and reeled part, add the suffix R to the part number (e.g., TPA0213DGQR).



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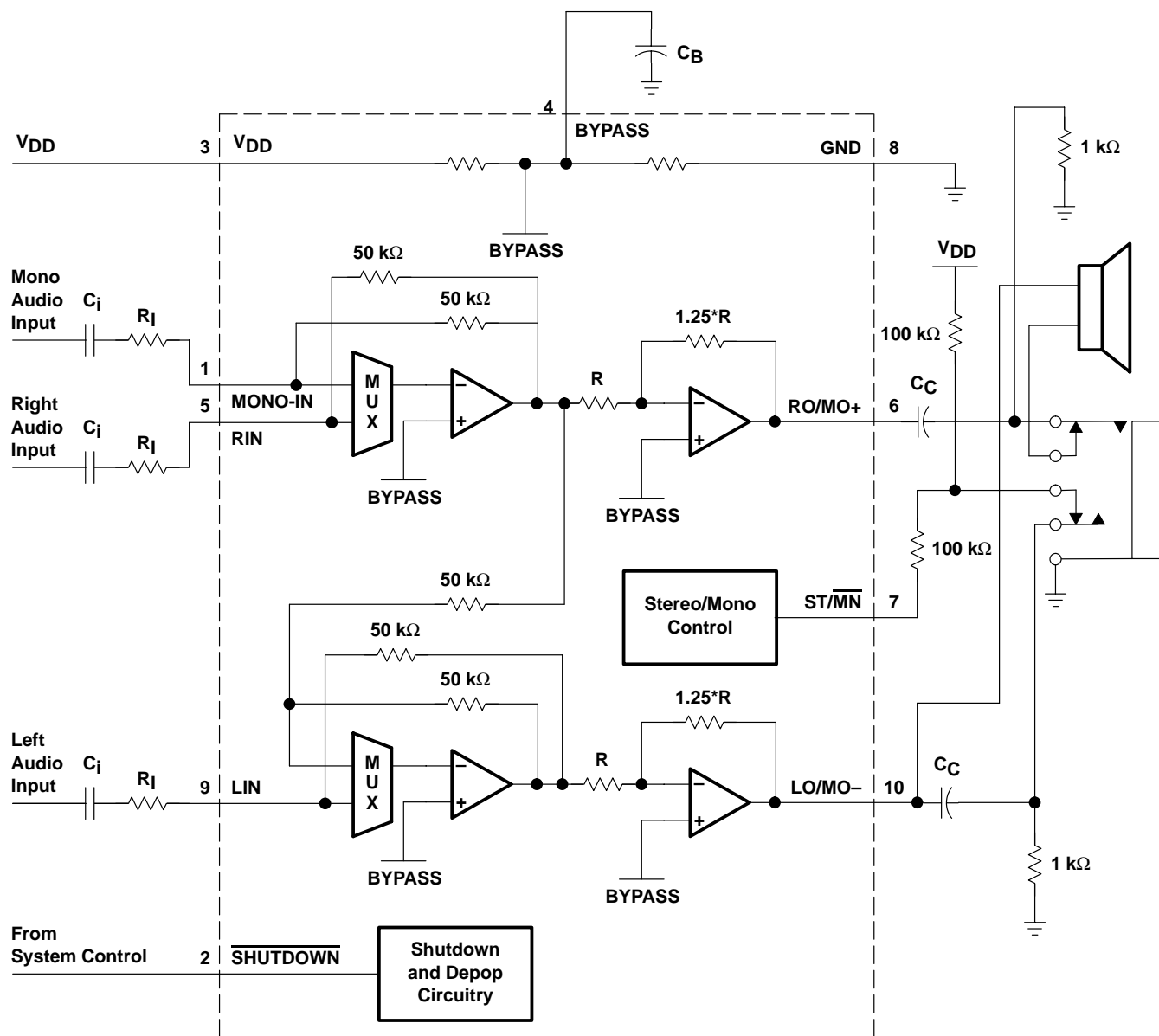
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functional block diagram



Terminal Functions

TERMINAL NAME	NO.	I/O	DESCRIPTION
MONO-IN	1	I	Mono input terminal
SHUTDOWN	2	I	SHUTDOWN places the entire device in shutdown mode when held low. TTL compatible input.
V _{DD}	3	I	V _{DD} is the supply voltage terminal.
BYPASS	4	I	BYPASS is the tap to the voltage divider for internal mid-supply bias. This terminal should be connected to a 0.1-μF to 1-μF capacitor.
RIN	5	I	Right-channel input terminal
RO/MO+	6	O	Right-output in SE mode and mono positive output in BTL mode
ST/MN	7	I	Selects between stereo and mono mode. When held high, the amplifier is in SE stereo mode, while held low, the amplifier is in BTL mono mode.
GND	8		Ground terminal
LIN	9	I	Left-channel input terminal
LO/MO–	10	O	Left-output in SE mode and mono negative output in BTL mode.

absolute maximum ratings over operating free-air temperature range (unless otherwise noted)§

Supply voltage, V _{DD}	6 V
Input voltage, V _I	–0.3 V to V _{DD} +0.3 V
Continuous total power dissipation	internally limited (see Dissipation Rating Table)
Operating free-air temperature range, T _A (see Table 3)	–40°C to 85°C
Operating junction temperature range, T _J	–40°C to 150°C
Storage temperature range, T _{stg}	–65°C to 150°C
Lead temperature 1,6 mm (1/16 inch) from case for 10 seconds	260°C

§ Stresses beyond those listed under “absolute maximum ratings” may cause permanent damage to the device. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those indicated under “recommended operating conditions” is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

DISSIPATION RATING TABLE

PACKAGE	T _A ≤ 25°C	DERATING FACTOR	T _A = 70°C	T _A = 85°C
DGQ	2.14 W [¶]	17.1 mW/°C	1.37 W	1.11 W

[¶] Please see the Texas Instruments document, *PowerPAD Thermally Enhanced Package Application Report* (literature number SLMA002), for more information on the PowerPAD package. The thermal data was measured on a PCB layout based on the information in the section entitled *Texas Instruments Recommended Board for PowerPAD* on page 33 of the before mentioned document.

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recommended operating conditions

			MIN	MAX	UNIT
Supply voltage, V_{DD}			2.5	5.5	V
High-level input voltage, V_{IH}	ST/MN	$V_{DD} = 3\text{ V}$	2.7		V
		$V_{DD} = 5\text{ V}$	4.5		
	SHUTDOWN		2		
Low-level input voltage, V_{IL}	ST/MN	$V_{DD} = 3\text{ V}$		1.65	V
		$V_{DD} = 5\text{ V}$		2.75	
	SHUTDOWN			0.8	
Operating free-air temperature, T_A			-40	85	°C

electrical characteristics at specified free-air temperature, $V_{DD} = 3\text{ V}$, $T_A = 25^\circ\text{C}$ (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
$ V_{OO} $	Output offset voltage (measured differentially)	$V_{IO} = 0$, Gain = 8 dB			30	mV
PSRR	Power supply rejection ratio	$V_{DD} = 2.9\text{ V}$ to 3.1 V , BTL mode		65		dB
$ I_{IH} $	High-level input current	$V_{DD} = 3.3\text{ V}$, $V_I = V_{DD}$			1	μA
$ I_{IL} $	Low-level input current	$V_{DD} = 3.3\text{ V}$, $V_I = 0$			1	μA
z_i	Input impedance			50		k Ω
I_{DD}	Supply current			3.6	5.5	mA
$I_{DD(SD)}$	Supply current, shutdown mode			1	10	μA

operating characteristics, $V_{DD} = 3\text{ V}$, $T_A = 25^\circ\text{C}$, $R_L = 4\text{ }\Omega$, $f = 1\text{ kHz}$ (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
P_O	Output power, see Note 1	THD = 1%, BTL mode		660		mW
		THD = 0.1%, SE mode, $R_L = 32\text{ }\Omega$		33		
THD + N	Total harmonic distortion plus noise	$P_O = 500\text{ mW}$, $f = 20\text{ Hz}$ to 20 kHz		0.2%		
BOM	Maximum output power bandwidth	Gain = 8 dB, THD = 2%		20		kHz
Supply ripple rejection ratio		$f = 1\text{ kHz}$, $CB = 0.47\text{ }\mu\text{F}$	BTL mode	52		dB
			SE mode	62		
V_n	Noise output voltage	$CB = 0.47\text{ }\mu\text{F}$, $f = 20\text{ Hz}$ to 20 kHz	BTL mode	42		μVRMS
			SE mode	21		

NOTE 1: Output power is measured at the output terminals of the device at $f = 1\text{ kHz}$.



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electrical characteristics at specified free-air temperature, $V_{DD} = 5\text{ V}$, $T_A = 25^\circ\text{C}$ (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
$ V_{OO} $	Output offset voltage (measured differentially)	$V_{IO} = 0$, Gain = 8 dB			30	mV
PSRR	Power supply rejection ratio	$V_{DD} = 4.9\text{ V to } 5.1\text{ V}$, BTL mode		62		dB
$ I_{IH} $	High-level input current	$V_{DD} = 5.5\text{ V}$, $V_I = V_{DD}$			1	μA
$ I_{IL} $	Low-level input current	$V_{DD} = 5.5\text{ V}$, $V_I = 0$			1	μA
z_i	Input impedance			50		$\text{k}\Omega$
I_{DD}	Supply current			4.2	6.3	mA
$I_{DD}(\text{SD})$	Supply current, shutdown mode			1	10	μA

operating characteristics, $V_{DD} = 5\text{ V}$, $T_A = 25^\circ\text{C}$, $R_L = 4\ \Omega$

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
P_O	Output power, see Note 1	THD = 0.3%, BTL mode		2		W
		THD = 0.1%, SE mode, $R_L = 32\ \Omega$		90		mW
THD + N	Total harmonic distortion plus noise	$P_O = 1.5\text{ W}$, $f = 20\text{ Hz to } 20\text{ kHz}$		0.2%		
B_{OM}	Maximum output power bandwidth	Gain = 6 dB, THD = 2%		20		kHz
	Supply ripple rejection ratio	$f = 1\text{ kHz}$, $CB = 0.47\ \mu\text{F}$	BTL mode	52		dB
			SE mode	62		
V_n	Noise output voltage	$CB = 0.47\ \mu\text{F}$, $f = 20\text{ Hz to } 20\text{ kHz}$	BTL mode	42		μV_{RMS}
			SE mode	21		

NOTE 1: Output power is measured at the output terminals of the device at $f = 1\text{ kHz}$.

TYPICAL CHARACTERISTICS

Table of Graphs

		FIGURE
THD+N	Total harmonic distortion plus noise	vs Output power
		1, 3, 5, 6, 8, 10
V_n	Output noise voltage	vs Frequency
		2, 4, 7, 9
	Power supply rejection ratio	vs Frequency
		11
		12, 13



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TYPICAL CHARACTERISTICS

TOTAL HARMONIC DISTORTION + NOISE
vs
OUTPUT POWER

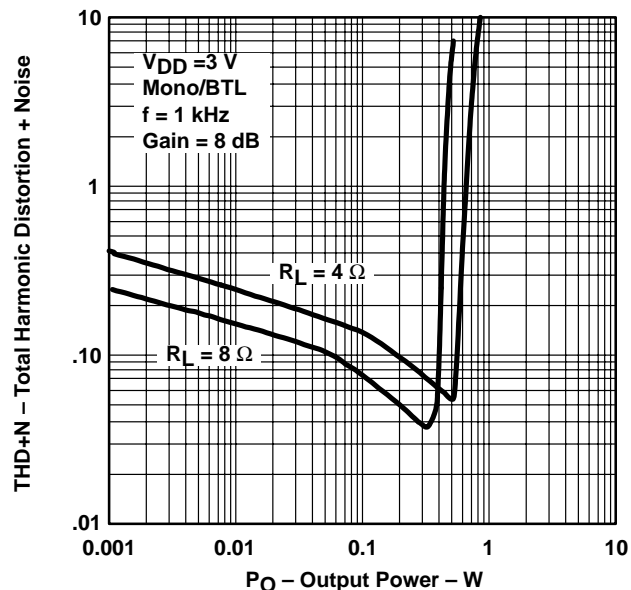


Figure 1

TOTAL HARMONIC DISTORTION + NOISE
vs
FREQUENCY

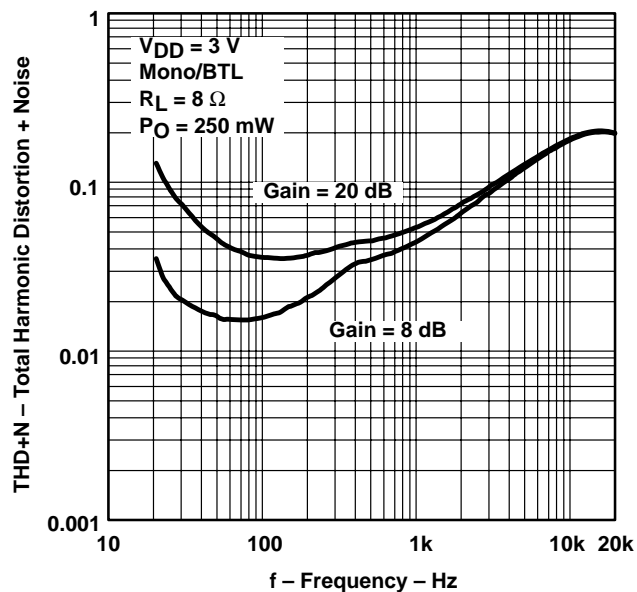


Figure 2

TOTAL HARMONIC DISTORTION + NOISE
vs
OUTPUT POWER

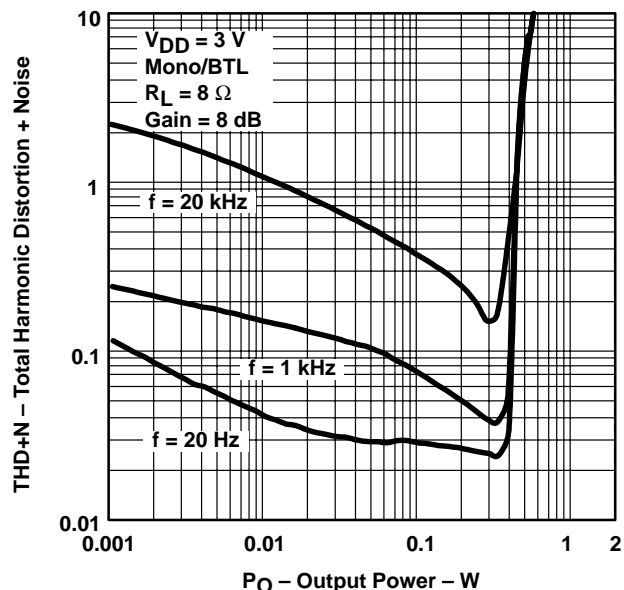


Figure 3

TOTAL HARMONIC DISTORTION + NOISE
vs
FREQUENCY

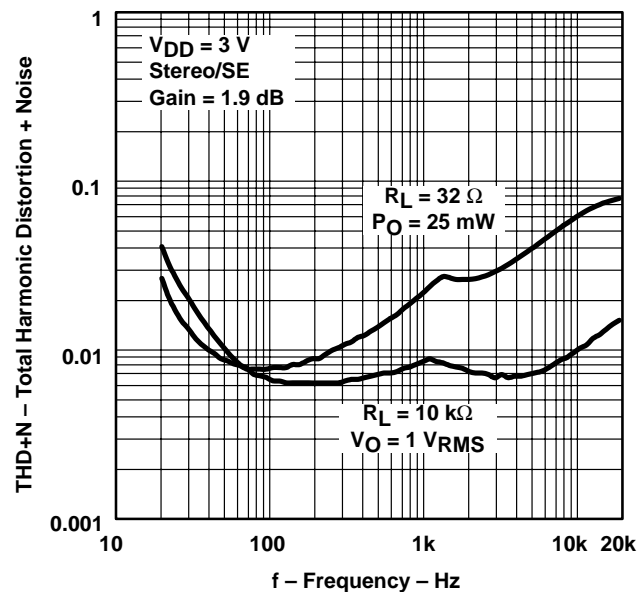


Figure 4

TYPICAL CHARACTERISTICS

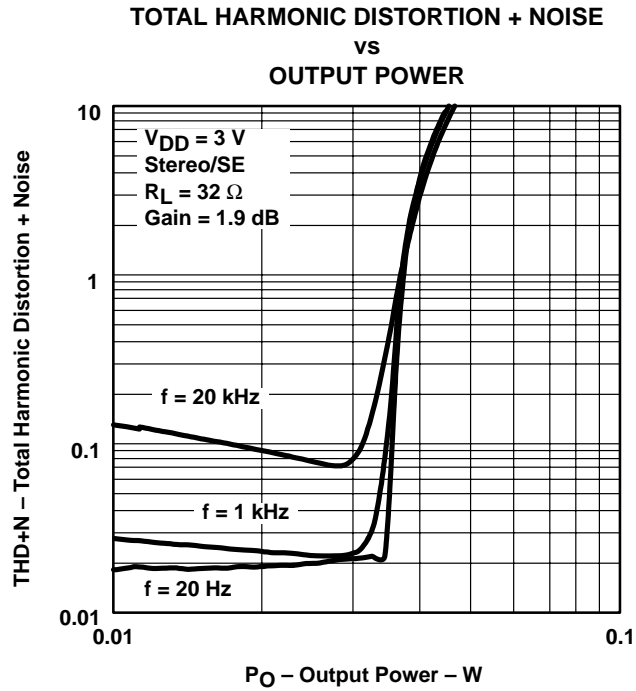


Figure 5

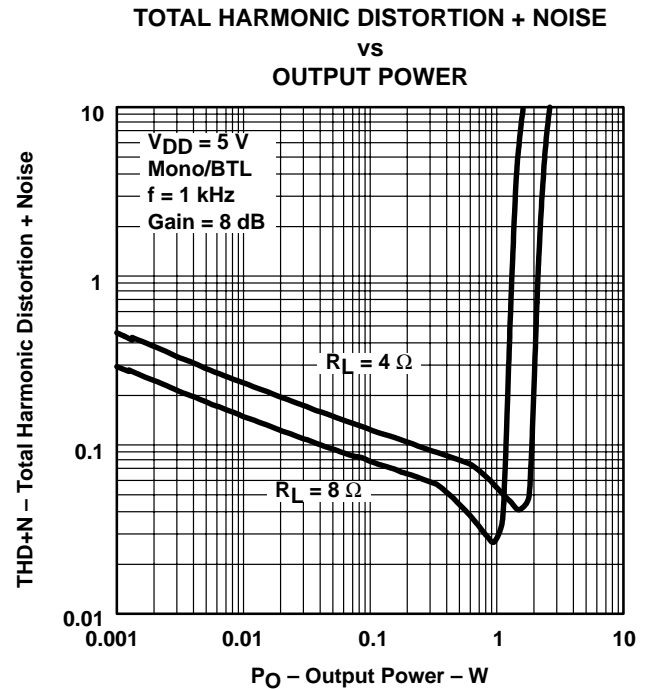


Figure 6

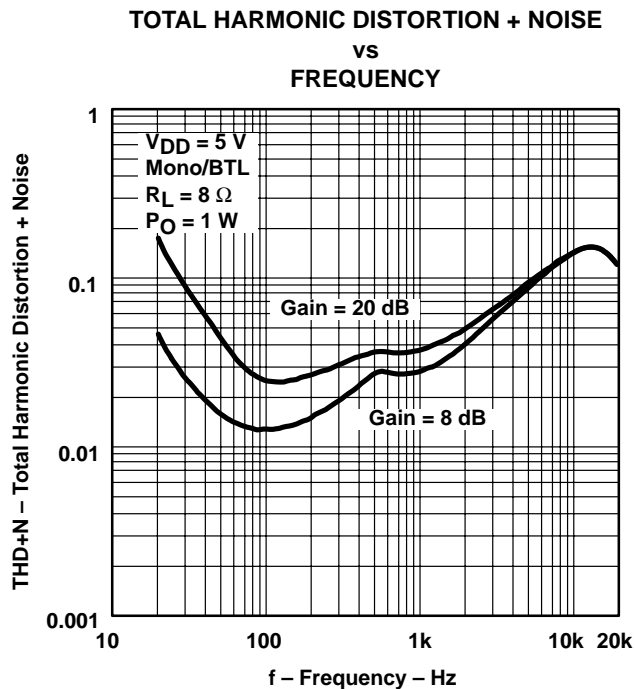


Figure 7

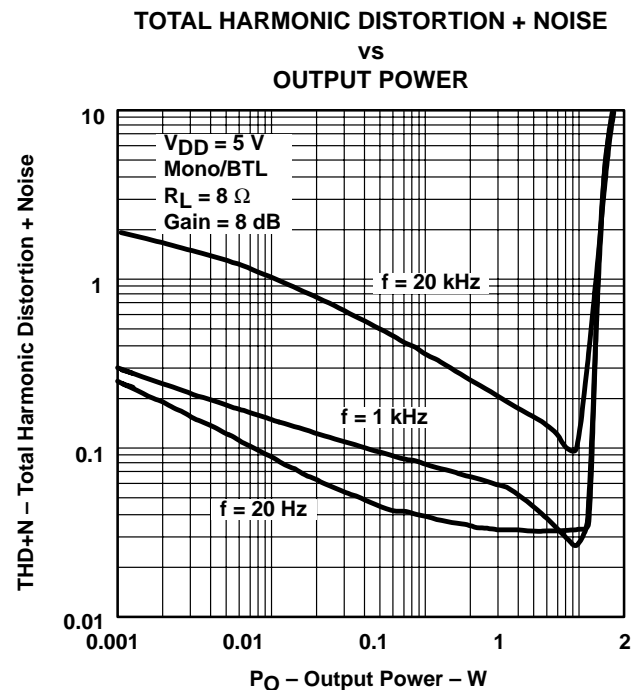


Figure 8

TPA0213

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TYPICAL CHARACTERISTICS

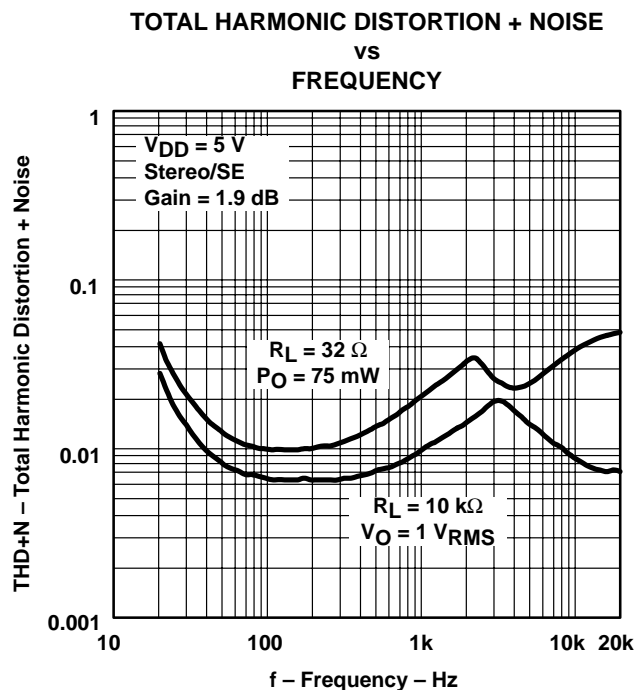


Figure 9

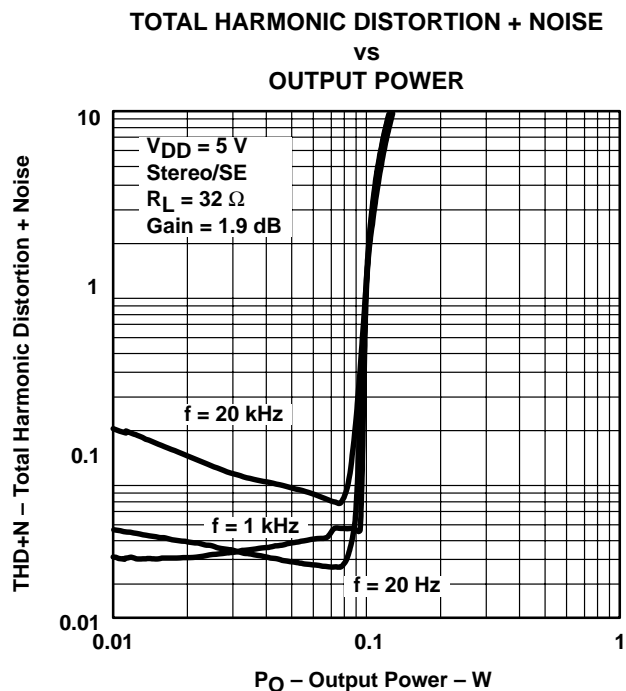


Figure 10

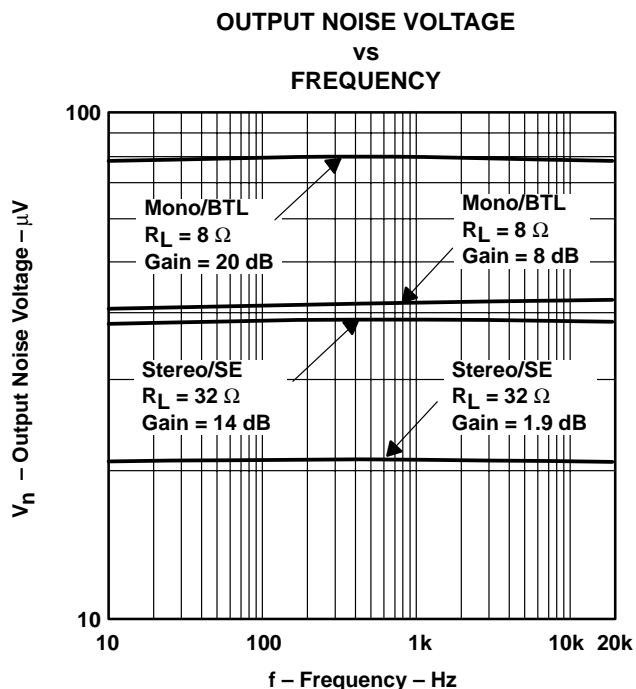


Figure 11

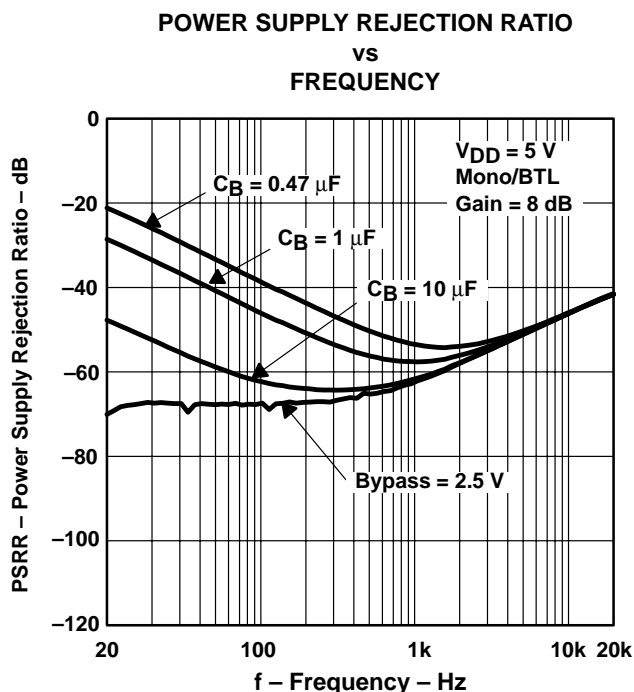
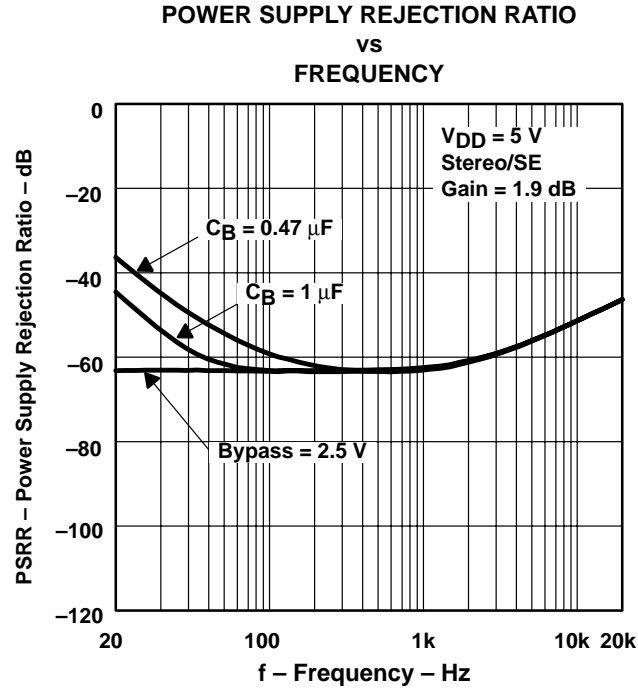


Figure 12

TYPICAL CHARACTERISTICS



APPLICATION INFORMATION

gain setting via input resistance

The gain of the input stage is set by the user-selected input resistor and a 50-k Ω internal feedback resistor.

However, the power stage is internally configured with a gain of -1.25 V/V in SE mode, and -2.5 V/V in BTL mode. Thus, the feedback resistor (R_F) is effectively 62.5 k Ω in SE mode and 125 k Ω in BTL mode. Therefore, the overall gain can be calculated using equations (1) and (2).

$$A_V = \frac{-125 \text{ k}\Omega}{R_I} \quad (\text{BTL}) \quad (1)$$

$$A_V = \frac{-62.5 \text{ k}\Omega}{R_I} \quad (\text{SE}) \quad (2)$$

The -3 dB frequency can be calculated using equation 3:

$$f_{-3 \text{ dB}} = \frac{1}{2\pi R_I C_i} \quad (3)$$

If the filter must be more accurate, the value of the capacitor should be increased while the value of the resistor to ground should be decreased. In addition, the order of the filter could be increased.

TPA0213

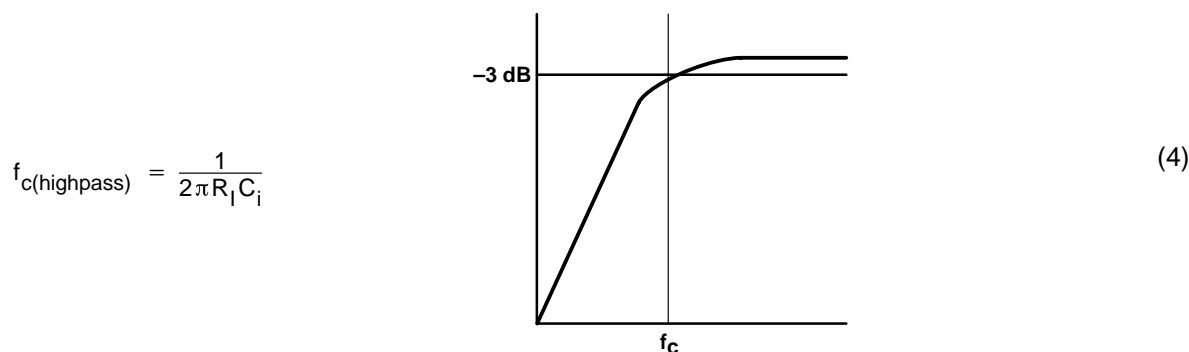
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APPLICATION INFORMATION

input capacitor, C_i

In the typical application an input capacitor, C_i , is required to allow the amplifier to bias the input signal to the proper dc level for optimum operation. In this case, C_i and the input resistance of the amplifier, R_i , form a high-pass filter with the corner frequency determined in equation 4.



The value of C_i is important to consider as it directly affects the bass (low frequency) performance of the circuit. Consider the example where R_i is 710 k Ω and the specification calls for a flat bass response down to 40 Hz. Equation 2 is reconfigured as equation 5.

$$C_i = \frac{1}{2\pi R_i f_c} \quad (5)$$

In this example, C_i is 5.6 nF so one would likely choose a value in the range of 5.6 nF to 1 μ F. A further consideration for this capacitor is the leakage path from the input source through the input network (C_i) and the feedback network to the load. This leakage current creates a dc offset voltage at the input to the amplifier that reduces useful headroom, especially in high gain applications. For this reason a low-leakage tantalum or ceramic capacitor is the best choice. When polarized capacitors are used, the positive side of the capacitor should face the amplifier input in most applications as the dc level there is held at $V_{DD}/2$, which is likely higher than the source dc level. Note that it is important to confirm the capacitor polarity in the application.

power supply decoupling, $C(s)$

The TPA0213 is a high-performance CMOS audio amplifier that requires adequate power supply decoupling to ensure the output total harmonic distortion (THD) is as low as possible. Power supply decoupling also prevents oscillations for long lead lengths between the amplifier and the speaker. The optimum decoupling is achieved by using two capacitors of different types that target different types of noise on the power supply leads. For higher frequency transients, spikes, or digital hash on the line, a good low equivalent-series-resistance (ESR) ceramic capacitor, typically 0.1 μ F placed as close as possible to the device V_{DD} lead, works best. For filtering lower-frequency noise signals, a larger aluminum electrolytic capacitor of 10 μ F or greater placed near the audio power amplifier is recommended.

midrail bypass capacitor, $C_{(BYP)}$

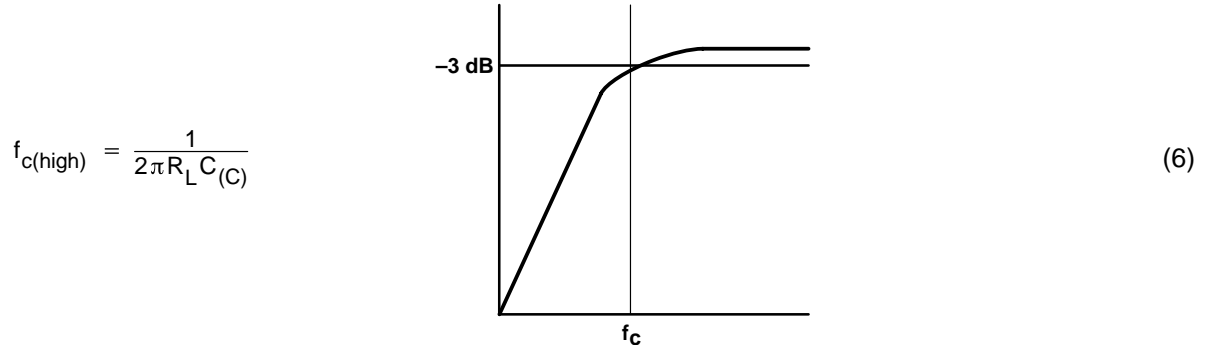
The midrail bypass capacitor, $C_{(BYP)}$, is the most critical capacitor and serves several important functions. During start-up or recovery from shutdown mode, $C_{(BYP)}$ determines the rate at which the amplifier starts up. The second function is to reduce noise produced by the power supply caused by coupling into the output drive signal. This noise is from the midrail generation circuit internal to the amplifier, which appears as degraded PSRR and THD+N.

Bypass capacitor, $C_{(BYP)}$, values of 0.47 μ F to 1 μ F ceramic or tantalum low-ESR capacitors are recommended for the best THD and noise performance.

APPLICATION INFORMATION

output coupling capacitor, $C_{(C)}$

In the typical single-supply SE configuration, an output coupling capacitor ($C_{(C)}$) is required to block the dc bias at the output of the amplifier, thus preventing dc currents in the load. As with the input coupling capacitor, the output coupling capacitor and impedance of the load form a high-pass filter governed by equation 6.



The main disadvantage, from a performance standpoint, is the load impedances are typically small, which drives the low-frequency corner higher, degrading the bass response. Large values of $C_{(C)}$ are required to pass low frequencies into the load. Consider the example where a $C_{(C)}$ of 330 μF is chosen and loads vary from 3 Ω , 4 Ω , 8 Ω , 32 Ω , 10 k Ω , to 47 k Ω . Table 1 summarizes the frequency response characteristics of each configuration.

Table 1. Common Load Impedances vs Low Frequency Output Characteristics in SE Mode

R_L	$C_{(C)}$	Lowest Frequency
3 Ω	330 μF	161 Hz
4 Ω	330 μF	120 Hz
8 Ω	330 μF	60 Hz
32 Ω	330 μF	15 Hz
10,000 Ω	330 μF	0.05 Hz
47,000 Ω	330 μF	0.01 Hz

As Table 1 indicates, most of the bass response is attenuated into a 4- Ω load, an 8- Ω load is adequate, headphone response is good, and drive into line level inputs (a home stereo for example) is exceptional.

Furthermore, the total amount of ripple current that must flow through the capacitor must be considered when choosing the component. As shown in the application circuit, one coupling capacitor must be in series with the mono loudspeaker for proper operation of the stereo-mono switching circuit. For a 4- Ω load, this capacitor must be able to handle about 700 mA of ripple current for a continuous output power of 2 W.

using low-ESR capacitors

Low-ESR capacitors are recommended throughout this applications section. A real (as opposed to ideal) capacitor can be modeled simply as a resistor in series with an ideal capacitor. The voltage drop across this resistor minimizes the beneficial effects of the capacitor in the circuit. The lower the equivalent value of this resistance the more the real capacitor behaves like an ideal capacitor.

APPLICATION INFORMATION

bridged-tied load versus single-ended mode

Figure 14 shows a Class-AB audio power amplifier (APA) in a BTL configuration. The TPA0213 BTL amplifier consists of two Class-AB amplifiers driving both ends of the load. There are several potential benefits to this differential drive configuration, but initially consider power to the load. The differential drive to the speaker means that as one side is slewing up, the other side is slewing down, and vice versa. This in effect doubles the voltage swing on the load as compared to a ground referenced load. Plugging $2 \times V_{O(PP)}$ into the power equation, where voltage is squared, yields 4x the output power from the same supply rail and load impedance (see equation 7).

$$V_{(RMS)} = \frac{V_{O(PP)}}{2\sqrt{2}} \quad (7)$$

$$Power = \frac{V_{(RMS)}^2}{R_L}$$

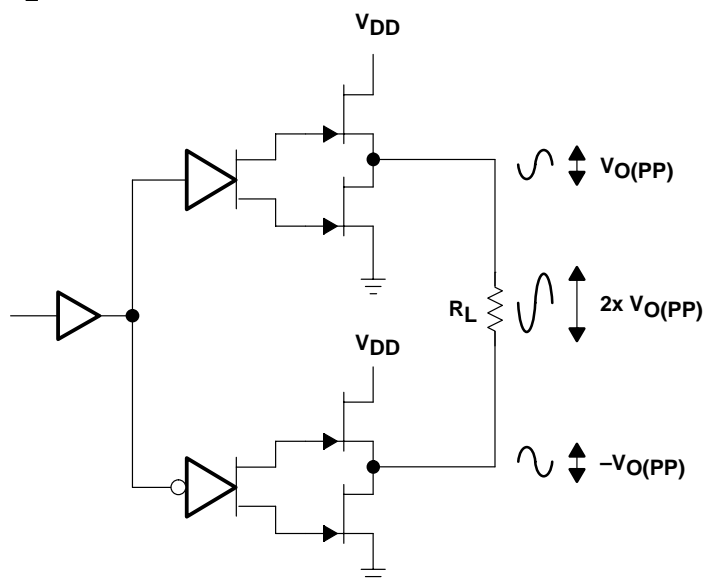


Figure 14. Bridge-Tied Load Configuration

In a typical computer sound channel operating at 5 V, bridging raises the power into an 8-Ω speaker from a singled-ended (SE, ground reference) limit of 250 mW to 1 W. In sound power, that is a 6-dB improvement—which is loudness that can be heard. In addition to increased power, there are frequency response concerns. Consider the single-supply SE configuration shown in Figure 15. A coupling capacitor is required to block the dc offset voltage from reaching the load. These capacitors can be quite large (approximately 33 μF to 1000 μF) so they tend to be expensive, heavy, occupy valuable PCB area, and have the additional drawback of limiting low-frequency performance of the system. This frequency limiting effect is due to the high pass filter network created with the speaker impedance and the coupling capacitance and is calculated with equation 8.

$$f_c = \frac{1}{2\pi R_L C(C)} \quad (8)$$

APPLICATION INFORMATION

bridged-tied load versus single-ended mode (continued)

For example, a 68- μF capacitor with an 8- Ω speaker would attenuate low frequencies below 293 Hz. The BTL configuration cancels the dc offsets, which eliminates the need for the blocking capacitors. Low-frequency performance is then limited only by the input network and speaker response. Cost and PCB space are also minimized by eliminating the bulky coupling capacitor.

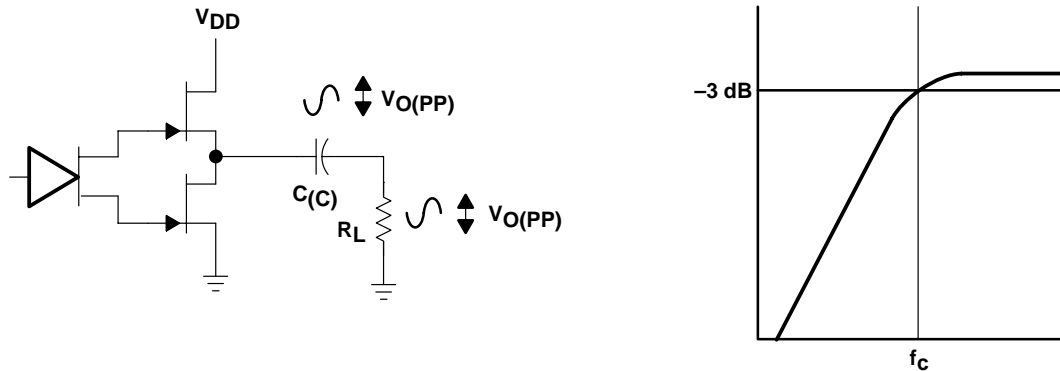


Figure 15. Single-Ended Configuration and Frequency Response

Increasing power to the load does carry a penalty of increased internal power dissipation. The increased dissipation is understandable considering that the BTL configuration produces 4 \times the output power of the SE configuration. Internal dissipation versus output power is discussed further in the *crest factor and thermal considerations* section.

single-ended operation

In SE mode (see Figure 14 and Figure 15), the load is driven from the primary amplifier output for each channel (LO and RO, terminals 6 and 10)

The amplifier switches to single-ended operation when the $\text{ST}/\overline{\text{MN}}$ terminal is held high.

input MUX operation

The input MUX allows two separate inputs to be applied to the amplifier. When the $\text{ST}/\overline{\text{MN}}$ terminal is held high, the headphone inputs (LIN and RIN) are active. When the $\text{ST}/\overline{\text{MN}}$ terminal is held low, the line BTL input (MONO-IN) is active.

BTL amplifier efficiency

Class-AB amplifiers are inefficient. The primary cause of inefficiencies is the voltage drop across the output stage transistors. There are two components of the internal voltage drop. One is the headroom or dc voltage drop that varies inversely to output power. The second component is due to the sinewave nature of the output. The total voltage drop can be calculated by subtracting the RMS value of the output voltage from V_{DD} . The internal voltage drop multiplied by the RMS value of the supply current, $I_{DD\text{rms}}$, determines the internal power dissipation of the amplifier.

An easy-to-use equation to calculate efficiency starts out as being equal to the ratio of power from the power supply to the power delivered to the load. To accurately calculate the RMS and average values of power in the load and in the amplifier, the current and voltage waveform shapes must first be understood (see Figure 16).

APPLICATION INFORMATION

BTL amplifier efficiency (continued)

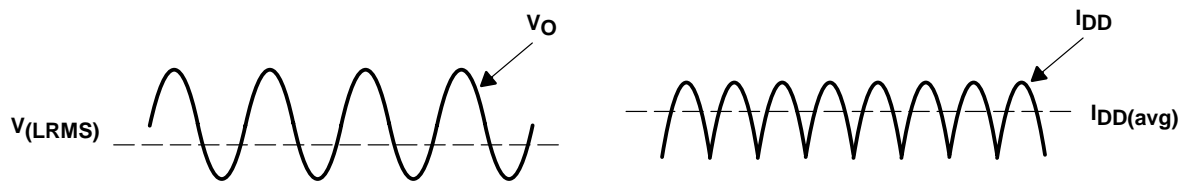


Figure 16. Voltage and Current Waveforms for BTL Amplifiers

Although the voltages and currents for SE and BTL are sinusoidal in the load, currents from the supply are very different between SE and BTL configurations. In an SE application the current waveform is a half-wave rectified shape, whereas in BTL it is a full-wave rectified waveform. This means RMS conversion factors are different. Keep in mind that for most of the waveform both the push and pull transistors are not on at the same time, which supports the fact that each amplifier in the BTL device only draws current from the supply for half the waveform. The following equations are the basis for calculating amplifier efficiency.

$$\text{Efficiency of a BTL amplifier} = \frac{P_L}{P_{SUP}} \quad (9)$$

Where:

$$P_L = \frac{V_{LRMS}^2}{R_L}, \text{ and } V_{LRMS} = \frac{V_P}{\sqrt{2}}, \text{ therefore, } P_L = \frac{V_P^2}{2R_L}$$

$$\text{and } P_{SUP} = V_{DD} I_{DDavg} \quad \text{and} \quad I_{DDavg} = \frac{1}{\pi} \int_0^{\pi} \frac{V_P}{R_L} \sin(t) dt = \frac{1}{\pi} \times \frac{V_P}{R_L} [\cos(t)]_0^{\pi} = \frac{2V_P}{\pi R_L}$$

Therefore,

$$P_{SUP} = \frac{2 V_{DD} V_P}{\pi R_L}$$

substituting P_L and P_{SUP} into equation 9,

$$\text{Efficiency of a BTL amplifier} = \frac{\frac{V_P^2}{2R_L}}{\frac{2 V_{DD} V_P}{\pi R_L}} = \frac{\pi V_P}{4 V_{DD}}$$

Where:

$$V_P = \sqrt{2 P_L R_L}$$

Therefore,

$$\eta_{BTL} = \frac{\pi \sqrt{2 P_L R_L}}{4 V_{DD}} \quad (10)$$

P_L = Power delivered to load
 P_{SUP} = Power drawn from power supply
 V_{LRMS} = RMS voltage on BTL load
 R_L = Load resistance

V_P = Peak voltage on BTL load
 I_{DDavg} = Average current drawn from the power supply
 V_{DD} = Power supply voltage
 η_{BTL} = Efficiency of a BTL amplifier

APPLICATION INFORMATION

BTL amplifier efficiency (continued)

Table 2 employs equation 10 to calculate efficiencies for four different output power levels. Note that the efficiency of the amplifier is quite low for lower power levels and rises sharply as power to the load is increased resulting in a nearly flat internal power dissipation over the normal operating range. Note that the internal dissipation at full output power is less than in the half power range. Calculating the efficiency for a specific system is the key to proper power supply design. For a stereo 1-W audio system with 8-Ω loads and a 5-V supply, the maximum draw on the power supply is almost 3.25 W.

Table 2. Efficiency Vs Output Power in 5-V 8-Ω BTL Systems

Output Power (W)	Efficiency (%)	Peak Voltage (V)	Internal Dissipation (W)
0.25	31.4	2.00	0.55
0.50	44.4	2.83	0.62
1.00	62.8	4.00	0.59
1.25	70.2	4.47 [†]	0.53

[†] High peak voltages cause the THD to increase.

A final point to remember about Class-AB amplifiers (either SE or BTL) is how to manipulate the terms in the efficiency equation to utmost advantage when possible. Note that in equation 10, V_{DD} is in the denominator. This indicates that as V_{DD} goes down, efficiency goes up.

crest factor and thermal considerations

Class-AB power amplifiers dissipate a significant amount of heat in the package under normal operating conditions. A typical music CD requires 12 dB to 15 dB of dynamic range, or headroom above the average power output, to pass the loudest portions of the signal without distortion. In other words, music typically has a crest factor between 12 dB and 15 dB. When determining the optimal ambient operating temperature, the internal dissipated power at the average output power level must be used. From the TPA0213 data sheet, one can see that when the TPA0213 is operating from a 5-V supply into a 4-Ω speaker 4-W peaks are available. Converting watts to dB:

$$P_{dB} = 10 \log \frac{P_W}{P_{ref}} = 10 \log \frac{4 \text{ W}}{1 \text{ W}} = 6 \text{ dB} \quad (11)$$

Subtracting the headroom restriction to obtain the average listening level without distortion yields:

- 6 dB – 15 dB = –9 dB (15-dB crest factor)
- 6 dB – 12 dB = –6 dB (12-dB crest factor)
- 6 dB – 9 dB = –3 dB (9-dB crest factor)
- 6 dB – 6 dB = 0 dB (6-dB crest factor)
- 6 dB – 3 dB = 3 dB (3-dB crest factor)

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APPLICATION INFORMATION

crest factor and thermal considerations (continued)

Converting dB back into watts:

$$P_W = 10^{P_{dB}/10} \times P_{ref} \quad (12)$$

- = 63 mW (18-dB crest factor)
- = 125 mW (15-dB crest factor)
- = 250 mW (12-dB crest factor)
- = 500 mW (9-dB crest factor)
- = 1000 mW (6-dB crest factor)
- = 2000 mW (3-dB crest factor)

This is valuable information to consider when attempting to estimate the heat dissipation requirements for the amplifier system. Comparing the absolute worst case, which is 2 W of continuous power output with a 3 dB crest factor, against 12 dB and 15 dB applications drastically affects maximum ambient temperature ratings for the system. Using the power dissipation curves for a 5-V, 4-Ω system, the internal dissipation in the TPA0213 and maximum ambient temperatures is shown in Table 3.

Table 3. TPA0213 Power Rating, 5-V, 3-Ω, Mono

PEAK OUTPUT POWER (W)	AVERAGE OUTPUT POWER	POWER DISSIPATION (W)	MAXIMUM AMBIENT TEMPERATURE
4	2 W (3-dB crest factor)	1.7	–3°C
4	1000 mW (6-dB crest factor)	1.6	6°C
4	500 mW (9-dB crest factor)	1.4	24°C
4	250 mW (12-dB crest factor)	1.1	51°C
4	125 mW (15-dB crest factor)	0.8	78°C
4	63 mW (18-dB crest factor)	0.6	96°C

Table 4. TPA0213 Power Rating, 5-V, 8-Ω, Stereo

PEAK OUTPUT POWER (W)	AVERAGE OUTPUT POWER	POWER DISSIPATION (W)	MAXIMUM AMBIENT TEMPERATURE
2.5	1250 mW (3-dB crest factor)	0.55	100°C
2.5	1000 mW (4-dB crest factor)	0.62	94°C
2.5	500 mW (7-dB crest factor)	0.59	97°C
2.5	250 mW (10-dB crest factor)	0.53	102°C

The maximum dissipated power, P_{Dmax} , is reached at a much lower output power level for an 4-Ω load than for a 8-Ω load. As a result, this simple formula for calculating P_{Dmax} may be used for a 4-Ω application:

$$P_{Dmax} = \frac{2V_{DD}^2}{\pi^2 R_L} \quad (13)$$

However, in the case of a 8-Ω load, the P_{Dmax} occurs at a point well above the normal operating power level. The amplifier may therefore be operated at a higher ambient temperature than required by the P_{Dmax} formula for a 8-Ω load.

The maximum ambient temperature depends on the heat sinking ability of the PCB system. The derating factor for the DGQ package is shown in the dissipation rating table (see page 4). Converting this to Θ_{JA} :

$$\Theta_{JA} = \frac{1}{\text{Derating Factor}} = \frac{1}{0.0171} = 58.48^\circ\text{C/W} \quad (14)$$



APPLICATION INFORMATION

crest factor and thermal considerations (continued)

To calculate maximum ambient temperatures, first consider that the numbers from the dissipation graphs are per channel so the dissipated power needs to be doubled for two channel operation. Given Θ_{JA} , the maximum allowable junction temperature, and the total internal dissipation, the maximum ambient temperature can be calculated with the following equation. The maximum recommended junction temperature for the TPA0213 is 150°C. The internal dissipation figures are taken from the Power Dissipation vs Output Power graphs.

$$T_A \text{ Max} = T_J \text{ Max} - \Theta_{JA} P_D = 150 - 58.48(0.8 \times 2) = 56^\circ\text{C} \text{ (15-dB crest factor)} \quad (15)$$

NOTE:

Internal dissipation of 0.8 W is estimated for a 2-W system with 15-dB crest factor per channel.

Tables 3 and 4 show that for some applications no airflow is required to keep junction temperatures in the specified range. The TPA0213 is designed with thermal protection that turns the device off when the junction temperature surpasses 150°C to prevent damage to the IC. Tables 3 and 4 were calculated for maximum listening volume without distortion. When the output level is reduced the numbers in the table change significantly. Also, using 8-Ω speakers dramatically increases the thermal performance by increasing amplifier efficiency.

ST/MN (stereo/mono) operation

The ability of the TPA0213 to easily switch between mono BTL and stereo SE modes is one of its most important cost saving features. This feature eliminates the requirement for an additional headphone amplifier in applications where an internal speaker is driven in BTL mode but external stereo headphone or speakers must be accommodated. When $\overline{\text{ST/MN}}$ is held high, the input mux selects the RIN and LIN inputs and the output is in stereo SE mode. When $\overline{\text{ST/MN}}$ is held low, the input mux selects the mono-in input and the output is in mono BTL mode. Control of the $\overline{\text{ST/MN}}$ input can be from a logic-level CMOS source or, more typically, from a switch-controlled resistor divider network as shown in Figure 17.

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ST/MN (stereo/mono) operation (continued)

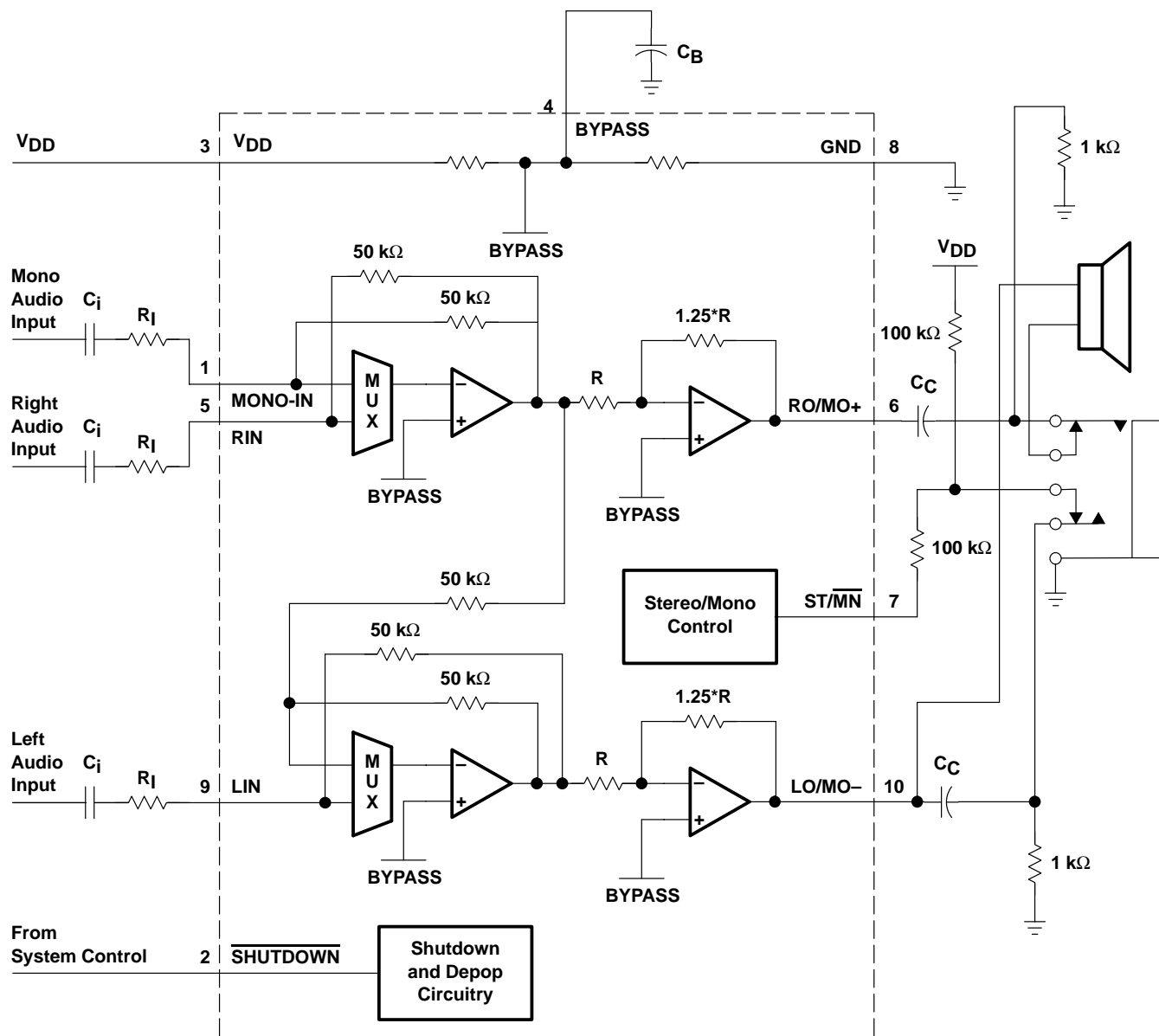


Figure 17. TPA0213 Resistor Divider Network Circuit

Using a readily available 1/8-in. (3.5 mm) stereo headphone jack, the control switch is closed when no plug is inserted. When closed, the 100-kΩ/1-kΩ divider pulls the ST/MN input low. When a plug is inserted, the 1-kΩ resistor is disconnected and the ST/MN input is pulled high. The mono speaker is also physically disconnected from the RO/MO+ output so that no sound is heard from the speaker while the headphones are inserted.

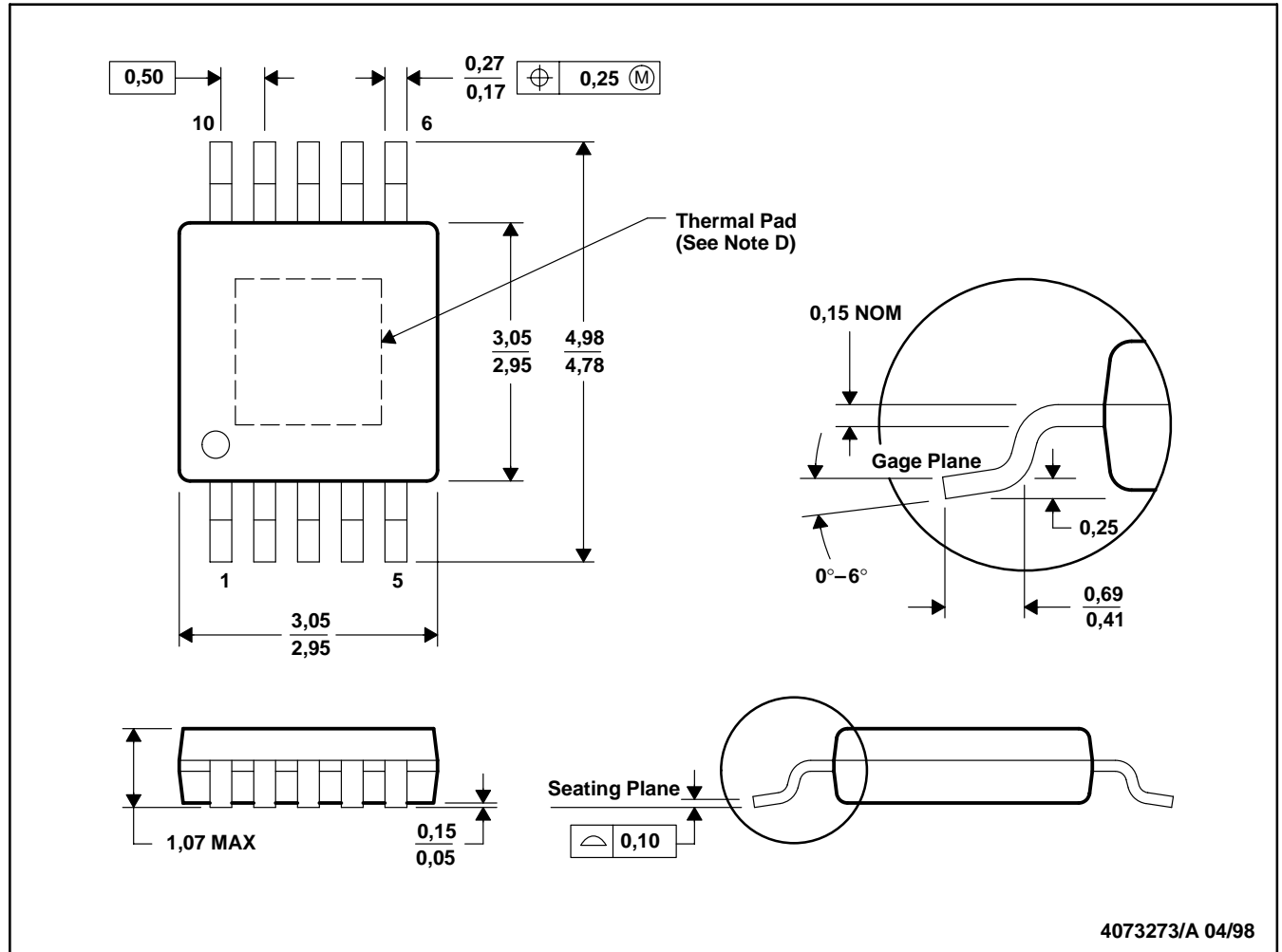
TPA0213
2-W MONO AUDIO POWER AMPLIFIER
WITH HEADPHONE DRIVE

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MECHANICAL DATA

DGQ (S-PDSO-G10)

PowerPAD™ PLASTIC SMALL-OUTLINE PACKAGE



- NOTES:
- All linear dimensions are in millimeters.
 - This drawing is subject to change without notice.
 - Body dimensions do not include mold flash or protrusion.
 - The package thermal performance may be enhanced by bonding the thermal pad to an external thermal plane. This pad is electrically and thermally connected to the backside of the die and possibly selected leads. The dimension of the thermal pad is 1.40 mm (height as illustrated) × 1.80 (width as illustrated) mm (maximum). The pad is centered on the bottom of the package.

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