



FEATURES

- Wide Input Voltage Range: 3V to 60V
- Low Quiescent Current: 6mA
- Internal 5A Switch (2.5A for LT1171, 1.25A for LT1172)
- Very Few External Parts Required
- Self-Protected Against Overloads
- Operates in Nearly All Switching Topologies
- Shutdown Mode Draws Only 50µA Supply Current
- Flyback-Regulated Mode Has Fully Floating Outputs
- Comes in Standard 5-Pin Packages
- LT1172 Available in 8-Pin MiniDIP and Surface Mount Packages
- Can Be Externally Synchronized

APPLICATIONS

- Logic Supply 5V at 10A
- 5V Logic to $\pm 15\text{V}$ Op Amp Supply
- Battery Upconverter
- Power Inverter (+ to -) or (- to +)
- Fully Floating Multiple Outputs

USER NOTE:

This data sheet is only intended to provide specifications, graphs, and a general functional description of the LT1170/LT1171/LT1172. Application circuits are included to show the capability of the LT1170/LT1171/LT1172. A complete design manual (AN91) should be obtained to assist in developing new designs. This manual contains a comprehensive discussion of both the LT1070 and the external components used with it, as well as complete formulas for calculating the values of these components. The manual can also be used for the LT1170/LT1171/LT1172 by factoring in the higher frequency. A CAD design program called SwitcherCAD is also available.

DESCRIPTION

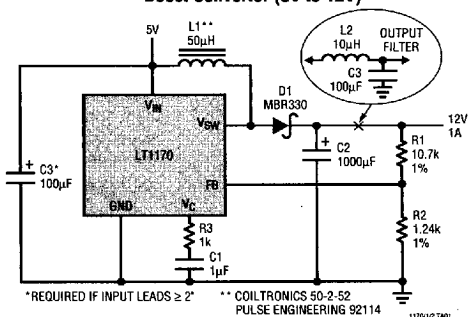
The LT1170/LT1171/LT1172 are monolithic high power switching regulators. They can be operated in all standard switching configurations including buck, boost, flyback, forward, inverting and "Cuk." A high current, high efficiency switch is included on the die along with all oscillator, control, and protection circuitry. Integration of all functions allows the LT1170/LT1171/LT1172 to be built in a standard 5-pin TO-3 or TO-220 power package as well as the 8-pin packages (LT1172). This makes them extremely easy to use and provides "bust proof" operation similar to that obtained with 3-pin linear regulators.

The LT1170/LT1171/LT1172 operate with supply voltages from 3V to 60V, and draw only 6mA quiescent current. They can deliver load power up to 100W with no external power devices. By utilizing current-mode switching techniques, they provide excellent AC and DC load and line regulation.

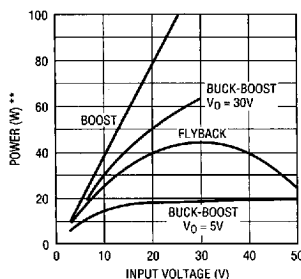
The LT1170/LT1171/LT1172 have many unique features not found even on the vastly more difficult to use low power control chips presently available. They use adaptive anti-sat switch drive to allow very wide ranging load currents with no loss in efficiency. An externally activated shutdown mode reduces total supply current to 50µA typically for standby operation.

TYPICAL APPLICATION

Boost Converter (5V to 12V)



Maximum Output Power*



* ROUGH GUIDE ONLY. BUCK MODE
 $P_{OUT} = 5A \times V_{OUT}$.
 SPECIAL TOPOLOGIES DELIVER
 MORE POWER.

** DIVIDE VERTICAL POWER SCALE
 BY TWO FOR LT1171, BY FOUR
 FOR LT1172.

LEARNING OBJECTS



ABSOLUTE MAXIMUM RATINGS

Supply Voltage	
LT1170/71/72HV	60V
LT1170/71/72 (See Note 1)	40V
Switch Output Voltage	
LT1170/71/72HV	75V
LT1170/71/72	65V
LT1172S8	60V
Feedback Pin Voltage (Transient, 1ms)	
Storage Temperature Range	
Lead Temperature (Soldering, 10 sec)	
Operating Junction Temperature Range	
LT1170/71/72M	-55°C to 150°C
LT1170/71/72HVC,	
LT1170/71/72C (Oper.)	0°C to 100°C
LT1170/71/72HVC,	
LT1170/71/72C (Sh. Ckt.)	0°C to 125°C
LT1170/71/72I (Oper.)	-40°C to 100°C
LT1170/71/72I (Sh. Ckt.)	-40°C to 125°C

Note 1: Minimum effective switch "on" time for the LT1170/71/72 (in current limit only) is $\approx 0.6\mu\text{s}$. This limits the maximum safe input voltage during an output shorted condition. Buck mode and inverting mode input voltage during an output shorted condition is limited to:

$$V_{IN} (\text{max, output shorted}) = 15V + \frac{R \cdot I_L + V_f}{t \cdot f}$$

buck and inverting mode

R = Inductor DC resistance

I_L = 10A for LT1170, 5A for LT1171, and 2.5A for LT1172

V_f = Output catch diode forward voltage at I_L

t = $0.6\mu\text{s}$, f = 100kHz switching frequency

Maximum input voltage can be increased by increasing R or V_f .

External current limiting such as that shown in AN19, Figure 39, will provide protection up to the full supply voltage rating. C1 in Figure 39 should be reduced to 200pF.

Transformer designs will tolerate much higher input voltages because leakage inductance limits rate of rise of current in the switch. These designs must be evaluated individually to assure that current limit is well controlled up to maximum input voltage.

Boost mode designs are never protected against output shorts because the external catch diode and inductor connect input to output.

PACKAGE/ORDER INFORMATION

<div><div>TOP VIEW</div><div><div><div><div>1</div><div>2</div><div>3</div><div>4</div></div><div><div>8</div><div>7</div><div>6</div><div>5</div></div></div><div><div>GND</div><div>V_C</div><div>FB</div><div>NC</div></div><div><div>E2</div><div>V_{SW}</div><div>E1</div><div>V_{IN}</div></div></div><div><div>J8 PACKAGE</div><div>N8 PACKAGE</div></div><div>8-LEAD CERAMIC DIP</div><div>8-LEAD PLASTIC DIP</div><div>S8 PACKAGE, 8-LEAD PLASTIC SOIC</div><div><div>$T_{JMAX} = 150^{\circ}\text{C}$, $\theta_{JA} = 100^{\circ}\text{C/W}$ (J)</div><div>$T_{JMAX} = 100^{\circ}\text{C}$, $\theta_{JA} = 130^{\circ}\text{C/W}$ (N)</div><div>$T_{JMAX} = 100^{\circ}\text{C}$, $\theta_{JA} = 120^{\circ}\text{C/W}$ (S)</div></div></div>	<div>ORDER PART NUMBER</div> <div>LT1172MJ8</div> <div>LT1172CJ8</div> <div>LT1172CN8</div> <div>LT1172IN8</div> <div>LT1172CS8</div> <div>LT1172IS8</div> <div>S8 PART MARKING</div> <div>1172</div> <div>1172I</div>																												
<div><div>BOTTOM VIEW</div><div><div><div>1</div><div>2</div><div>3</div><div>4</div></div><div><div>V_{SW}</div><div>V_C</div><div>V_{IN}</div><div>FB</div></div></div><div>CASE IS GND</div><div>K PACKAGE, 4-LEAD TO-3 METAL CAN</div><table><thead><tr><th></th><th>T_{JMAX}</th><th>θ_{JC}</th><th>θ_{JA}</th></tr></thead><tbody><tr><td>LT1170MK</td><td>150°C</td><td>2°C/W</td><td>35°C/W</td></tr><tr><td>LT1170CK</td><td>100°C</td><td>2°C/W</td><td>35°C/W</td></tr><tr><td>LT1171MK</td><td>150°C</td><td>4°C/W</td><td>35°C/W</td></tr><tr><td>LT1171CK</td><td>100°C</td><td>4°C/W</td><td>35°C/W</td></tr><tr><td>LT1172MK/LT1172HVMK</td><td>150°C</td><td>8°C/W</td><td>35°C/W</td></tr><tr><td>LT1172CK/LT1172HVCK</td><td>150°C</td><td>8°C/W</td><td>35°C/W</td></tr></tbody></table><div>Based on continuous operation. T_{JMAX} = 125°C for intermittent fault conditions.</div></div>		T _{JMAX}	θ _{JC}	θ _{JA}	LT1170MK	150°C	2°C/W	35°C/W	LT1170CK	100°C	2°C/W	35°C/W	LT1171MK	150°C	4°C/W	35°C/W	LT1171CK	100°C	4°C/W	35°C/W	LT1172MK/LT1172HVMK	150°C	8°C/W	35°C/W	LT1172CK/LT1172HVCK	150°C	8°C/W	35°C/W	<div>ORDER PART NUMBER</div> <div>LT1170MK</div> <div>LT1170CK</div> <div>LT1171MK</div> <div>LT1171CK</div> <div>LT1172MK</div> <div>LT1172CK</div>
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ELECTRICAL CHARACTERISTICS $V_{IN} = 15V$, $V_C = 0.5V$, $V_{FB} = V_{REF}$, output pin open, unless otherwise noted.

SYMBOL	PARAMETER	CONDITIONS			MIN	TYP	MAX	UNITS
V _{REF}	Reference Voltage	Measured at Feedback Pin V _C = 0.8V		●	1.224 1.214	1.244 1.244	1.264 1.274	V V
I _B	Feedback Input Current	V _{FB} = V _{REF}		●	350		750	nA nA
g _m	Error Amplifier Transconductance	ΔI _C = ±25μA		●	3000 2400	4400	6000 7000	μmho μmho
	Error Amplifier Source or Sink Current	V _C = 1.5V		●	150 120	200	350 400	μA μA
	Error Amplifier Clamp Voltage	Hi Clamp, V _{FB} = 1V Lo Clamp, V _{FB} = 1.5V			1.80 0.25	0.38	2.30 0.52	V V
	Reference Voltage Line Regulation	3V ≤ V _{IN} ≤ V _{MAX} V _C = 0.8V		●			0.03	%/V
A _V	Error Amplifier Voltage Gain	0.9V ≤ V _C ≤ 1.4V			500	800		V/V
	Minimum Input Voltage (Note 3)			●	2.6		3.0	V
I _O	Supply Current	3V ≤ V _{IN} ≤ V _{MAX} , V _C = 0.6V			6		9	mA
	Control Pin Threshold	Duty Cycle = 0		●	0.8 0.6	0.9	1.08 1.25	V V
	Normal/Flyback Threshold on Feedback Pin				0.4	0.45	0.54	V
V _{FB}	Flyback Reference Voltage (Note 3)	I _{FB} = 50μA		●	15.0 14.0	16.3	17.6 18.0	V V
	Change in Flyback Reference Voltage	0.05 ≤ I _{FB} ≤ 1mA			4.5	6.8	9	V
	Flyback Reference Voltage Line Regulation (Note 3)	I _{FB} = 50μA 7V ≤ V _{IN} ≤ V _{MAX}			0.01		0.03	%/V
	Flyback Amplifier Transconductance (g _m)	ΔI _C = ±10μA			150	300	500	μmho
	Flyback Amplifier Source and Sink Current	V _C = 0.6V I _{FB} = 50μA	Source Sink	● ●	15 25	32 40	70 70	μA μA
BV	Output Switch Breakdown Voltage	3V ≤ V _{IN} ≤ V _{MAX} , I _{SW} = 1.5mA	LT1170/LT1171/LT1172 LT1170HV/LT1171HV/LT1172HV LT1172S8	● ● ●	65 75 60	90 90 80		V V V
V _{SAT}	Output Switch "On" Resistance (Note 1)	LT1170 LT1171 LT1172		● ● ●	0.15 0.30 0.60		0.24 0.50 1.00	Ω Ω Ω
	Control Voltage to Switch Current Transconductance	LT1170 LT1171 LT1172			8 4 2			A/V A/V A/V
I _{LIM}	Switch Current Limit	(LT1170)	Duty Cycle = 50% Duty Cycle = 50% Duty Cycle = 80% (Note 2)	T _J ≥ 25°C T _J < 25°C ● ● ●	5 5 4	10		A A A
		(LT1171)	Duty Cycle = 50% Duty Cycle = 50% Duty Cycle = 80% (Note 2)	T _J ≥ 25°C T _J < 25°C ● ● ●	2.5 2.5 2.0	5.0		A A A
		(LT1172)	Duty Cycle = 50% Duty Cycle = 50% Duty Cycle = 80% (Note 2)	T _J ≥ 25°C T _J < 25°C ● ● ●	1.25 1.25 1.00	3.0		A A A

ELECTRICAL CHARACTERISTICS

$V_{IN} = 15V$, $V_C = 0.5V$, $V_{FB} = V_{REF}$, output pin open, unless otherwise noted.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
ΔI_{IN}	Supply Current Increase			25	35	mA/A
ΔI_{SW}	During Switch On-Time					
f	Switching Frequency		88	100	112	kHz
			85		115	kHz
DC _{MAX}	Maximum Switch Duty Cycle		80	90	95	%
	Shutdown Mode	$3V \leq V_{IN} \leq V_{MAX}$		100	250	μA
	Supply Current	$V_C = 0.05V$				
	Shutdown Mode	$3V \leq V_{IN} \leq V_{MAX}$	100	150	250	mV
	Threshold Voltage		50		300	mV
	Flyback Sense Delay Time (Note 3)			1.5		μs

The ● denotes the specifications which apply over the full operating temperature range.

$V_{MAX} = 40V$ for LT1170/71/72 and 60V for LT1170/71/72HV.

Note 1: Measured with V_C in hi clamp, $V_{FB} = 0.8V$. $I_{SW} = 4A$ for LT1170, 2A for LT1171, and 1A for LT1172.

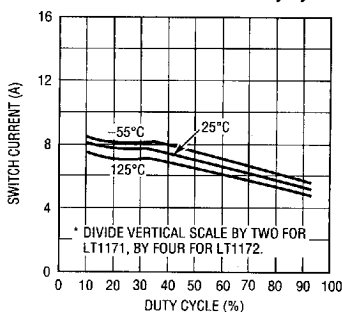
Note 2: For duty cycles (DC) between 50% and 80%, minimum

guaranteed switch current is given by $I_{LIM} = 3.33 (2 - DC)$ for the LT1170, $I_{LIM} = 1.67 (2 - DC)$ for the LT1171, and $I_{LIM} = 0.833 (2 - DC)$ for the LT1172.

Note 3: Minimum input voltage for isolated flyback mode is 7V. $V_{MAX} = 55V$ for HV grade in fully isolated mode to avoid switch breakdown.

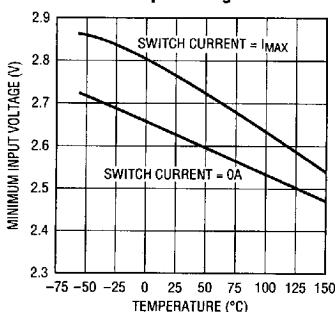
TYPICAL PERFORMANCE CHARACTERISTICS

Switch Current Limit vs Duty Cycle*



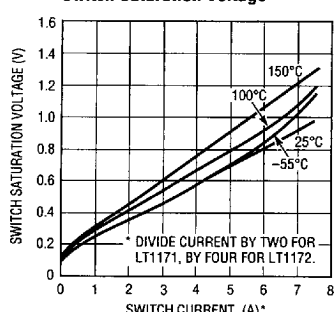
1170/71/2 501

Minimum Input Voltage



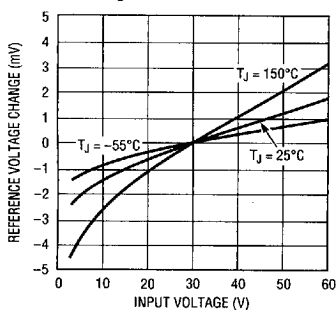
1170/71/2 002

Switch Saturation Voltage



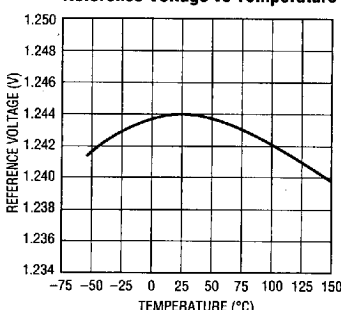
1170/71/2 603

Line Regulation



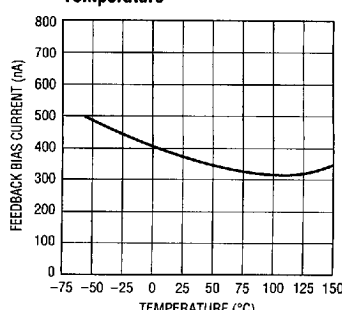
1170/71/2 504

Reference Voltage vs Temperature



1170/71/2 605

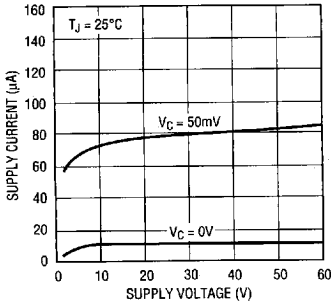
Feedback Bias Current vs Temperature



1170/71/2 006

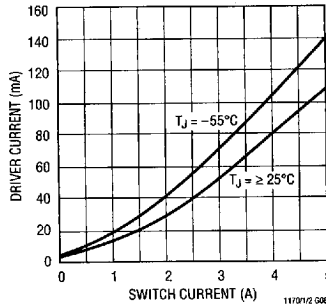
TYPICAL PERFORMANCE CHARACTERISTICS

**Supply Current vs Supply Voltage
(Shutdown Mode)**



1170/12 607

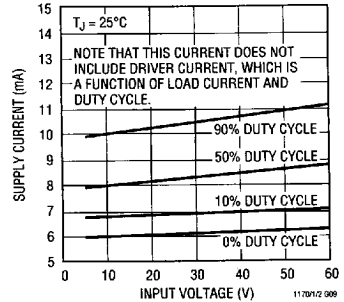
Driver Current* vs Switch Current



1170/12 008

* AVERAGE LT1170 POWER SUPPLY CURRENT IS FOUND BY MULTIPLYING DRIVER CURRENT BY DUTY CYCLE, THEN ADDING QUIESCENT CURRENT.

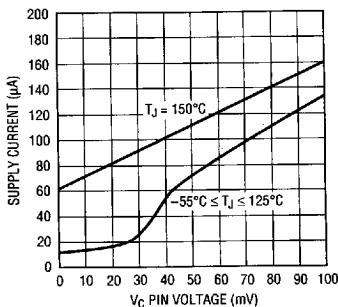
Supply Current vs Input Voltage*



1170/12 009

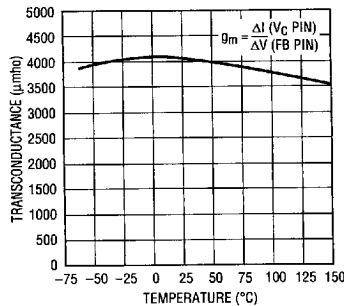
* UNDER VERY LOW OUTPUT CURRENT CONDITIONS, DUTY CYCLE FOR MOST CIRCUITS WILL APPROACH 10% OR LESS.

Shutdown Mode Supply Current



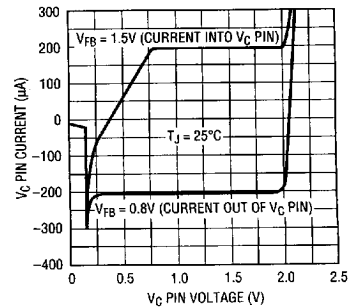
1170/12 010

Error Amplifier Transconductance



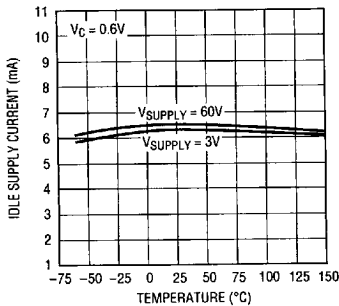
1170/12 011

Vc Pin Characteristics



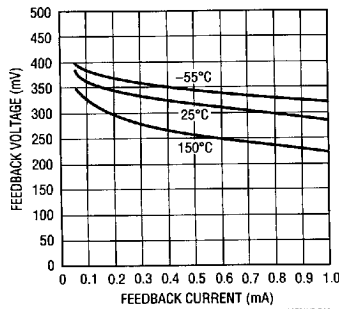
1170/12 012

Idle Supply Current vs Temperature



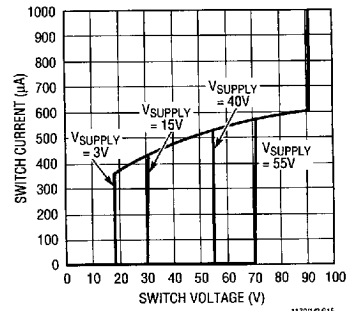
1170/12 013

Feedback Pin Clamp Voltage



1170/12 014

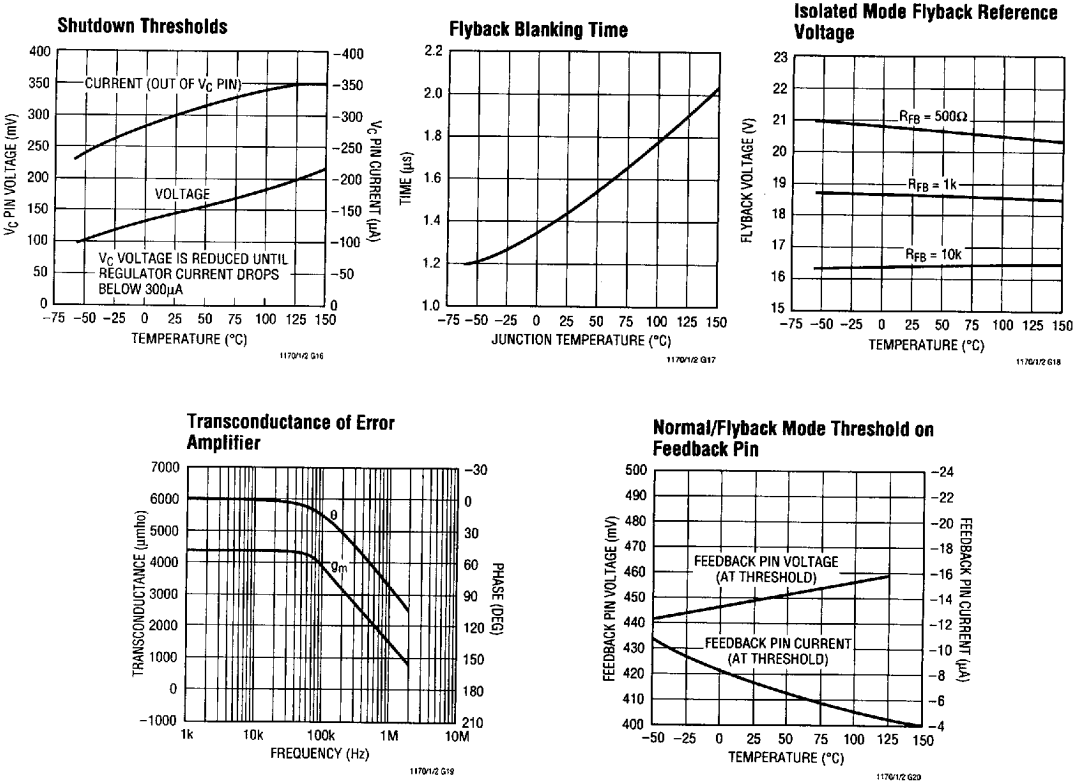
Switch "Off" Characteristics



1170/12 015



TYPICAL PERFORMANCE CHARACTERISTICS



11701281

A 1.2V bandgap reference biases the positive input of the error amplifier. The negative input is brought out for output voltage sensing. This feedback pin has a second

OPERATION

function; when pulled low with an external resistor, it programs the LT1170/LT1171/LT1172 to disconnect the main error amplifier output and connects the output of the flyback amplifier to the comparator input. The LT1170/LT1171/LT1172 will then regulate the value of the flyback pulse with respect to the supply voltage.* This flyback pulse is directly proportional to output voltage in the traditional transformer coupled flyback topology regulator. By regulating the amplitude of the flyback pulse, the output voltage can be regulated with no direct connection between input and output. The output is fully floating up to the breakdown voltage of the transformer windings. Multiple floating outputs are easily obtained with additional windings. A special delay network inside the LT1170/LT1171/LT1172 ignores the leakage inductance spike at the leading edge of the flyback pulse to improve output regulation.

The error signal developed at the comparator input is brought out externally. This pin (V_C) has four different functions. It is used for frequency compensation, current limit adjustment, soft starting, and total regulator shutdown. During normal regulator operation this pin sits at a voltage between 0.9V (low output current) and 2.0V (high output current). The error amplifiers are current output (g_m) types, so this voltage can be externally clamped for adjusting current limit. Likewise, a capacitor coupled external clamp will provide soft start. Switch duty cycle goes to zero if the V_C pin is pulled to ground through a diode, placing the LT1170/LT1171/LT1172 in an idle mode. Pulling the V_C pin below 0.15V causes total regulator shutdown, with only 50 μ A supply current for shutdown circuitry biasing. See AN19 for full application details.

Extra Pins on the MiniDIP and Surface Mount Packages

The 8- and 16-pin versions of the LT1172 have the emitters of the power transistor brought out separately from the ground pin. This eliminates errors due to ground pin voltage drops and allows the user to reduce switch current limit 2:1 by leaving the second emitter (E2) disconnected. The first emitter (E1) should always be connected to the ground pin. Note that switch "on" resistance doubles when E2 is left open, so efficiency will suffer somewhat

when switch currents exceed 300mA. Also, note that chip dissipation will actually *increase* with E2 open during normal load operation, even though dissipation in current limit mode will *decrease*. See "Thermal Considerations" next.

Thermal Considerations When Using the MiniDIP and SOL Packages

The low supply current and high switch efficiency of the LT1172 allow it to be used without a heat sink in most applications when the TO-220 or TO-3 package is selected. These packages are rated at 50°C/W and 35°C/W respectively. The miniDIPs, however, are rated at 100°C/W in ceramic (J) and 130°C/W in plastic (N).

Care should be taken for miniDIP applications to ensure that the worst case input voltage and load current conditions do not cause excessive die temperatures. The following formulas can be used as a rough guide to calculate LT1172 power dissipation. For more details, the reader is referred to Application Note 19 (AN19), "Efficiency Calculations" section.

Average supply current (including driver current) is:

$$I_{IN} \approx 6\text{mA} + I_{SW}(0.004 + \text{DC}/40)$$

I_{SW} = switch current

DC = switch duty cycle

Switch power dissipation is given by:

$$P_{SW} = (I_{SW})^2 \cdot R_{SW} \cdot \text{DC}$$

R_{SW} = LT1172 switch "on" resistance (1 Ω maximum)

Total power dissipation is the sum of supply current times input voltage plus switch power:

$$P_{D(TOT)} = (I_{IN})(V_{IN}) + P_{SW}$$

In a typical example, using a boost converter to generate 12V at 0.12A from a 5V input, duty cycle is approximately 60%, and switch current is about 0.65A, yielding:

$$I_{IN} = 6\text{mA} + 0.65(0.004 + \text{DC}/40) = 18\text{mA}$$

$$P_{SW} = (0.65)^2 \cdot 1\Omega \cdot (0.6) = 0.25\text{W}$$

$$P_{D(TOT)} = (5\text{V})(0.018\text{A}) + 0.25 = 0.34\text{W}$$

*See note under block diagram.

OPERATION

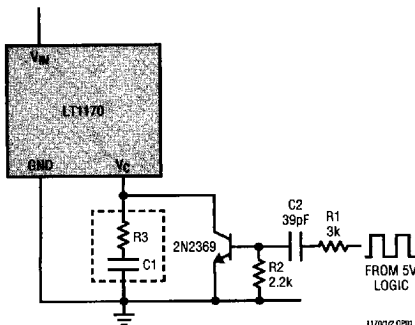
Temperature rise in a plastic miniDIP would be $130^{\circ}\text{C}/\text{W}$ times 0.34W , or approximately 44°C . The maximum ambient temperature would be limited to 100°C (commercial temperature limit) minus 44°C , or 56°C .

In most applications, full load current is used to calculate die temperature. However, if overload conditions must also be accounted for, four approaches are possible. First, if loss of regulated output is acceptable under overload conditions, the internal *thermal limit* of the LT1172 will protect the die in most applications by shutting off switch current. *Thermal limit is not a tested parameter*, however, and should be considered only for noncritical applications with temporary overloads. A second approach is to use the larger TO-220 (T) or TO-3 (K) package which, even without a heat sink, may limit die temperatures to safe levels under overload conditions. In critical situations, heat sinking of these packages is required; especially if overload conditions must be tolerated for extended periods of time.

The third approach for lower current applications is to leave the second switch emitter (miniDIP only) open. This increases switch "on" resistance by 2:1, but reduces switch current limit by 2:1 also, resulting in a net 2:1 reduction in I^2R switch dissipation under current limit conditions.

The fourth approach is to clamp the V_C pin to a voltage less than its internal clamp level of 2V. The LT1172 switch current limit is zero at approximately 1V on the V_C pin and 2A at 2V on the V_C pin. Peak switch current can be externally clamped between these two levels with a diode. See AN19 for details.

Synchronizing with Bipolar Transistor



LT1170/LT1171/LT1172 Synchronizing

The LT1170/LT1171/LT1172 can be externally synchronized in the frequency range of 120kHz to 160kHz. This is accomplished as shown in the accompanying figures. Synchronizing occurs when the V_C pin is pulled to ground with an external transistor. To avoid disturbing the DC characteristics of the internal error amplifier, the width of the synchronizing pulse should be under $0.3\mu\text{s}$. C_2 sets the pulse width at $\approx 0.2\mu\text{s}$. The effect of a synchronizing pulse on the LT1170/LT1171/LT1172 amplifier offset can be calculated from:

$$\Delta V_{OS} = \frac{\left(\frac{KT}{q}\right)(t_s)(f_s)\left(I_C + \frac{V_C}{R_3}\right)}{I_C}$$

$$\frac{KT}{q} = 26\text{mV at } 25^{\circ}\text{C}$$

t_s = pulse width

f_s = pulse frequency

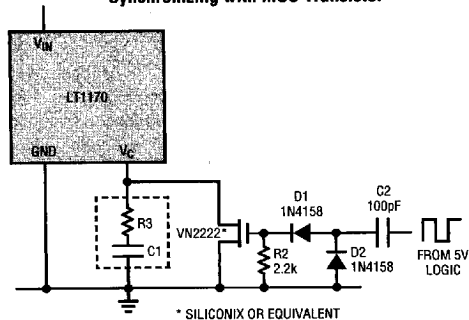
I_C = V_C source current ($\approx 200\mu\text{A}$)

V_C = operating V_C voltage (1V to 2V)

R_3 = resistor used to set mid-frequency "zero" in frequency compensation network.

With $t_s = 0.2\mu\text{s}$, $f_s = 150\text{kHz}$, $V_C = 1.5\text{V}$, and $R_3 = 2\text{k}$, offset voltage shift is $\approx 3.8\text{mV}$. This is not particularly bothersome, but note that high offsets could result if R_3 were reduced to a much lower value. Also, the synchronizing transistor must sink higher currents with low values of R_3 , so larger drives may have to be used. The transistor must be capable of pulling the V_C pin to within 200mV of ground to ensure synchronizing.

Synchronizing with MOS Transistor

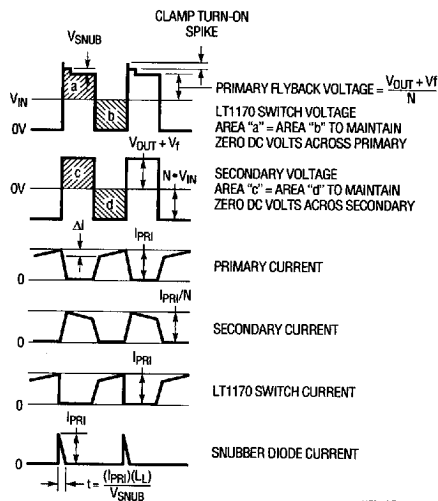
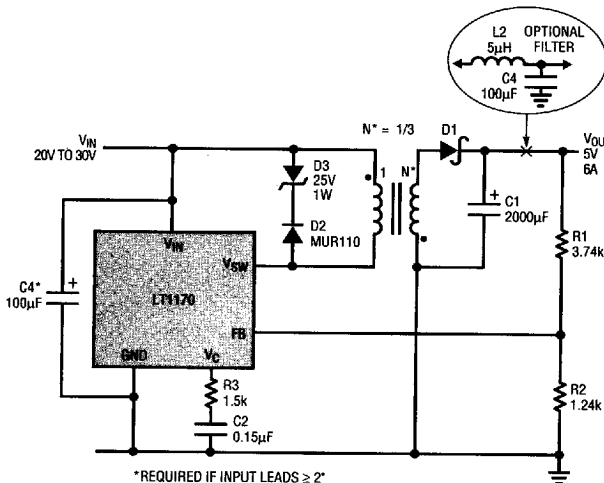


* SILICONIX OR EQUIVALENT

1170/1172 01R2

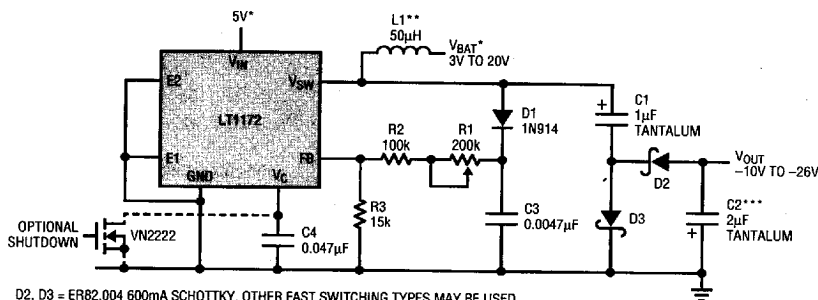
TYPICAL APPLICATIONS

Flyback Converter



1170/1172 TA03

LCD Contrast Supply



D2, D3 = ER82.004 600mA SCHOTTKY. OTHER FAST SWITCHING TYPES MAY BE USED.

* V_{IN} AND BATTERY MAY BE TIED TOGETHER. MAXIMUM VALUE FOR V_{BAT} IS EQUAL TO THE [NEGATIVE OUTPUT] + 1V. WITH HIGHER BATTERY VOLTAGES, HIGHEST EFFICIENCY IS OBTAINED BY RUNNING THE LT1172 V_{IN} PIN FROM 5V. SHUTTING OFF THE 5V SUPPLY WILL AUTOMATICALLY TURN OFF THE LT1172. EFFICIENCY IS ABOUT 80% AT $I_{OUT} = 25mA$.

R1, R2, R3 ARE MADE LARGE TO MINIMIZE BATTERY DRAIN IN SHUTDOWN, WHICH IS APPROXIMATELY $V_{BAT} / (R1 + R2 + R3)$.

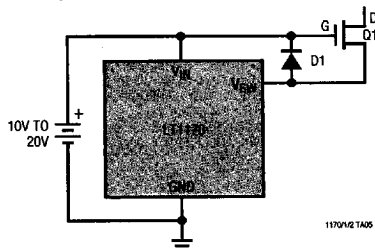
** FOR HIGH EFFICIENCY, L1 SHOULD BE MADE ON A FERRITE OR MOLYPERMALLOY CORE. PEAK INDUCTOR CURRENTS ARE ABOUT 600mA AT $P_{OUT} = 0.752$. INDUCTOR SERIES RESISTANCE SHOULD BE LESS THAN 0.4Ω FOR HIGH EFFICIENCY.

*** OUTPUT RIPPLE IS ABOUT 200mVp-p TO 400mVp-p WITH $C2 = 2\mu F$ TANTALUM. IF LOWER RIPPLE IS DESIRED, INCREASE C2, OR ADD A 10Ω , $1\mu F$ TANTALUM OUTPUT FILTER.

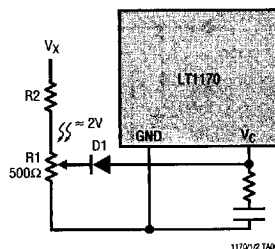
1170/1172 TA04

TYPICAL APPLICATIONS (Note that maximum output currents are divided by 2 for LT1171, by 4 for LT1172.)

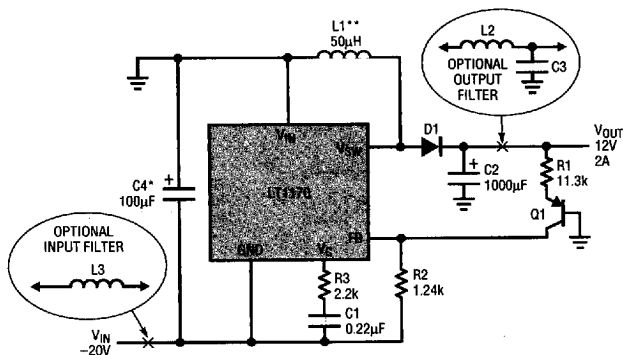
Driving High Voltage FET
(for Off-Line Applications, See AN25)



External Current Limit



Negative-to-Positive Buck-Boost Converter†

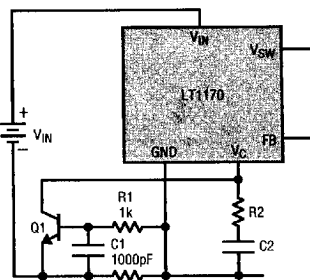


* REQUIRED IF INPUT LEADS $\geq 2^\circ$

** PULSE ENGINEERING 92114, COILTRONICS 50-2-52

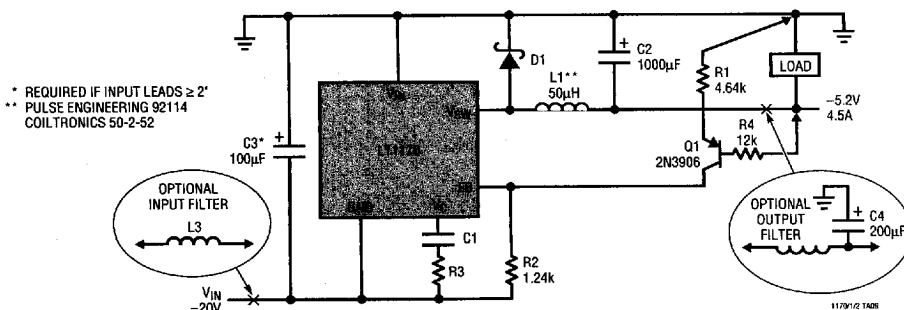
† THIS CIRCUIT IS OFTEN USED TO CONVERT -48V TO 5V . TO GUARANTEE FULL SHORT-CIRCUIT PROTECTION, THE CURRENT LIMIT CIRCUIT SHOWN IN AN19, FIGURE 39, SHOULD BE ADDED WITH $C1$ REDUCED TO 200pF .

External Current Limit



NOTE THAT THE LT1170 GND PIN IS NO LONGER COMMON TO V_{IN} .

Negative Buck Converter

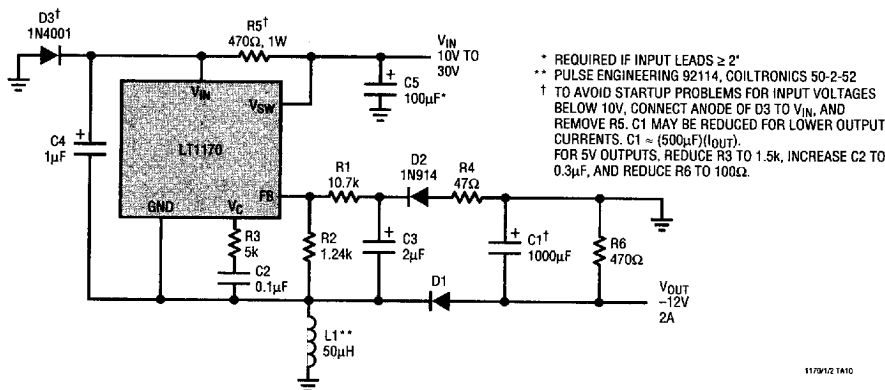


* REQUIRED IF INPUT LEADS $\geq 2^\circ$

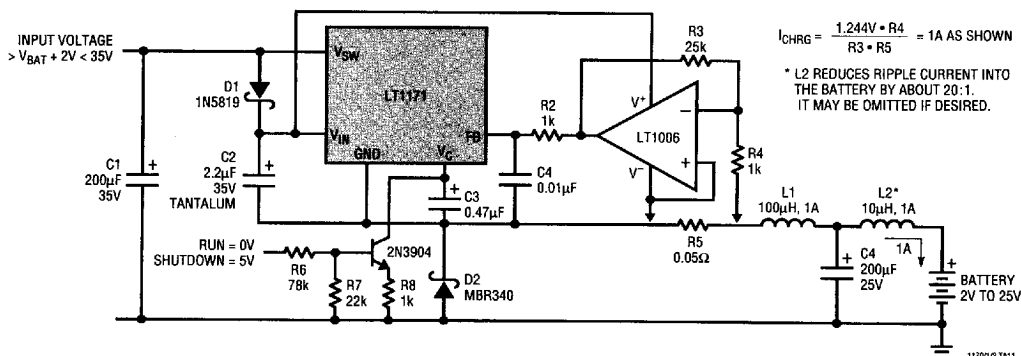
** PULSE ENGINEERING 92114
COILTRONICS 50-2-52

TYPICAL APPLICATIONS

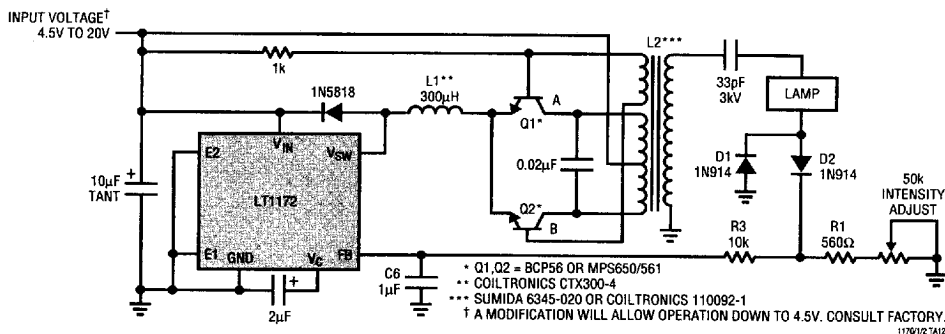
Positive-to-Negative Buck-Boost Converter



High Efficiency Constant Current Charger

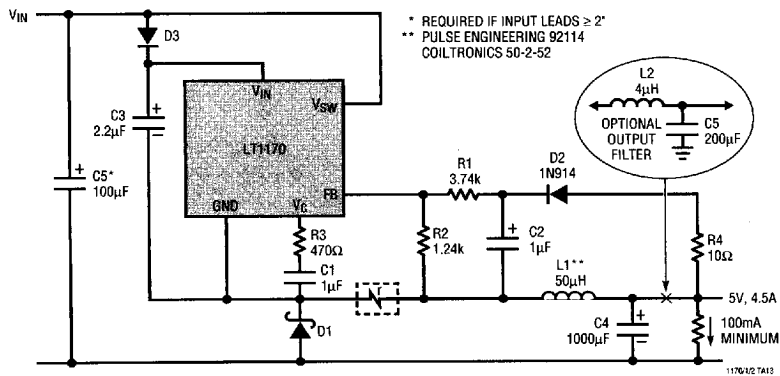


Backlight CCFL Supply (see AN45 for details)

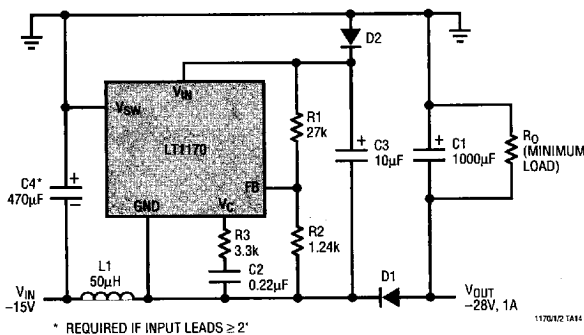


TYPICAL APPLICATIONS

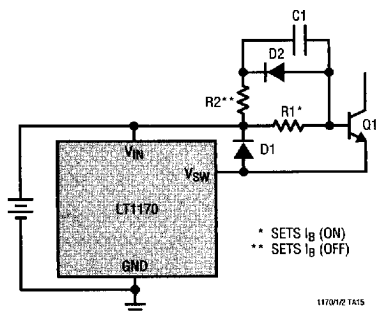
Positive Buck Converter



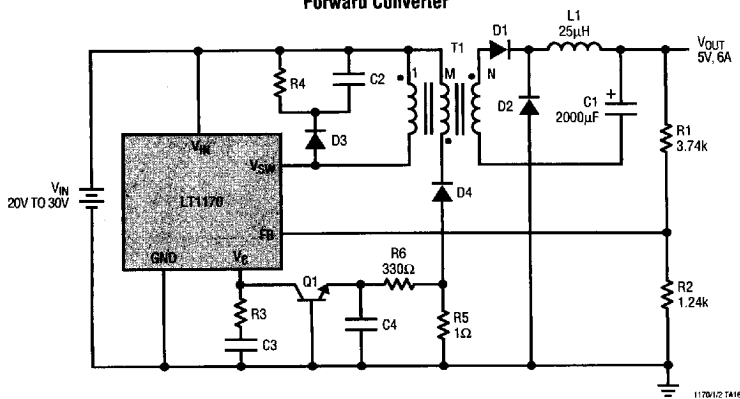
Negative Boost Regulator



Driving High Voltage NPN

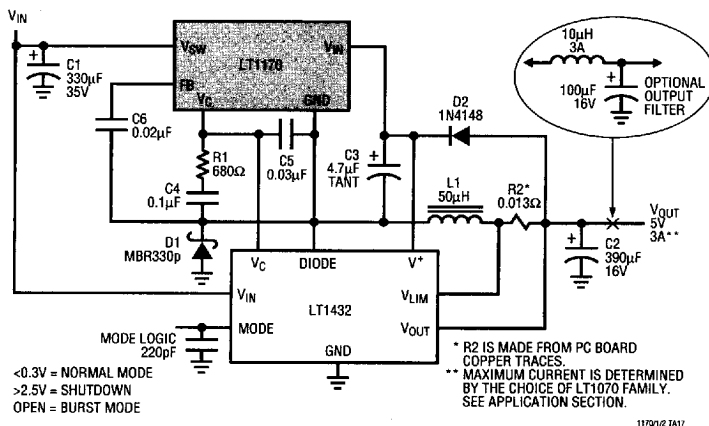


Forward Converter



TYPICAL APPLICATIONS

High Efficiency 5V Buck Converter



Positive Current Boosted Buck Converter

